

## Microwave Wideband Synthesizer with Integrated VCO and Deterministic General-Purpose Pulse Retimer

### FEATURES

- ▶ Output frequency range: 800 MHz to 12.8 GHz
- ▶ Jitter = 18 fs<sub>RMS</sub> (integration bandwidth: 100 Hz to 100 MHz)
- ▶ Jitter = 27 fs<sub>RMS</sub> (ADC SNR method)
- ▶ Wideband noise floor: -160 dBc/Hz at 12 GHz
- ▶ Retimed LVDS SYSREF output
- ▶ General-purpose pulse retimer for SYSREF, SYNC, and MCS applications
- ▶ PLL specifications
  - ▶ -239 dBc/Hz: normalized in-band phase noise floor
  - ▶ -147 dBc/Hz: normalized in-band 1/f phase noise floor
  - ▶ Phase detector frequency up to 500 MHz
  - ▶ Reference input frequency up to 1000 MHz
  - ▶ Typical spurious f<sub>PFD</sub>: -95 dBc PFD at f<sub>OUT</sub> = 12 GHz
- ▶ Reference input to output delay specifications
  - ▶ Device-to-device standard deviation: 3 ps
  - ▶ Temperature coefficient: 0.03 ps/°C
  - ▶ Adjustment step size: < ±0.1 ps
- ▶ Multichip output phase alignment
- ▶ 3.3 V and 5 V power supplies
- ▶ Available in 48-lead, 7 mm × 7 mm LGA package

### APPLICATIONS

- ▶ High performance data converter and MxFE clocking
- ▶ Wireless infrastructure (MC-GSM, 5G)
- ▶ Test and measurement
- ▶ FPGA with integrated data converters

### GENERAL DESCRIPTION

The ADF4378 is a high performance, ultra-low jitter, integer-N phased locked loop (PLL) with an integrated voltage controlled oscillator (VCO) and system reference (SYSREF) retimer ideally suited for data converter and mixed signal front end (MxFE) clock applications. The high performance PLL has a -239 dBc/Hz: normalized in-band phase noise floor, ultra-low 1/f noise, and a high phase/frequency detector (PFD) frequency that can achieve ultra-low in-band noise and integrated jitter. The fundamental VCO and output divider of the ADF4378 generate frequencies from 800 MHz to 12.8 GHz. The ADF4378 integrates all necessary power-supply bypass capacitors, which saves board space on compact boards.

For multiple data converter and MxFE clock applications, the ADF4378 simplifies clock alignment and calibration routines required with other clock solutions by implementing the automatic reference to output synchronization feature, the matched reference to output delays across process, voltage, and temperature feature, and the less than ±0.1 ps, jitter free reference to output delay adjustment capability feature.

The general-purpose pulse retimer feature allows for predictable and precise multichip clock and pulse alignment for SYSREF, SYNC, and multichip synchronization (MCS) architectures. JESD204B and JESD204C Subclass 1 solutions are supported by pairing the ADF4378 with an integrated circuit (IC) that distributes pairs of reference and SYSREF signals. The pulse retimer feature simplifies the system design by allowing the widely distributed SYSREF to only meet the slower reference frequency timing vs. the much more stringent output clock timing. Serial-peripheral interface (SPI) selectable current-mode logic (CML)/low-voltage positive/pseudo emitter-coupled logic (LVPECL) or low-voltage differential signaling (LVDS) SYSREF input and LVDS SYSREF output allow CML to LVDS signal conversion, which simplifies clock and SYSREF alignment for various converters. The pulse retimer feature also can be used with transceiver MCS signals and SYNC signals for other ICs.

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**REVISION HISTORY****12/2023—Revision 0: Initial Version**

FUNCTIONAL BLOCK DIAGRAM

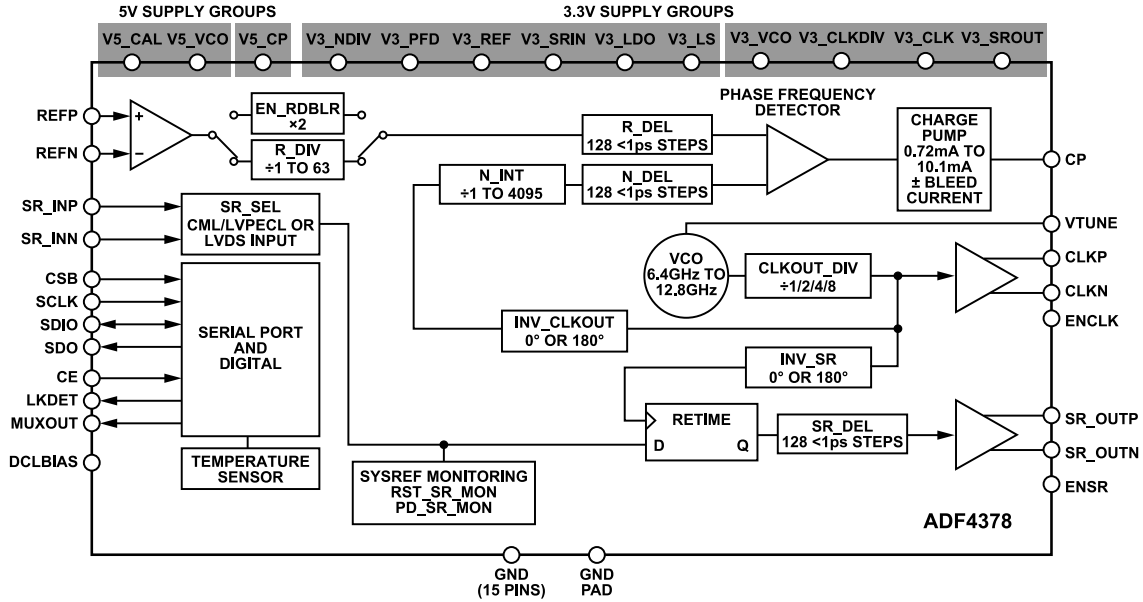


Figure 1. ADF4378 Functional Block Diagram

## SPECIFICATIONS

3.3 V Supply Group 1 pins voltage ( $V_{3.3V_1}$ ) = 3.15 V to 3.45 V, Supply Group 2 pins voltage ( $V_{3.3V_2}$ ) = 3.15 V to 3.45 V,  $V_{V5\_VCO} = V_{V5\_CP} = V_{V5\_CAL} = 4.75$  V to 5.25 V, all voltages are with respect to GND,  $T_A = -40^\circ\text{C}$  to  $+105^\circ\text{C}$ , operating temperature range, unless otherwise noted.

Table 1. Specifications

Parameter	Symbol	Min	Typ	Max	Unit	Test Conditions/Comments
REFERENCE INPUTS (REFP, REFN)						
Input Frequency	$f_{REF}$	10		1000	MHz	Non-SYSREF applications
		10		500	MHz	SYSREF applications
Input Signal Level	$V_{REF}$	0.5		2.6	V p-p	See Figure 66
Minimum Input Slew Rate			100		V/ $\mu\text{s}$	
Input Duty Cycle			50		%	
Self-Bias Voltage			1.85		V	
Input Resistance			3		k $\Omega$	Differential
Input Capacitance			1		pF	Differential
Input Current			-2		$\mu\text{A}$	
REFERENCE PEAK DETECTOR						
Input Frequency		10		1000	MHz	
Minimum Input Signal Detected (REF_OK Bit = 1)			200		mV p-p	$f_{REF} = 100$ MHz, single-ended sine wave
Maximum Input Signal Not Detected (REF_OK Bit = 0)			160		mV p-p	$f_{REF} = 100$ MHz, single-ended sine wave
REFERENCE DIVIDER						
R		1		63		Non-SYSREF applications, all integers included
		1		1		SYSREF applications
REFERENCE DOUBLER						
Input Frequency		10		250	MHz	EN_RDBLR = 1
PHASE/FREQUENCY DETECTOR (PFD)						
Input Frequency	$f_{PFD}$	3		500	MHz	
SYSREF INPUTS (SR_INP, SR_INN)						
Input Frequency	$f_{SR\_IN}$	DC		125	MHz	$f_{REF} \div f_{SR\_IN}$ must be an even integer
Input Signal Level	$V_{SR\_IN}$	0.4		2.6	V p-p	SR_SEL = 0, $f_{SR\_IN} = 10$ MHz
		0.4		2.6	V p-p	SER_SEL = 1, $f_{SR\_IN} = 10$ MHz
Self-Bias Voltage (AC-Coupled)	$V_{CM}$		1.85		V	SR_SEL = 0, $f_{SR\_IN} = 10$ MHz
			1.3		V	SR_SEL = 1, $f_{SR\_IN} = 10$ MHz
Input Common Mode Voltage Range (DC-Coupled)	$V_{CM}$	1.4		3.1	V	SR_SEL = 0, $f_{SR\_IN} = 10$ MHz, $V_{SR\_IN} = 0.8$ V p-p
		0.5		1.6	V	SR_SEL = 1, $f_{SR\_IN} = 10$ MHz, $V_{SR\_IN} = 0.8$ V p-p
Input Resistance			3		k $\Omega$	Differential
Input Capacitance			1		pF	Differential
Input Current			-2		$\mu\text{A}$	
SYSREF to Reference Setup Time		400			ps	$V_{CM}$ set to self-bias voltage, V p-p = 0.8 V p-p
SYSREF to Reference Hold Time		600			ps	$V_{CM}$ set to self-bias voltage, V p-p = 0.8 V p-p
SYSREF Monitor Window Around Metastability State			$\pm 190$		ps	
CHARGE PUMP (CP)						
Output Current Range	$I_{CP}$		0.79 to 11.1		mA	Set by CP_I bit fields
Output Current Source/Sink Accuracy			$\pm 2$		%	All CP_I bit field settings, $V_{CP} = V_{V5\_CP}/2$
Output Current Source/Sink Matching			$\pm 2$		%	All CP_I bit field settings, $V_{CP} = V_{V5\_CP}/2$
Output Current vs. Output Voltage Sensitivity			0.2		%/V	$V_{CP}^1$
Output Current vs. Temperature			280		ppm/ $^\circ\text{C}$	$V_{CP} = V_{V5\_CP}/2$

## SPECIFICATIONS

Table 1. Specifications (Continued)

Parameter	Symbol	Min	Typ	Max	Unit	Test Conditions/Comments
Output High-Z Leakage Current			-0.01 -0.3		$\mu\text{A}$ $\mu\text{A}$	Minimum $I_{CP}$ , $V_{CP}^1$ Maximum $I_{CP}$ , $V_{CP}^1$
VCO						
Frequency Range	$f_{VCO}$	6.4		12.8	GHz	
Tuning Sensitivity	$K_{VCO}$		0.75 to 1.25		%Hz/V	$K_{VCO}^{2,3}$
VCO Calibration Frequency	$f_{DIV\_RCLK}$			125	MHz	Must set $DCLK\_MODE = 1$ , when $f_{DIV\_RCLK} > 80$ MHz
FEEDBACK DIVIDER (N) AND CLOCK OUTPUT DIVIDER (O)						
N		2		4095		All integers included
O		1		8		1, 2, 4, 8
CLOCK OUTPUT (CLKP and CLKN)						Differential termination = 100 $\Omega$ for all clock output specifications unless noted
Output Frequency	$f_{OUT}$	0.8		12.8	GHz	
Output Differential Voltage	$V_{OD}$		320		mV	$V_{OH} - V_{OL}$ measurement across a differential pair with output driver not toggling and $CLKOUT\_OP = 0$
			420		mV	$V_{OH} - V_{OL}$ measurement across a differential pair with output driver not toggling and $CLKOUT\_OP = 1$
			530		mV	$V_{OH} - V_{OL}$ measurement across a differential pair with output driver not toggling and $CLKOUT\_OP = 2$
			640		mV	$V_{OH} - V_{OL}$ measurement across a differential pair with output driver not toggling and $CLKOUT\_OP = 3$
Output Resistance			100		$\Omega$	Differential
Output Common Mode			$V_{CLK} - 1.2 \times V_{OD}$		V	
Output Rise Time	$t_R$		15		ps	20% to 80%, $CLKOUT\_OP = 1$
Output Fall Time	$t_F$		15		ps	80% to 20%, $CLKOUT\_OP = 1$
Output Duty Cycle			50		%	
SYSREF OUTPUT (SR_OUTP and SR_OUTN)						Differential termination = 100 $\Omega$ for all SYSREF output specifications unless noted
Output Frequency		DC		125	MHz	
Output Differential Voltage			0.85		V p-p	
Output Resistance			100		$\Omega$	Differential
Output Common Mode			1.2		V	
Output Rise Time			20		ps	Differential
Output Fall Time			30		ps	Differential
Output Duty Cycle			50		%	
REFERENCE INPUT TO OUTPUT DELAY						Device setup <sup>4</sup> for all delay specifications unless noted, measure rising reference edge at REF input to rising edge at CLK1 output
Propagation Delay Temperature Coefficient	$t_{PD-TC}$		0.03		ps/ $^{\circ}\text{C}$	$REF\_SEL = 0$
Propagation Delay	$t_{PD}$		104		ps	$f_{OUT} = 12$ GHz, $f_{REF} = 200$ MHz, $f_{PFD} = 200$ MHz, $R\_DIV = 1$ , $REF\_SEL = 0$
			112		ps	$f_{OUT} = 6$ GHz, $f_{REF} = 200$ MHz, $f_{PFD} = 200$ MHz, $R\_DIV = 1$ , $REF\_SEL = 0$

## SPECIFICATIONS

Table 1. Specifications (Continued)

Parameter	Symbol	Min	Typ	Max	Unit	Test Conditions/Comments
			110		ps	$f_{OUT} = 3 \text{ GHz}$ , $f_{REF} = 200 \text{ MHz}$ , $f_{PFD} = 200 \text{ MHz}$ , $R\_DIV = 1$ , $REF\_SEL = 0$
			110		ps	$f_{OUT} = 1.6 \text{ GHz}$ , $f_{REF} = 200 \text{ MHz}$ , $f_{PFD} = 200 \text{ MHz}$ , $R\_DIV = 1$ , $REF\_SEL = 0$
			122		ps	$f_{OUT} = 3 \text{ GHz}$ , $f_{REF} = 100 \text{ MHz}$ , $f_{PFD} = 200 \text{ MHz}$ , $EN\_RDBLR = 1$ , $REF\_SEL = 0$
N_DEL, R_DEL Step Size			1		ps	
N_DEL Range			105		ps	$N\_DEL = 127$ , $R\_DEL = 0$
R_DEL Range			127		ps	$N\_DEL = 0$ , $R\_DEL = 127$
SYSREF OUTPUT-TO-CLOCK OUTPUT DELAY						Device setup <sup>5</sup> for all delay specifications unless noted, measure the rising edge at CLK output to the rising edge at SYSREF output
SR_DEL Step Size			0.8		ps	
SR_DEL Range			110		ps	
LOGIC INPUTS (CSB, SCLK, SDIO, ENCLK, and ENSR)						
Input High Voltage	$V_{INH}$	1.2			V	
Input Low Voltage	$V_{INL}$			0.6	V	
Input Current (High, Low)	$I_{IH}/I_{IL}$			$\pm 1$	$\mu\text{A}$	
Input Capacitance (CSB, SCLK, ENCLK, ENSR)	$C_{IN}$		1		pF	
SDIO	$C_{IN-SDIO}$		2		pF	
LOGIC INPUT (CE Pin)						
Input High Voltage	$V_{INH-CE}$	1.8			V	
Input Low Voltage	$V_{INL-CE}$			0.8	V	
Input Current (High, Low)	$I_{IH-CE}/I_{IL-CE}$			$\pm 1$	$\mu\text{A}$	
Input Capacitance	$C_{IN-CE}$		1		pF	
LOGIC OUTPUTS (SDIO, SDO, LKDET, MUXOUT)						
Output High Voltage (1.8 V Mode)	$V_{OH}$	1.5	1.8		V	$I_{OH} = 500 \mu\text{A}$ , 1.8 V output selected (default setting)
Output High Voltage (3.3 V Mode)	$V_{OH-3V}$	$V_{3.3V} - 0.4$			V	$I_{OH} = 500 \mu\text{A}$ , 3.3 V output selected, set by voltage on V3_LDO pin
Output Low Voltage	$V_{OL}$			0.4	V	$I_{OL} = 500 \mu\text{A}$
SDO High-Z Leakage	$I_{ZH}/I_{ZL}$			$\pm 1$	$\mu\text{A}$	
POWER SUPPLIES						Device setup <sup>6</sup> for all supply current specifications, unless noted
V5_VCO Supply Range	$V_{V5\_VCO}$	4.75	5	5.25	V	
V5_CAL Supply Range	$V_{V5\_CAL}$	4.75	5	5.25	V	
V5_CP Supply Range	$V_{V5\_CP}$	4.75	5	5.25	V	
V <sub>3.3V_1</sub> Supply Range	$V_{3.3V\_1}$	3.15	3.3	3.45	V	3.3 V Power Supply Group 1 (V3_LS, V3_LDO, V3_REF, V3_PFD, V3_NDIV, V3_SRIN)
V <sub>3.3V_2</sub> Supply Range	$V_{3.3V\_2}$	3.15	3.3	3.45	V	3.3 V Power Supply Group 2 (V3_CLK, V3_SROUT, V3_VCO, V3_CLKDIV)
V5_VCO Supply Current	$I_{V5\_VCO}$		90	135	$\text{mA}$	$f_{OUT} = 12.8 \text{ GHz}$
			170	220	$\text{mA}$	$f_{OUT} = 6.4 \text{ GHz}$ , $CLKOUT\_DIV = 0$
V5_CAL Supply Current	$I_{V5\_CAL}$		50	160	$\mu\text{A}$	
			8		$\text{mA}$	During VCO calibration
V5_CP Supply Current	$I_{V5\_CP}$		55	65	$\text{mA}$	CP current ( $I_{CP}$ ) = 11.1 mA, $CP\_I = 15$
			26		$\text{mA}$	$I_{CP} = 0.79 \text{ mA}$ , $CP\_I = 0$

## SPECIFICATIONS

Table 1. Specifications (Continued)

Parameter	Symbol	Min	Typ	Max	Unit	Test Conditions/Comments
V <sub>3.3V_1</sub> Supply Current	I <sub>3.3V_1</sub>		55.2		mA	CP_1 = 15, EN_BLEED = 1, BLEED_[1:0] = 512
			170	205	mA	ENSR = low
			170		mA	ENSR = low, R_DEL = 127
			174		mA	ENSR = low, REF_SEL = BST_REF = FILT_REF = 1
			170		mA	ENSR = low, PD_RDET = 1
			204		mA	ENSR = high, REF_SEL = 0
			215		mA	During VCO calibration, EN_DRCLK = EN_DNCLK = EN_ADC_CLK = 1
V <sub>3.3V_2</sub> Supply Current	I <sub>3.3V_2</sub>		153		mA	CLKOUT_OP = 0, ENSR = 0 CLKOUT_DIV = 3
			212		mA	CLKOUT_OP = 0, ENSR = high
			217		mA	CLKOUT_OP = 1, ENSR = high
			221		mA	CLKOUT_OP = 2, ENSR = high
			226		mA	CLKOUT_OP = 3, ENSR = high
			128	160	mA	CLKOUT_OP = 0, ENSR = low
Typical Power Dissipation	P <sub>DIS</sub>		2.22		W	ENSR = high, V <sub>3.3V_1</sub> = V <sub>3.3V_2</sub> = 3.3 V, V <sub>V5_VCO</sub> = 5 V, VCO Core 2 and Core 3
			2.05		W	ENSR = low, V <sub>3.3V_1</sub> = V <sub>3.3V_2</sub> = 3.3 V, V <sub>V5_VCO</sub> = 5 V, VCO Core 0 and Core 1
Typical Power-Down Current						
3.3 V Supplies			11	15	mA	PD_ALL = 1, I <sub>3.3V_1</sub> + I <sub>3.3V_2</sub>
5 V Supplies			350	750	μA	PD_ALL = 1, I <sub>V5_VCO</sub> + I <sub>V5_CAL</sub> + I <sub>V5_CP</sub>
Typical Disable Current						
3.3 V Supplies			0.1	1.5	mA	CE = low, I <sub>3.3V_1</sub> + I <sub>3.3V_2</sub>
5 V Supplies			350	750	μA	CE = low, I <sub>V5_VCO</sub> + I <sub>V5_CAL</sub> + I <sub>V5_CP</sub>
<b>CLOCK OUTPUT NOISE CHARACTERISTICS</b>						
12 GHz Output Frequency						Device setup <sup>7</sup> , f <sub>OUT</sub> = 12 GHz
Phase Noise Floor			-160		dBc/Hz	
RMS Jitter						
12 kHz to 20 MHz Integration			17.6		f <sub>RMS</sub>	
100 Hz to 100 MHz Integration			18		f <sub>RMS</sub>	
Equivalent ADC SNR Method <sup>8</sup>			27		f <sub>RMS</sub>	
10 GHz Output Frequency						Device setup <sup>7</sup> , f <sub>OUT</sub> = 10 GHz
Phase Noise Floor			-159.5		dBc/Hz	
RMS Jitter						
12 kHz to 20 MHz Integration			18.5		f <sub>RMS</sub>	
100 Hz to 100 MHz Integration			18.7		f <sub>RMS</sub>	
Equivalent ADC SNR Method <sup>8</sup>			30		f <sub>RMS</sub>	
8 GHz Output Frequency						Device setup <sup>7</sup> , f <sub>OUT</sub> = 8 GHz
Phase Noise Floor			-160.5		dBc/Hz	
RMS Jitter						
12 kHz to 20 MHz Integration			18		f <sub>RMS</sub>	
100 Hz to 100 MHz Integration			18.3		f <sub>RMS</sub>	
Equivalent ADC SNR Method <sup>8</sup>			30		f <sub>RMS</sub>	
6 GHz Output Frequency						Device setup <sup>7</sup> , f <sub>OUT</sub> = 6 GHz
Phase Noise Floor			-163		dBc/Hz	
RMS Jitter						

## SPECIFICATIONS

Table 1. Specifications (Continued)

Parameter	Symbol	Min	Typ	Max	Unit	Test Conditions/Comments
12 kHz to 20 MHz Integration			17.7		f <sub>RMS</sub>	Device setup <sup>7</sup> , f <sub>OUT</sub> = 3 GHz
100 Hz to 100 MHz Integration			18.3		f <sub>RMS</sub>	
Equivalent ADC SNR Method <sup>8</sup>			27		f <sub>RMS</sub>	
3 GHz Output Frequency						Device setup <sup>7</sup> , f <sub>OUT</sub> = 1.5 GHz
Phase Noise Floor			-165.7		dBc/Hz	
RMS Jitter						
12 kHz to 20 MHz Integration			17.7		f <sub>RMS</sub>	Device setup <sup>7</sup> , f <sub>OUT</sub> = 1.5 GHz
100 Hz to 100 MHz Integration			18.3		f <sub>RMS</sub>	
Equivalent ADC SNR Method <sup>8</sup>			28		f <sub>RMS</sub>	
1.5 GHz Output Frequency						Device setup <sup>7</sup> , f <sub>OUT</sub> = 1.5 GHz
Phase Noise Floor			-169.5		dBc/Hz	
RMS Jitter						
12 kHz to 20 MHz Integration			19.5		f <sub>RMS</sub>	Device setup <sup>7</sup> , f <sub>OUT</sub> = 1.5 GHz
100 Hz to 100 MHz Integration			20.5		f <sub>RMS</sub>	
Equivalent ADC SNR Method <sup>8</sup>			29		f <sub>RMS</sub>	
Normalized In-Band Phase Noise Floor <sup>9</sup>	L <sub>NORM</sub>		-239		dBc/Hz	Normalized to 1 Hz
Normalized 1/f Phase Noise Floor <sup>9</sup>	L <sub>1/f</sub>		-287		dBc/Hz	
	L <sub>1/f_1G_10k</sub>		-147		dBc/Hz	
Spurious						LOCKED bit = 1, f <sub>REF</sub> = 100 MHz, f <sub>PPD</sub> = 200 MHz, f <sub>OUT</sub> = 12 GHz
f <sub>REF</sub>			-105		dBc	
f <sub>PPD</sub>			-95		dBc	
f <sub>SR_IN</sub>			-69		dBc	LOCKED bit = 1, f <sub>REF</sub> = f <sub>PPD</sub> = 200 MHz, f <sub>OUT</sub> = 12 GHz, f <sub>SR_IN</sub> = 50 MHz
TEMPERATURE SENSOR (ADC)						
ADC Clock Frequency	f <sub>ADC_CLK</sub>			400	kHz	ADC clock divider output
ADC Clock Divider Frequency	f <sub>ADC_CLKDIV</sub>			125	MHz	ADC clock divider input
Resolution				8	Bits	

<sup>1</sup> 1.2 V < V<sub>CP</sub> < 3.4 V.

<sup>2</sup> Valid for 1.60 V ≤ V<sub>VTUNE</sub> ≤ 2.85 V with device calibrated after a power cycle or software power-on reset.

<sup>3</sup> Based on characterization.

<sup>4</sup> Device setup: f<sub>REF</sub> = 200 MHz, f<sub>PPD</sub> = 200 MHz, f<sub>OUT</sub> = 3000 MHz, ENCLK = ENSR = CE = High. Bit fields: R\_DEL = 0, N\_DEL = 0, CP\_I = 15, CLKOUT\_OP = 1, REF\_SEL = 0, EN\_BLEED = 0, PD\_RDDET = 0, PD\_ADC = 0, PD\_LD = 0, LOCKED = 1.

<sup>5</sup> Device setup: f<sub>REF</sub> = 250 MHz, f<sub>SR\_IN</sub> = 50 MHz, f<sub>OUT</sub> = 12750 MHz, ENCLK = ENSR = CE = High. Bit fields: R\_DEL = 0, N\_DEL = 0, CP\_I = 15, CLKOUT\_OP = 1, REF\_SEL = 0, EN\_BLEED = 0, PD\_RDDET = 0, PD\_ADC = 0, PD\_LD = 0, LOCKED = 1.

<sup>6</sup> Device setup: f<sub>REF</sub> = 100 MHz, f<sub>PPD</sub> = 200 MHz, f<sub>OUT</sub> = 12.8 GHz, ENCLK = ENSR = CE = High. Bit fields: R\_DEL = 0, N\_DEL = 0, CP\_I = 15, CLKOUT\_OP = 1, REF\_SEL = 0, EN\_BLEED = 0, PD\_RDDET = 0, PD\_ADC = 0, PD\_LD = 0, LOCKED = 1, EN\_DNCLK = EN\_DRCLK = EN\_ADC\_CLK = 0, PD\_SRMON = 0, PD\_SYSREFOUT = 0, EN\_SR = Low.

<sup>7</sup> Device setup: f<sub>REF</sub> = 1000 MHz, f<sub>PPD</sub> = 500 MHz, ENCLK = ENSR = CE = High. Bit fields: R\_DEL = 0, N\_DEL = 0, CP\_I = 15, CLKOUT1\_OP = 1, CLKOUT2\_OP = 1, REF\_SEL = 0, EN\_BLEED = 0, PD\_RDDET = 0, PD\_ADC = 0, PD\_LD = 0, LOCKED = 1, the reference oscillator is the 0-CEGM-058AWEL-R-1GHz from NEL Frequency Control.

<sup>8</sup> Phase integration range 1 kHz to f<sub>OUT</sub> produces the same result as when clocking an ADC.

<sup>9</sup> See Equation 18 through Equation 22. These values are modeled in ADIsimPLL™.



**SPECIFICATIONS**

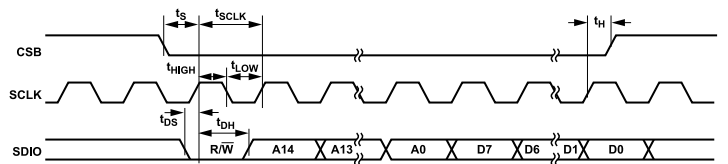
**SERIAL INTERFACE TIMING CHARACTERISTICS**

$V_{3.3V_1} = V_{3.3V_2} = 3.15\text{ V to }3.45\text{ V}$ ,  $V_{V5\_VCO} = V_{V5\_CP} = V_{V5\_CAL} = 4.75\text{ V to }5.25\text{ V}$ , all voltages are with respect to GND,  $T_A = -40^\circ\text{C to }+105^\circ\text{C}$ , operating temperature range, unless otherwise noted.

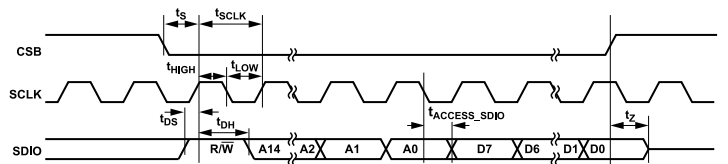
**Table 2. Serial Interface Timing Characteristics**

Parameter	Symbol	Min	Typ	Max	Unit	Test Conditions/Comments
SERIAL INTERFACE (CSB, SCLK, SDIO, SDO)						See Figure 2, Figure 3, and Figure 4
SCLK Frequency	$f_{SCLK}$			65	MHz	
SCLK Pulse Width High	$t_{HIGH}$	7.6			ns	
SCLK Pulse Width Low	$t_{LOW}$	7.6			ns	
SDIO Setup Time	$t_{DS}$	3			ns	
SDIO Hold Time	$t_{DH}$	3			ns	
SCLK Fall Edge to SDIO Valid Prop Delay	$t_{ACCESS\_SDIO}$	7.6			ns	
SCLK Fall Edge to SDO Valid Prop Delay	$t_{ACCESS\_SDO}$	7.6			ns	
CSB Rising Edge to SDIO High-Z	$t_Z$	7.6			ns	
CSB Falling Edge to SCLK Rise Setup Time	$t_S$	3			ns	
SCLK Rising Edge to CSB Rise Hold Time	$t_H$	3			ns	

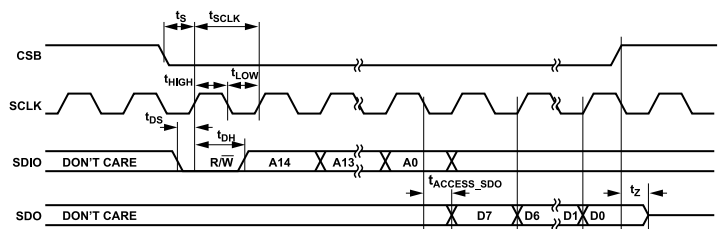
**Timing Diagrams**



**Figure 2. Write Timing Diagram**



**Figure 3. 3-Wire Read Timing Diagram (SDO\_ACTIVE = 0)**



**Figure 4. 4-Wire Read Timing Diagram (SDO\_ACTIVE = 1)**

## ABSOLUTE MAXIMUM RATINGS

$T_A = 25^\circ\text{C}$ , unless otherwise noted.

**Table 3. Absolute Maximum Ratings**

Parameter	Rating
$V_{3.3V_1}$ ( $V3\_LS$ , $V3\_LDO$ , $V3\_REF$ , $V3\_PFD$ , $V3\_NDIV$ ) to GND	-0.3 V to +3.6 V
$V_{3.3V_2}$ ( $V3\_VCO$ , $V3\_CLKDIV$ , $V3\_CLK$ , $V3\_SR$ ) to GND	-0.3 V to +3.6 V
$V_{5V}$ ( $V5\_CAL$ , $V5\_VCO$ , $V5\_CP$ ) to GND	-0.3 V to +5.5 V
Voltage on CP Pin	-0.3 V to $V_{V5\_CP} + 0.3$ V
Digital Outputs (MUXOUT, LKDET, SDO, SDIO) CLKP, CLKN	5 mA Maximum (GND - 0.3 V, $V_{3.3V_2} - 1.2$ V) to $V_{3.3V_2} + 0.3$ V
SR_OUTP, SR_OUTN	Maximum (GND - 0.3 V, $V_{3.3V_2} - 1.2$ V) to $V_{3.3V_2} + 0.3$ V
REFP, REFN	-0.65 V to $V_{3.3V_1} + 0.65$ V
SR_INP, SR_INN	-0.3 V to $V_{3.3V_1} + 0.3$ V
Voltage on All Other Pins	-0.3 V to $V_{3.3V_1} + 0.3$ V
REFP to REFN, When $V_{3.3V_1} > 3$ V	$\pm 1.35$ V
SR_INP to SR_INN, when $V_{3.3V_1} > 3$ V	$\pm 1.35$ V
Temperature	
Operating Junction Range <sup>1</sup>	-40°C to +125°C
Storage Range	-40°C to +125°C
Maximum Junction	125°C
Reflow Soldering	
Peak Temperature	260°C
Time at Peak Temperature	30 s

<sup>1</sup> Device is guaranteed to meet the specified performance limits over the full operating junction temperature range.

Stresses at or above those listed under Absolute Maximum Ratings may cause permanent damage to the product. This is a stress rating only; functional operation of the product at these or any other conditions above those indicated in the operational section of this specification is not implied. Operation beyond the maximum operating conditions for extended periods may affect product reliability.

## TRANSISTOR COUNT

The transistor count for the ADF4378 is 114258 (CMOS) and 2941 (bipolar).

## THERMAL RESISTANCE

Thermal performance is directly linked to printed circuit board (PCB) design and operating environment. Careful attention to PCB thermal design is required.

$\theta_{JA}$  is the natural convection, junction-to-ambient thermal resistance measured in a one cubic foot sealed enclosure.  $\theta_{JC}$  is the junction-to-case thermal resistance.

**Table 4. Thermal Resistance**

Package Type	$\theta_{JA}$	$\theta_{JC}$		$\theta_{JB}$	$\Psi_{JT}$	$\Psi_{JB}$	Unit
		TOP	BOTTOM				
CC-48-6 <sup>1</sup>	25.1	25.5	5.8	12.8	2.3	11.4	°C/W

<sup>1</sup> Test Condition 1: thermal impedance simulated values are based on use of a 4-layer PCB with the thermal impedance paddle soldered to a ground plane.

## ELECTROSTATIC DISCHARGE (ESD) RATINGS

The following ESD information is provided for handling of ESD-sensitive devices in an ESD protected area only.

Human body model (HBM) per ANSI/ESDA/JEDDEC JS-001.  
Charged device model (CDM) per ANSI/ESDA/JEDEC JS-002.

## ESD Ratings for ADF4378

**Table 5. ESD Ratings for ADF4378, 48-Lead LGA**

ESD Model	Withstand Threshold (V)	Class
HBM	3500	2
CDM	1250	C3

## ESD CAUTION



**ESD (electrostatic discharge) sensitive device.** Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.

PIN CONFIGURATIONS AND FUNCTION DESCRIPTIONS

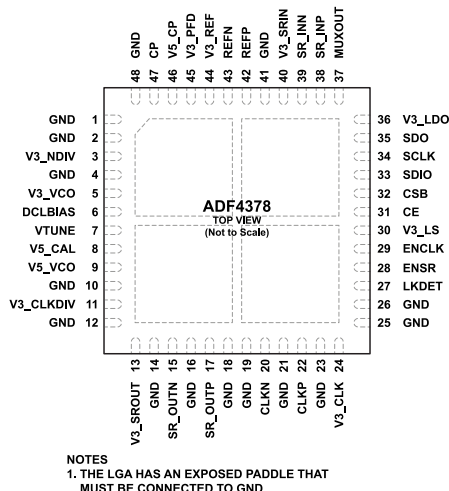


Figure 5. Pin Configuration

Table 6. Pin Function Descriptions

Pin Number	Mnemonic	Description
1, 2, 4, 10, 12, 14, 16, 18, 19, 21, 23, 25, 26, 41, 48	GND	Negative Power Supply (Ground). These pins must be connected directly to the ground pad.
3	V3_NDIV	3.15 V to 3.45 V Positive Power Supply Pin for the PLL Feedback Divider Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 1.
5	V3_VCO	3.15 V to 3.45 V Positive Power Supply Pin for the 3.3 V Portion of the VCO Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 2.
6	DCLBIAS	Do not connect to this pin.
7	VTUNE	VCO Tuning Input. This frequency control pin is normally connected to the external loop filter.
8	V5_CAL	4.75 V to 5.25 V Positive Power Supply Pin for VCO Calibration Circuitry. This pin can be shorted to the V5_VCO supply plane.
9	V5_VCO	4.75 V to 5.25 V Positive Power Supply Pin for the 5 V Portion of the VCO Circuitry.
11	V3_CLKDIV	3.15 V to 3.45 V Positive Power Supply Pin for the Output Divider Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 2.
13	V3_SROUT	3.15 V to 3.45 V Positive Power Supply Pin for the SYSREF Buffer Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 2.
15, 17	SR_OUTN, SR_OUTP	SYSREF Output Signal. The relocked SYSRREF input is presented differentially on these pins. The outputs have 50 Ω (typical) output resistance per side (100 Ω differential). The far end of the transmission line is typically terminated with 100 Ω connected across the outputs. Typically, these outputs have a 1.2 V common mode and are designed to interface with an LVDS input. However, there are termination schemes that allow for other common levels.
20, 22	CLKN, CLKP	Clock Output Signal. The VCO output divider is buffered and presented differentially on these pins. The outputs have 50 Ω (typical) output resistance per side (100 Ω differential). The far end of the transmission line is typically terminated with 100 Ω connected across the outputs. The output amplitude is programmable through the serial port.
24	V3_CLK	3.15 V to 3.45 V Positive Power Supply Pin for the Clock 1 Buffer Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 2.
27	LKDET	PLL Lock Detect. This output presents the lock status of the PLL. The PLL is locked when the LKDET pin is a logic high.
28	ENSR	Enable SYSREF Output Buffer. 1.8 V and 3.3 V compatible CMOS input. When ENSR = high, the SR_OUTP and SR_OUTN output buffer is active. When ENSR = low, SR_OUTP and SR_OUTN output buffer is powered down.
29	ENCLK	Enable Clock 1 Output Buffer. 1.8 V and 3.3 V compatible CMOS input. When ENCLK = high, the CLKP and CLKN output buffer is active. When ENCLK = low, the CLKP and CLKN output buffer is powered down.
30	V3_LS	3.15 V to 3.45 V Positive Power Supply Pin for the Internal Level Shift Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 1.
31	CE	Chip Enable. 3.3 V CMOS input. Does not support 1.8 V CMOS levels. This CMOS input enables the device when driven high. A logic low disables the device, putting the device in a full power-down state, which causes the registers to reset. Conversely, the PD_ALL bit powers down the device, but does not reset the registers.

## PIN CONFIGURATIONS AND FUNCTION DESCRIPTIONS

Table 6. Pin Function Descriptions (Continued)

Pin Number	Mnemonic	Description
32	CSB	Serial-Port Chip Select. 1.8 V and 3.3 V compatible CMOS input. This CMOS input initiates a serial-port communication burst when driven low, which ends the burst when driven back high.
33	SDIO	Serial Data Input/Output. 1.8 V and 3.3 V programmable CMOS input/output. When configured as an input, the serial port uses this CMOS input for data. In 3-wire readback mode (default mode), this pin outputs data from the serial port during a read communication burst.
34	SCLK	Serial-Port Clock. 1.8 V and 3.3 V compatible. This CMOS input clocks serial-port input data on its rising edge.
35	SDO	Optional Serial Data Output. 1.8 V and 3.3 V programmable CMOS output. In 3-wire mode (default mode), this three state CMOS pin remains in a high impedance state. In 4-wire readback mode, this pin presents data from the serial port during a read communication burst. When the $\overline{\text{CSB}}$ is deasserted, SDO returns to a high impedance. Optionally, attach a resistor of > 200 k $\Omega$ to prevent a floating output.
36	V3_LDO	3.15 V to 3.45 V Positive Power Supply Pin for the Internal LDO Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 1.
37	MUXOUT	Internal Device Mux Output. This output pin can be connected to multiple internal nodes for factory test and debug purposes.
38, 39	SR_INP, SR_INN	SYSREF Input. This input reclocks a reference aligned SYSREF signal to a known clock period on the SR_OUTP and SR_OUTN pins. DC-coupled common ranges that support CML, LVPECL, or LVDS can be selected through the serial port.
40	V3_SRIN	3.15 V to 3.45 V Positive Power Supply. Short this pin to the other pins in 3.3 V Power Supply Group 1.
42, 43	REFP, REFN	Reference Input Signal. This differential input is buffered with a delay matched amplifier (DMA) for well controlled reference to output propagation delays (default mode, REF_SEL = 0). For low slew-rate reference input signals, an alternate low noise amplifier (LNA) can be selected through the serial port (REF_SEL = 1). Reference inputs are self-biased and must be AC-coupled with 1 $\mu\text{F}$ capacitors. Reference inputs accept differential or single-ended inputs.
44	V3_REF	3.15 V to 3.45 V Positive Power Supply Pin for the PLL Reference Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 1.
45	V3_PFD	3.15 V to 3.45 V Positive Power Supply Pin for PFD Circuitry. Short this pin to the other pins in 3.3 V Power Supply Group 1.
46	V5_CP	4.75 V to 5.25 V Positive Power Supply Pin for Charge Pump Circuitry. This pin must be isolated from the V5_VCO supply plane.
47	CP	Charge Pump Output. This bidirectional current output is normally connected to the external loop filter.
Exposed Pad	EP	Exposed Pad. Negative power supply (ground). The LGA has exposed paddle that must be connected to the ground pad. The PCB land pattern must have multiple thermal vias to the ground plane for both low ground inductance and low thermal resistance.

TYPICAL PERFORMANCE CHARACTERISTICS

$V_{3.3V_1} = V_{3.3V_2} = 3.3\text{ V}$ ,  $V_{5V} = 5\text{ V}$ , all voltages are with respect to GND,  $T_A = 25^\circ\text{C}$ , unless otherwise noted.

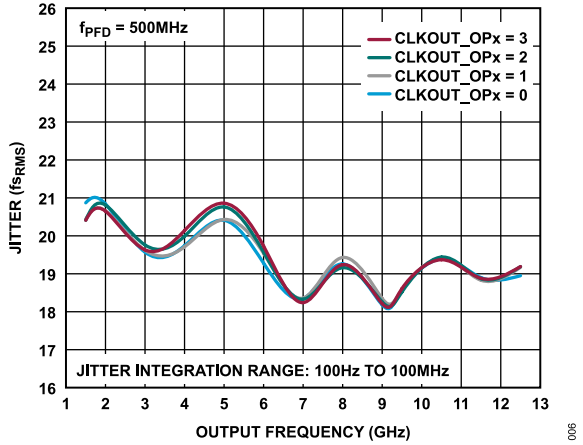


Figure 6. Jitter vs. Output Frequency at Various Output Amplitudes

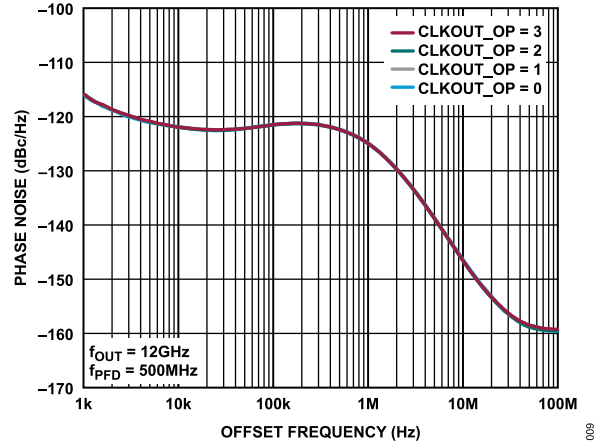


Figure 9. Closed-Loop Phase Noise at Various Output Amplitudes

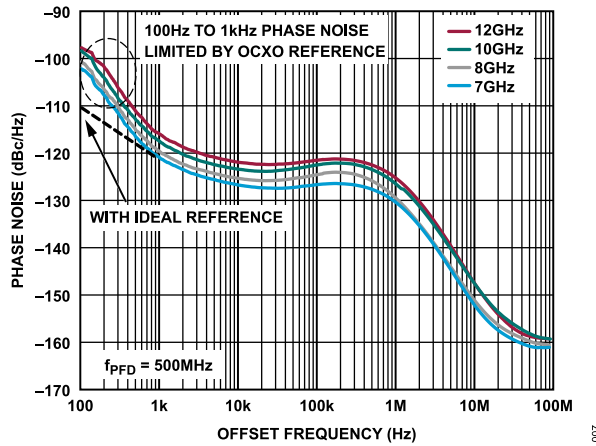


Figure 7. Closed-Loop Phase Noise at Various Output Frequencies

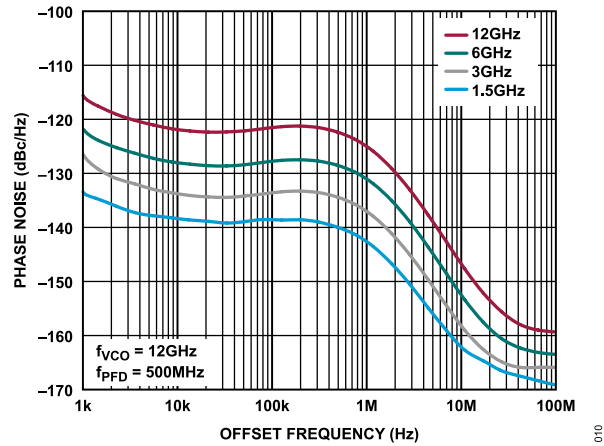


Figure 10. Closed-Loop Phase Noise at Various CLKOUT\_DIV Settings

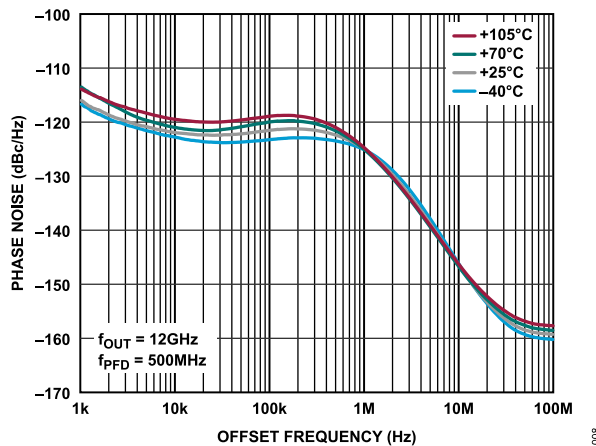


Figure 8. Closed-Loop Phase Noise at Various Temperatures

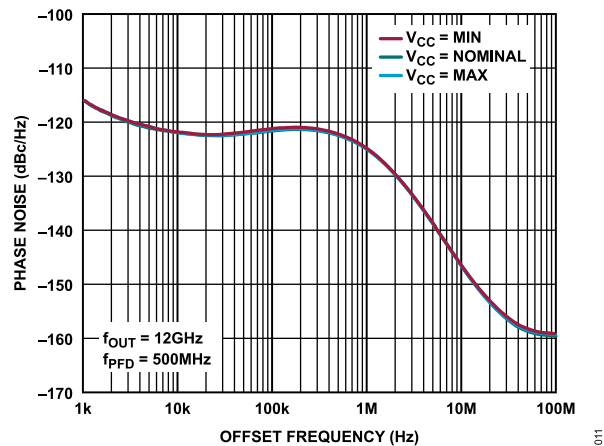


Figure 11. Closed-Loop Phase Noise at Various Power Supply Voltages

TYPICAL PERFORMANCE CHARACTERISTICS

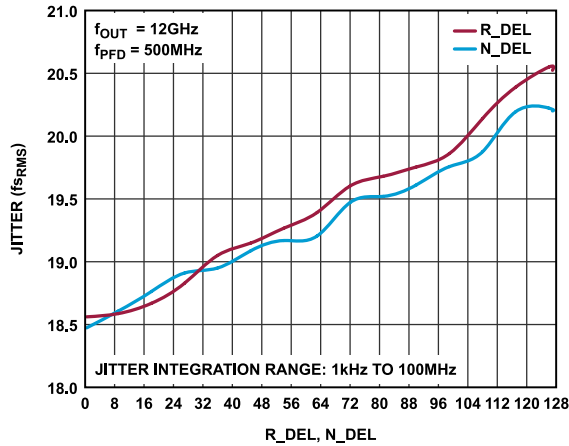


Figure 12. Jitter vs. R\_DEL, N\_DEL

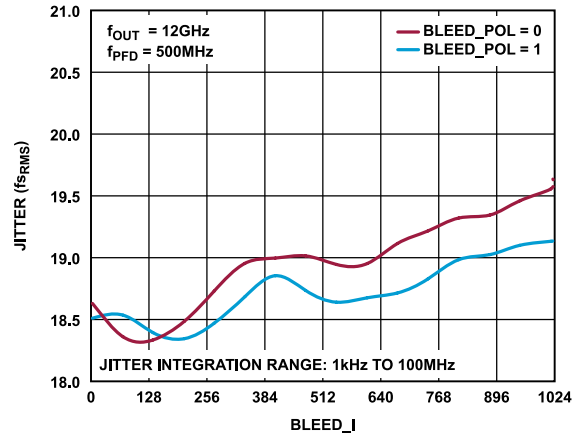


Figure 15. Jitter vs. BLEED\_I

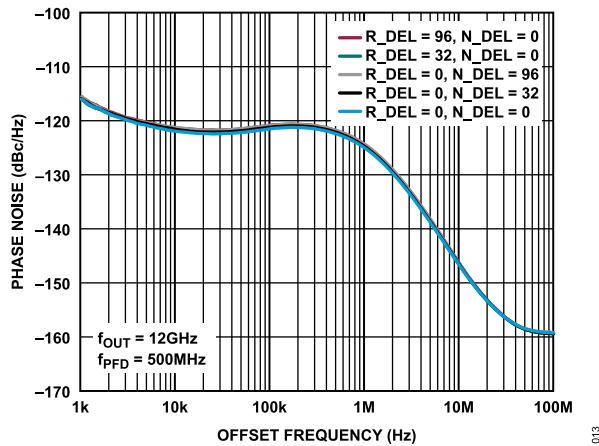


Figure 13. Closed-Loop Phase Noise at Various R\_DEL and N\_DEL Settings

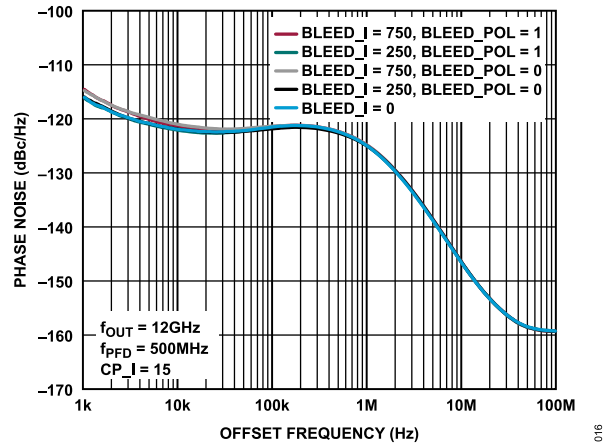


Figure 16. Closed-Loop Phase Noise at Various Charge-Pump Bleed Delays

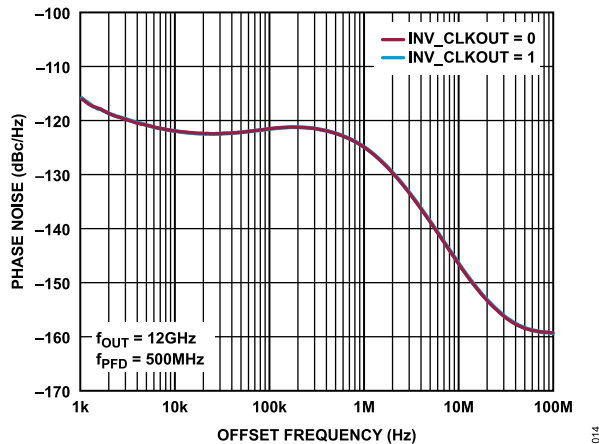


Figure 14. Closed-Loop Phase Noise at Various Clock Invert Settings

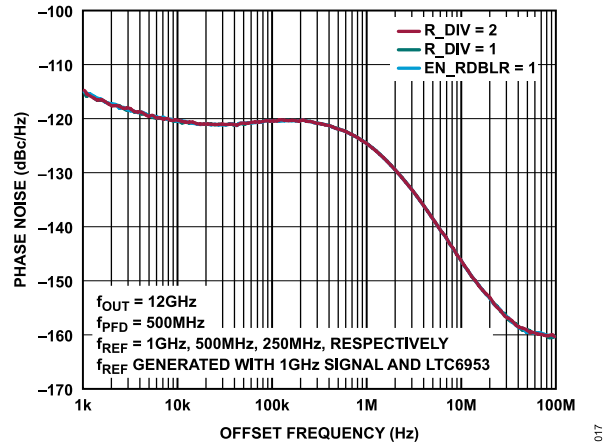


Figure 17. Closed-Loop Phase Noise at Various Reference Doubler and Reference Divider Settings

TYPICAL PERFORMANCE CHARACTERISTICS

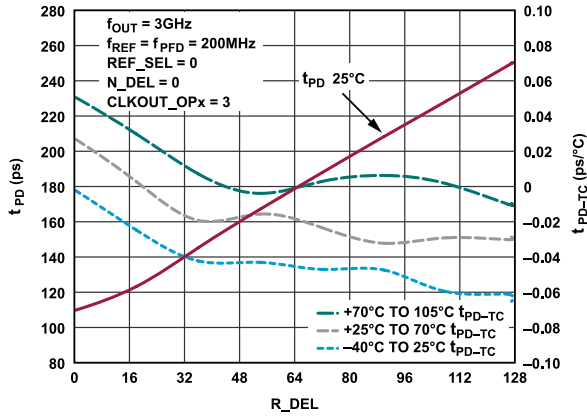


Figure 18. Propagation Delay ( $t_{PD}$ ) and Propagation Delay Temperature Coefficient ( $t_{PD-TC}$ ) vs.  $R\_DEL$

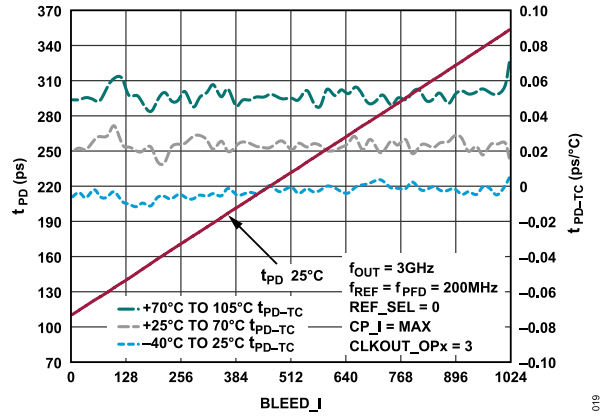


Figure 21.  $t_{PD}$  and  $t_{PD-TC}$  vs.  $BLEED\_I$ ,  $BLEED\_POL = 0$

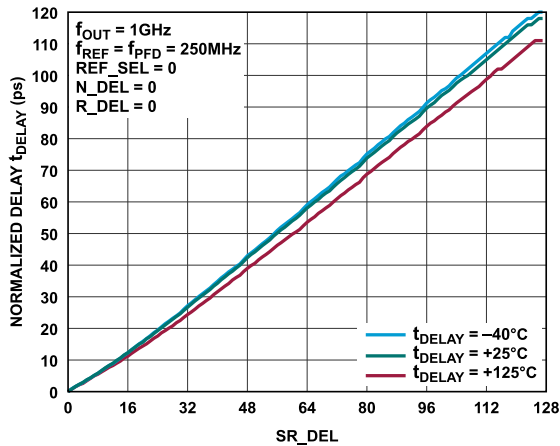


Figure 19. Normalized Delay Between SYSREF and CLK ( $t_{DELAY}$ ) vs.  $SR\_DEL$

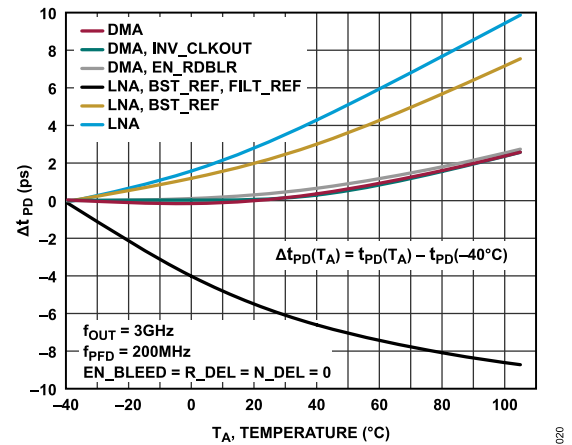


Figure 22. Delta Propagation Delay ( $\Delta t_{PD}$ ) vs.  $T_A$ , Temperature, Device Configuration

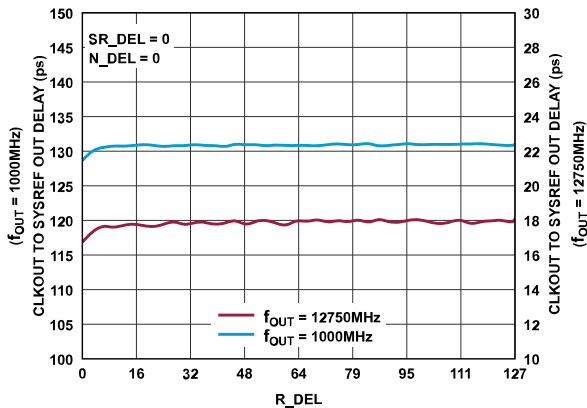


Figure 20. CLK OUT to SYSREF OUT Delay vs.  $R\_DEL$ ,  $f_{OUT} = 1000$  MHz and  $f_{OUT} = 12750$  MHz

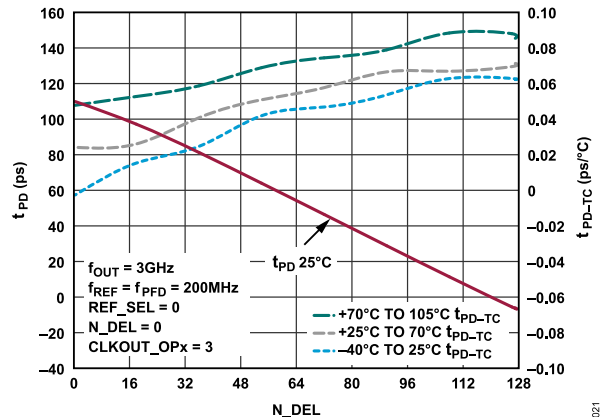


Figure 23.  $t_{PD}$  and  $t_{PD-TC}$  vs.  $N\_DEL$

TYPICAL PERFORMANCE CHARACTERISTICS

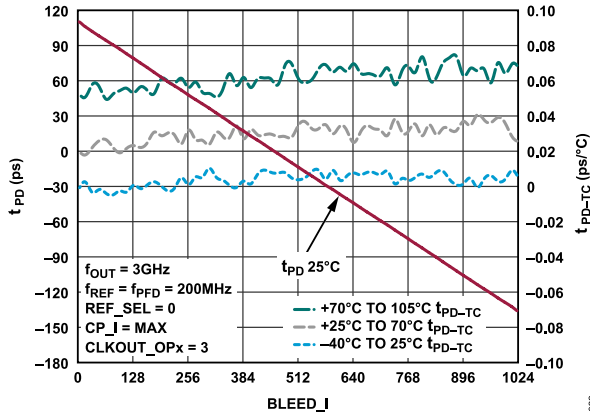


Figure 24.  $t_{PD}$  and  $t_{PD-TC}$  vs. BLEED\_I, BLEED\_POL = 1

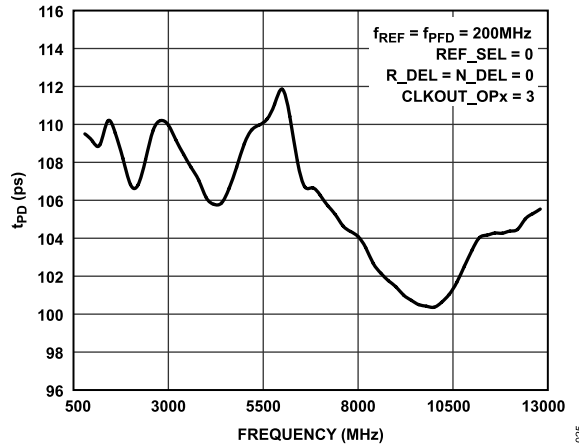


Figure 27.  $t_{PD}$  vs. Frequency

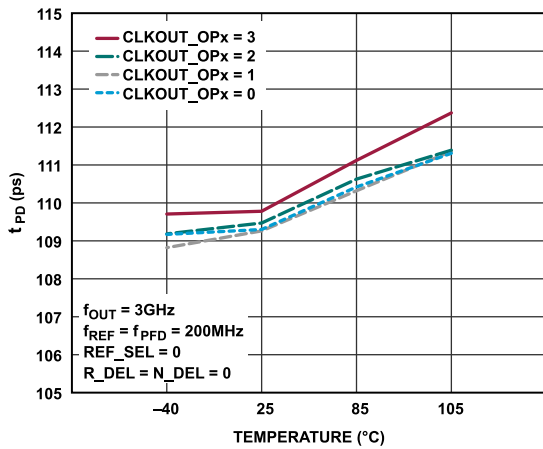


Figure 25.  $t_{PD}$  vs. Temperature, CLKOUT\_OP Setting

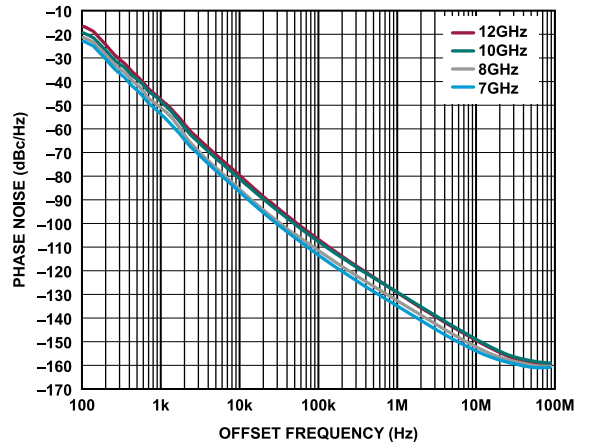


Figure 28. Open-Loop VCO Phase Noise at Various Frequencies

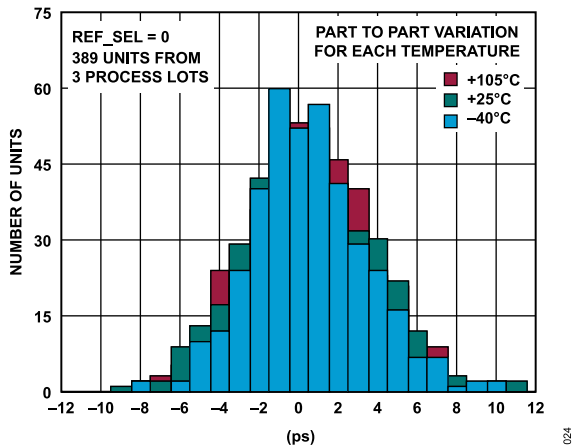


Figure 26. Normalized Propagation Delay ( $t_{PD}$ ) Histogram

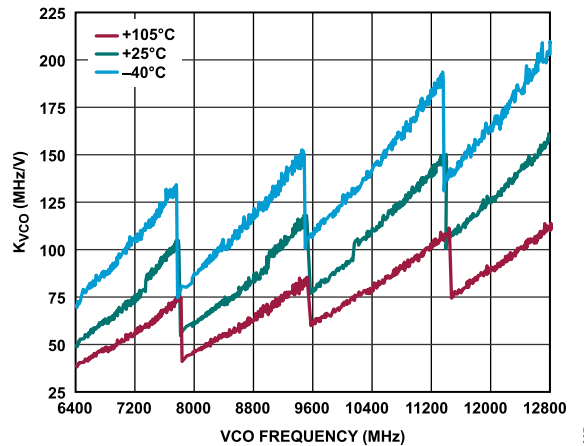


Figure 29.  $K_{VCO}$  at Various Frequencies and Temperatures



TYPICAL PERFORMANCE CHARACTERISTICS

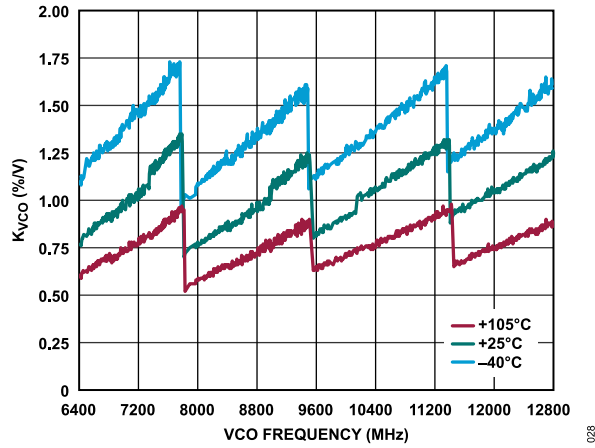


Figure 30.  $K_{VCO}$  Percentage at Various Frequencies and Temperatures

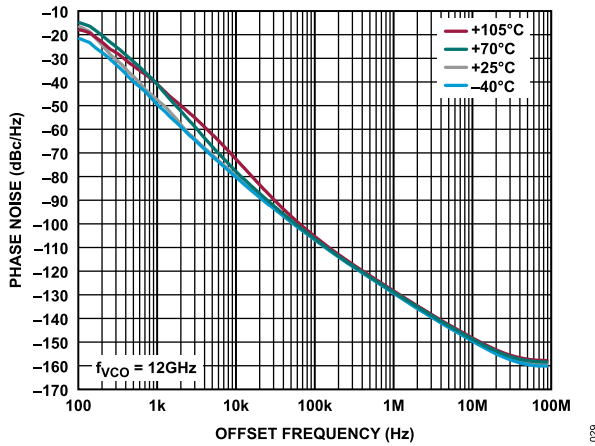


Figure 31. Open-Loop VCO Phase Noise at Various Temperatures

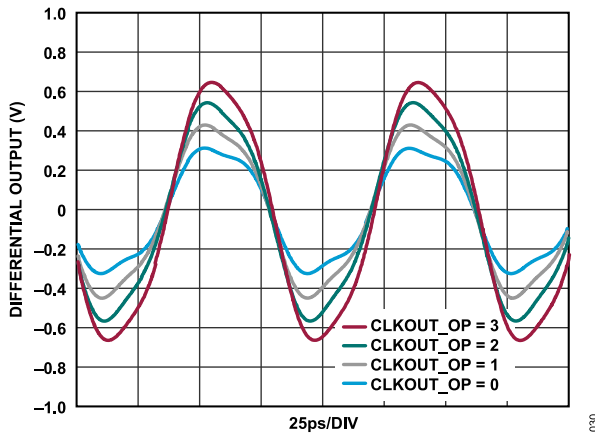


Figure 32. Differential Output at 12 GHz

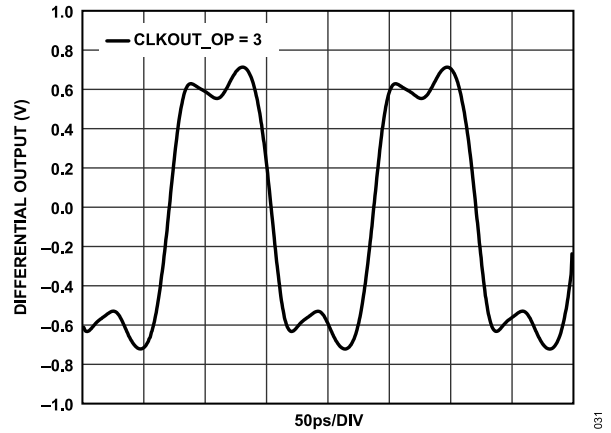


Figure 33. Differential Output at 6 GHz

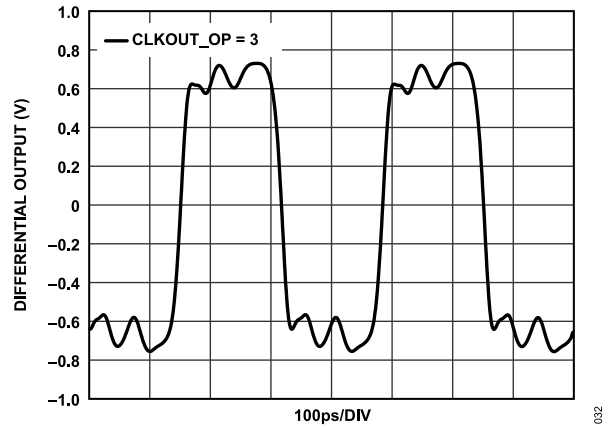


Figure 34. Differential Output at 3 GHz

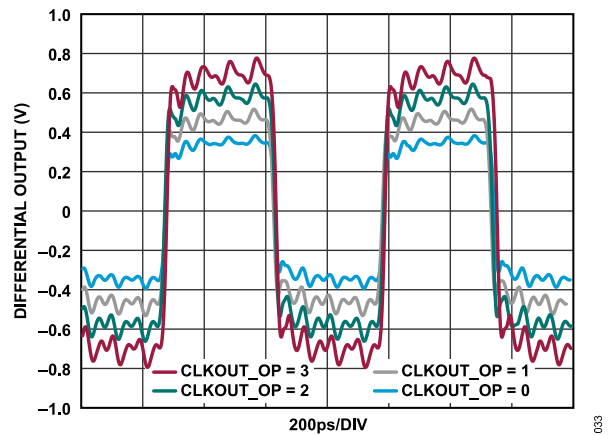


Figure 35. Differential Output at 1.5 GHz

TYPICAL PERFORMANCE CHARACTERISTICS

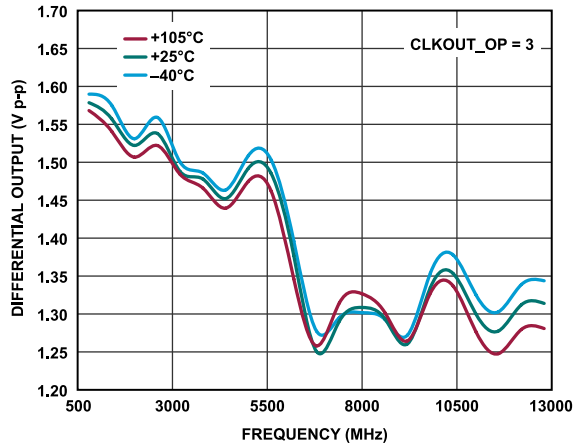


Figure 36. Differential Output vs. Frequency, Temperature

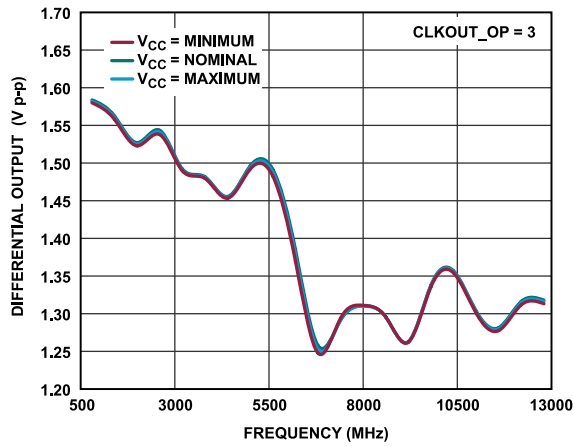


Figure 37. Differential Output vs. Frequency, Power Supply Voltage

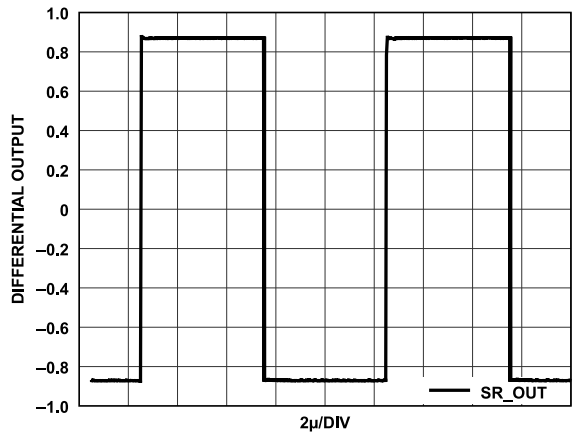


Figure 38. Differential Continuous SR\_OUT at 100 kHz (with 1 MΩ Termination)

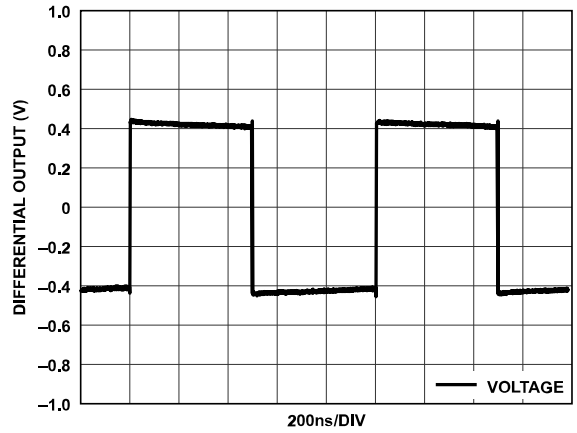


Figure 39. Differential Continuous SR\_OUT at 1 MHz

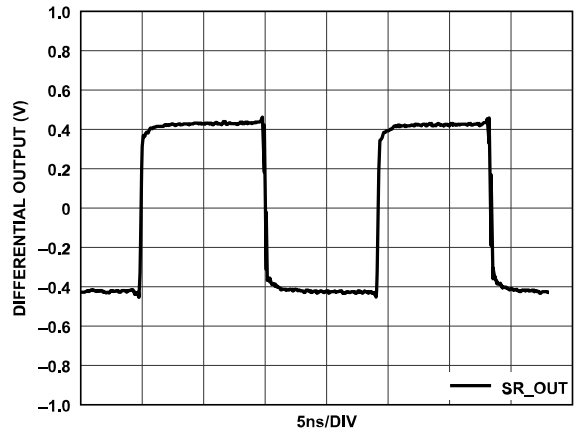


Figure 40. Differential Continuous SR\_OUT at 50 MHz

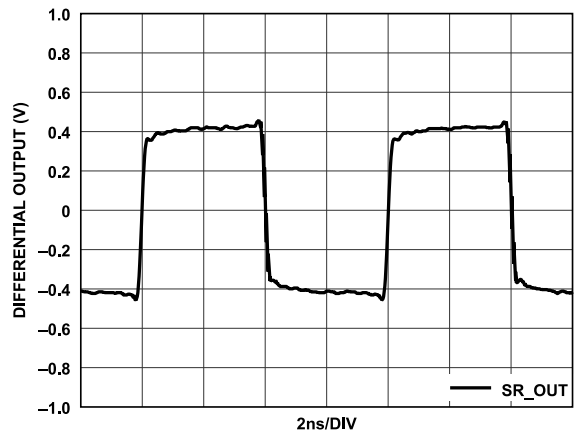


Figure 41. Differential Continuous SR\_OUT at 125 MHz

TYPICAL PERFORMANCE CHARACTERISTICS

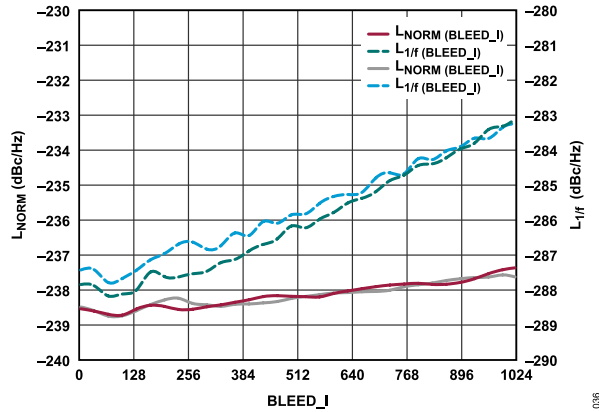


Figure 42.  $L_{NORM}$  and  $L_{1/f}$  vs. BLEED\_I

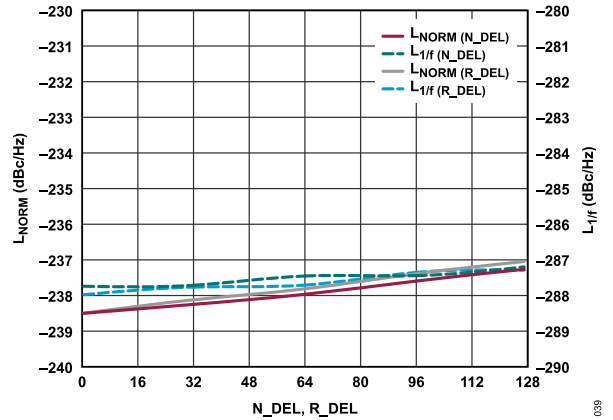


Figure 45.  $L_{NORM}$  and  $L_{1/f}$  vs. N\_DEL, R\_DEL

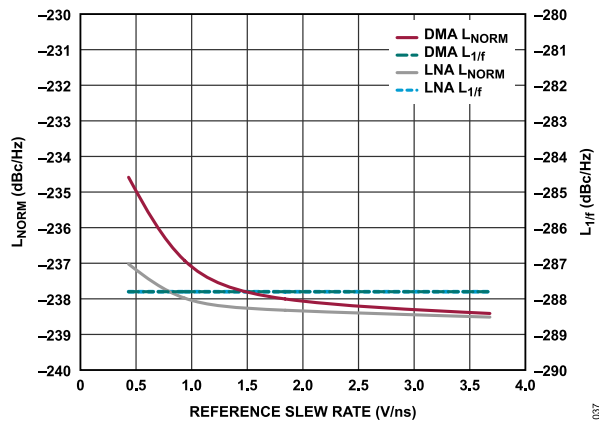


Figure 43.  $L_{NORM}$  and  $L_{1/f}$  vs. Reference Slew Rate, Reference Amplifier

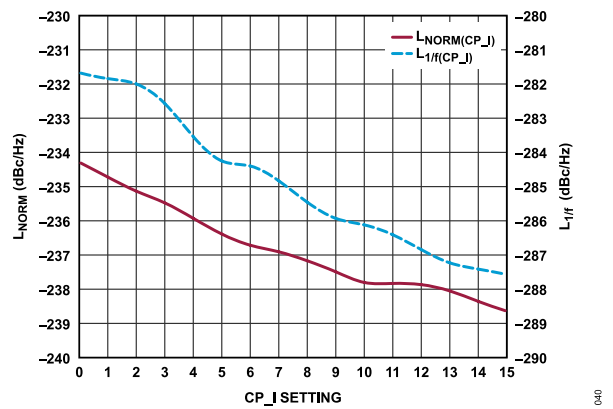


Figure 46.  $L_{NORM}$  and  $L_{1/f}$  vs. CP\_I Setting

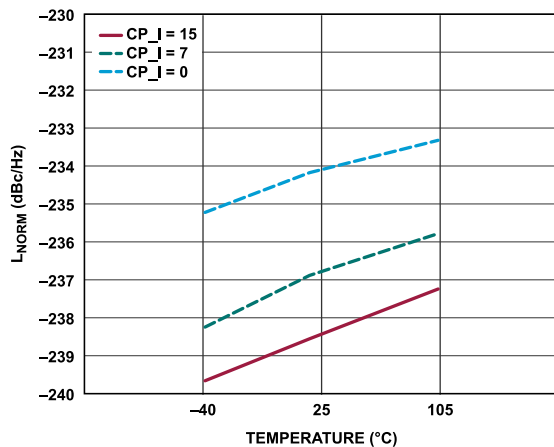


Figure 44.  $L_{NORM}$  vs. Temperature, Charge-Pump Current

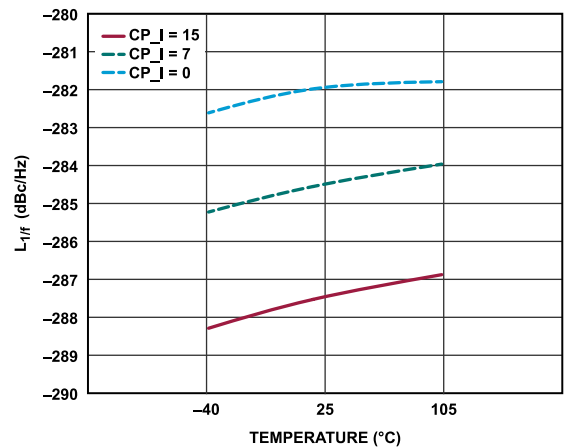


Figure 47.  $L_{1/f}$  vs. Temperature, Charge-Pump Current

TYPICAL PERFORMANCE CHARACTERISTICS

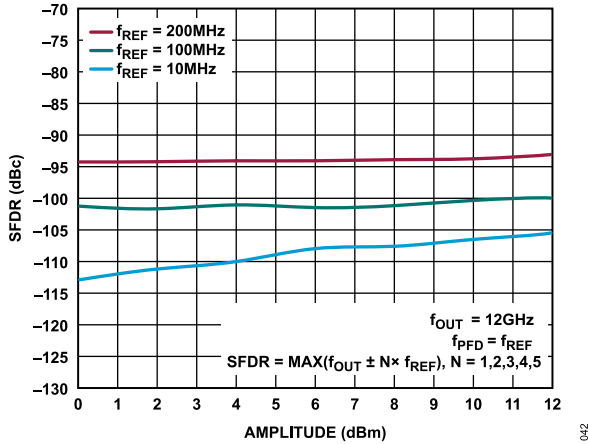


Figure 48. Reference and PFD Spurious Level at Various Reference Frequencies and Reference Amplitudes, EN\_RDBLR = 0

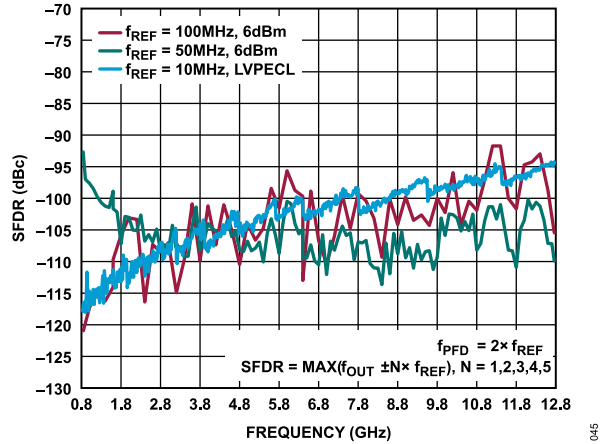


Figure 51. Reference and PFD Spurious Level at Various Reference Input Frequencies and Output Frequencies, EN\_RDBLR = 1

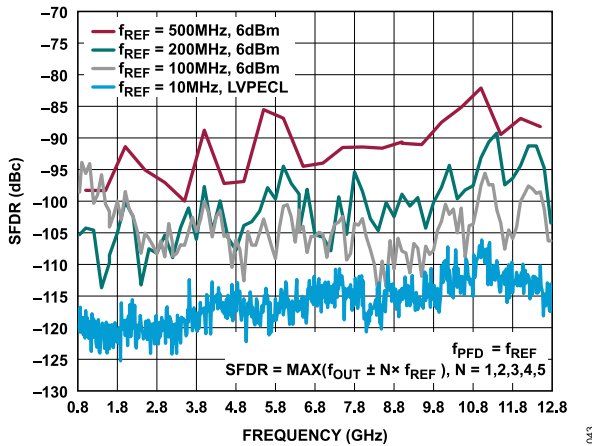


Figure 49. Reference and PFD Spurious Level at Various Reference Frequencies and Output Frequencies, EN\_RDBLR = 0

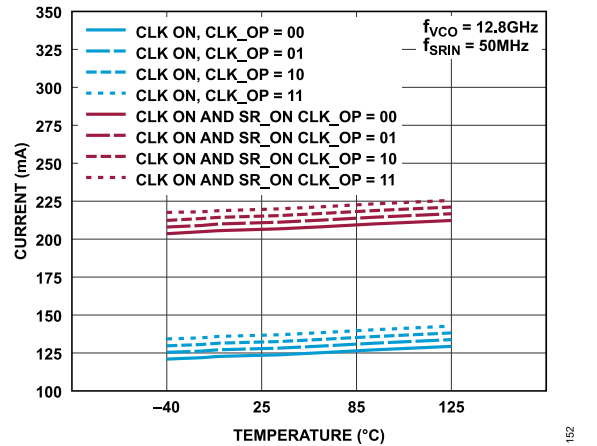


Figure 52. 3.3 V Supply Group 2 Current at Various Junction Temperatures and Output Settings

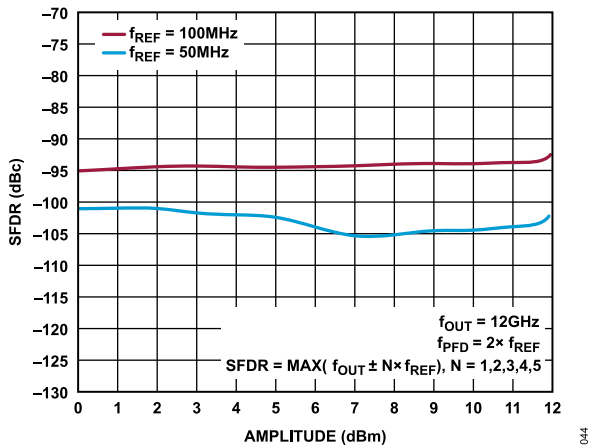


Figure 50. Reference and PFD Spurious Level at Various Reference Frequencies and Reference Amplitudes, EN\_RDBLR = 1

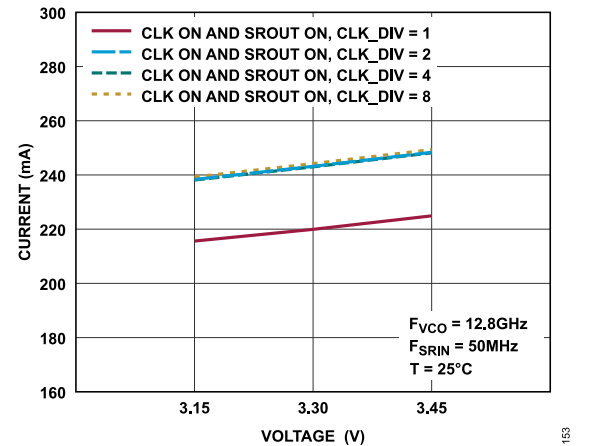


Figure 53. 3.3 V Supply Group 2 Current at Various Power Supply Voltages and CLKOUT\_DIV Settings

TYPICAL PERFORMANCE CHARACTERISTICS

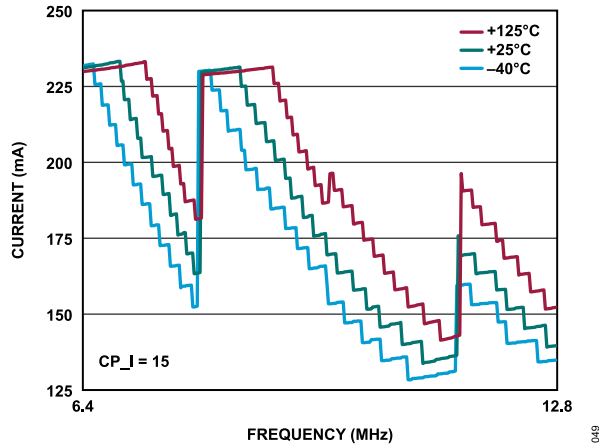


Figure 54. 5 V Supply Current at Various Output Frequencies and Junction Temperatures

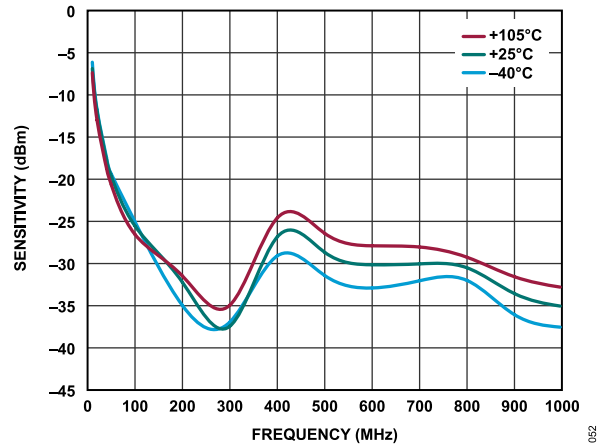


Figure 57. DMA Reference Input Sensitivity at Various Reference Frequencies and Temperatures

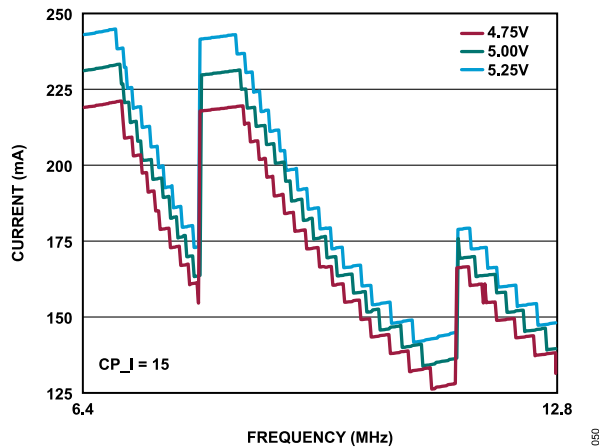


Figure 55. 5 V Supply Current at Various Output Frequencies and Power Supply Voltages

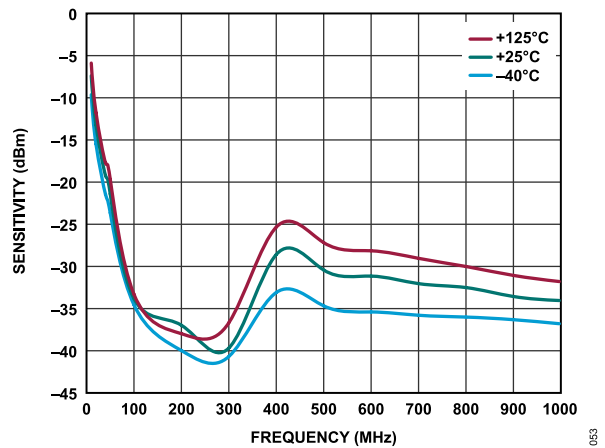


Figure 58. LNA Reference Input Sensitivity at Various Reference Frequencies and Temperatures

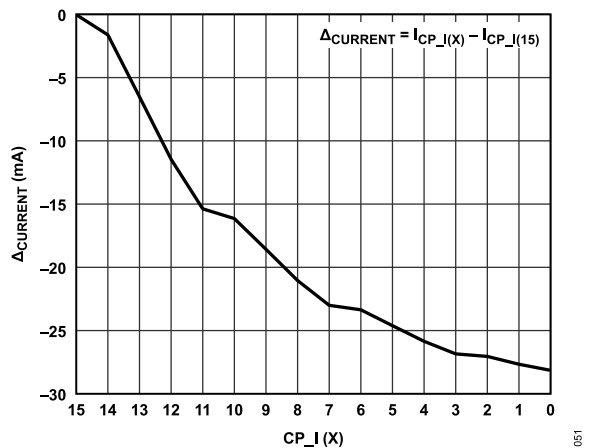


Figure 56. 5 V Delta Supply Current ( $\Delta_{CURRENT}$ ) at Various CP\_I Settings

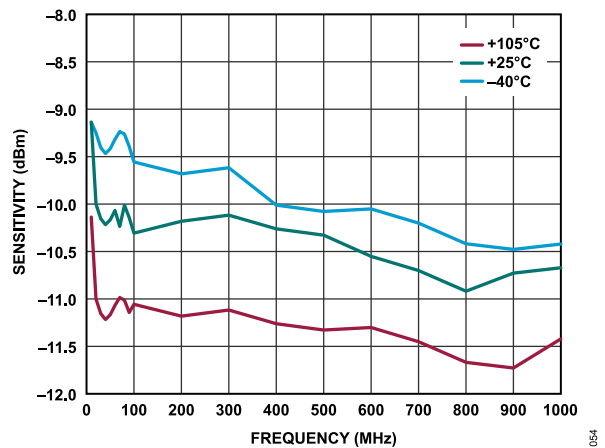


Figure 59. Reference Input Signal Detected at Various Reference Frequencies and Temperatures

TYPICAL PERFORMANCE CHARACTERISTICS

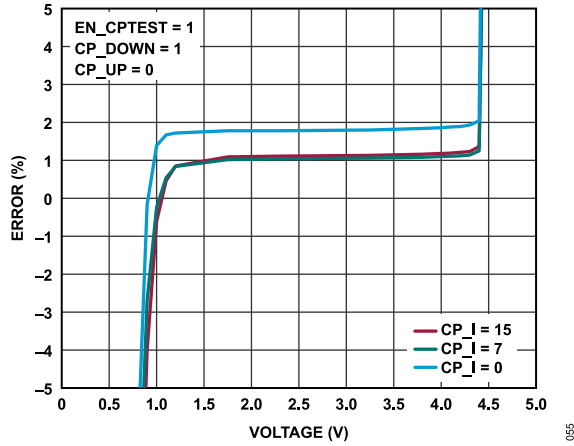


Figure 60. Charge-Pump Sink Current Error at Various Charge-Pump Voltages and CP\_I Settings

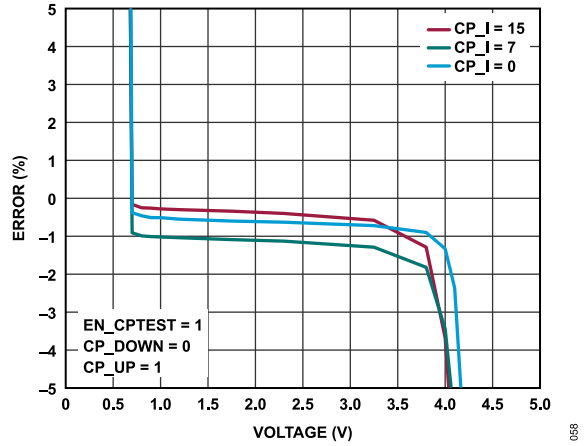


Figure 63. Charge-Pump Source Current Error at Various Charge-Pump Voltages and CP\_I Settings

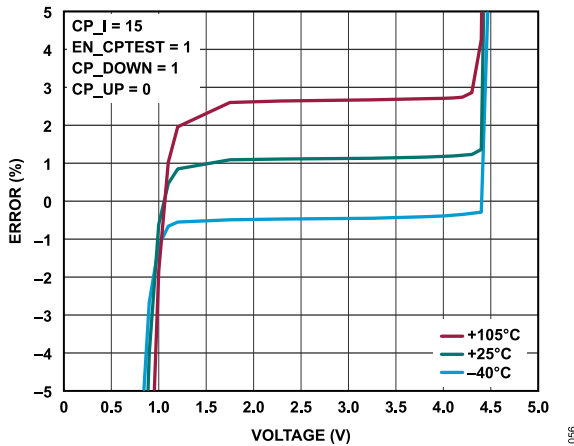


Figure 61. Charge-Pump Sink Current Error at Various Charge-Pump Voltages and Temperatures

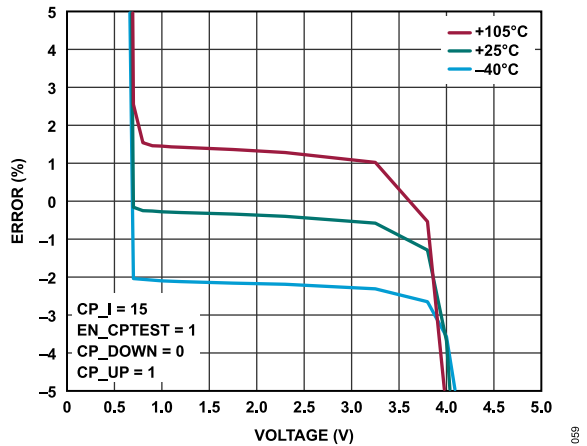


Figure 64. Charge-Pump Source Current Error at Various Charge-Pump Voltages and Temperatures

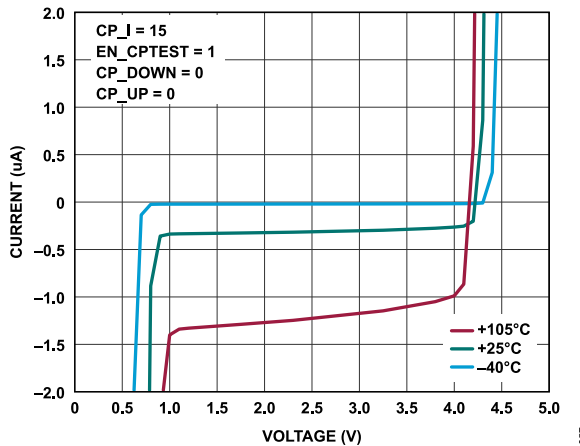


Figure 62. Charge-Pump High-Z Current at Various Charge-Pump Voltages and Temperatures

THEORY OF OPERATION

INTRODUCTION

A PLL is a complex feedback system that may conceptually be considered a frequency multiplier. The system multiplies the reference input frequency ( $f_{REF}$ ) and produces a higher frequency on the clock output pins ( $f_{OUT}$ ). The PFD, charge pump, output divider, feedback divider, VCO, and external loop filter forms a feedback loop to accurately control the output frequency (see Figure 65). The reference divider or reference doubler is used to set the frequency resolution.

The ADF4378 has an additional input and output clock pair, which is used to provide the retimed SYSREF clock to JESD204B/C devices. The SYSREF clock generated by an external clocking product is retimed with the reference clock, feedback clock, and output clock. This provides a well-controlled device clock and SYSREF clock pair in which any effect coming from temperature or any system level mismatched is compensated.

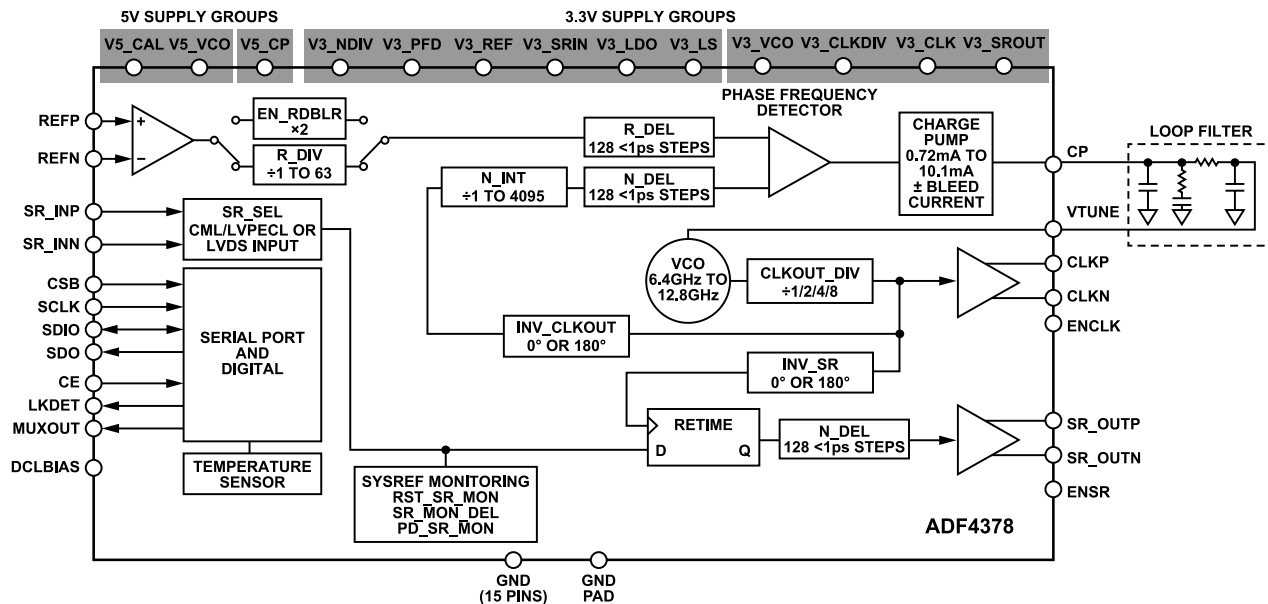


Figure 65. PLL Loop Diagram

## THEORY OF OPERATION

### OUTPUT FREQUENCY

#### When EN\_RDBLR = 0

When the loop is locked, the frequency ( $f_{VCO}$ ) (in Hz) produced at the output of the VCO is determined by the reference frequency ( $f_{REF}$ ) and the O, R, and N values given by Equation 1. For more information, see Table 11 and Table 18.

$$f_{VCO} = f_{REF} \times \frac{N \times O}{R} \quad (1)$$

In the following equation, the PFD frequency ( $f_{PFD}$ ) produced is given by Equation 2.

$$f_{PFD} = \frac{f_{REF}}{R} \quad (2)$$

The  $f_{VCO}$  may be alternatively expressed as:

$$f_{VCO} = f_{PFD} \times N \times O \quad (3)$$

The output frequency ( $f_{OUT}$ ) produced at the output of the output divider is given by Equation 4.

$$f_{OUT} = \frac{f_{VCO}}{O} \quad (4)$$

The output frequency resolution ( $f_{STEP}$ ) produced by a unit change in N is given by Equation 5.

$$f_{STEP} = f_{PFD} \quad (5)$$

#### When EN\_RDBLR = 1

When the loop is locked, the frequency ( $f_{VCO}$ ) (in Hz) produced at the output of the VCO is determined by the reference frequency ( $f_{REF}$ ) and the O, D, and N values given by Equation 6.

$$f_{VCO} = f_{REF} \times D \times N \times O \quad (6)$$

When EN\_RDBLR = 1, the PFD frequency ( $f_{PFD}$ ) produced is given by Equation 7.

$$f_{PFD} = f_{REF} \times D \quad (7)$$

Equation 3, Equation 4, and Equation 5 for  $f_{VCO}$ ,  $f_{OUT}$ , and  $f_{STEP}$  remain the same when EN\_RDBLR = 1.

## CIRCUIT DESCRIPTION

### Reference Input Buffer

The reference frequency of the PLL is applied differentially on the REFP and REFN pin. These high impedance inputs are self-biased and must be AC-coupled with 1  $\mu\text{F}$  capacitors (for a simplified schematic, see Figure 66). Alternatively, the differential inputs may be configured as a single ended input by applying the reference frequency at REFP and bypassing REFN to GND with a 1  $\mu\text{F}$  capacitor (see Figure 86).

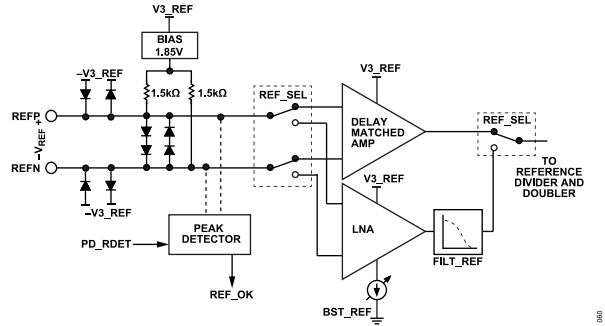


Figure 66. Reference Input Stage

A high quality signal must be applied to the REFP and REFN inputs because they provide the frequency reference to the entire PLL. To achieve the in-band phase noise performance of the PLL, apply a continuous waveform signal or a square wave with a slew rate of at least 1000 V/ $\mu\text{s}$ . For more information on reference input signal requirements and interfacing, see the Reference Source Considerations section.

When the REF\_SEL bit is set to 0, the DMA buffer is selected. The DMA is optimized for high slew rate signals, such as square waves or higher frequency and higher amplitude sine waves. The DMA has a controlled propagation delay from the reference input to clock output, which eases time zero and over temperature multichip clock alignment.

When the REF\_SEL bit is set to 1, the LNA is selected. The LNA is optimized for low slew rate signals, such as lower frequency or lower amplitude sine waves.

The REF\_SEL bit must be set correctly to optimize the in-band phase noise performance and propagation delay. For recommended settings, see Table 7, Figure 43, and Equation 8.

Table 7. REF\_SEL Programming

REF_SEL	Sine Wave Slew Rate (V/ $\mu\text{s}$ )	Square Wave	Optimized $t_{PD}$
0	$\geq 1500$	Preferred	Yes
1	$< 1500$	Not applicable	Not applicable

To calculate the slew rate of sine wave,

$$\text{Slew Rate} = 2 \times \pi \times f \times V \quad (8)$$

where:

$f$  = sine wave frequency.

$V$  = sine wave amplitude (in  $V_{PK}$ ).

The FILTER\_REF bit controls the low-pass filter of the reference input LNA and must be set for sine wave signals based on  $f_{REF}$  to limit the wideband noise of the input reference signal. The FILTER\_REF bit must be set correctly to reach the  $L_{NORM}$  normalized in-band phase noise floor. For recommended settings, see Table 8. Square wave inputs must have FILTER\_REF set to 0.



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**Table 8. *FILT\_REF* Programming**

FILT_REF	Sine Wave $f_{REF}$	Square Wave $f_{REF}$
0	$\geq 20$ MHz	All $f_{REF}$
1	$< 20$ MHz	Not applicable

The BST\_REF bit must be set based on the input signal level to prevent the LNA reference input buffer from saturating. The BST\_REF programming is the same whether the input is a sine wave or a square wave. For recommended settings, see Table 9 and for programming examples, see the Applications Information section.

**Table 9. *BST\_REF* Programming**

BST_REF	Sine Wave $V_{REF}$
0	$\geq 1.6$ V p-p
1	$< 1.6$ V p-p

**Reference Peak Detector**

A reference input peak detection circuit is provided on the REFP and REFN inputs to detect the presence of a reference signal and provides the REF\_OK status flag available through serial port register REG0049. The circuit has hysteresis to prevent the REF\_OK flag from chattering at the detection threshold.

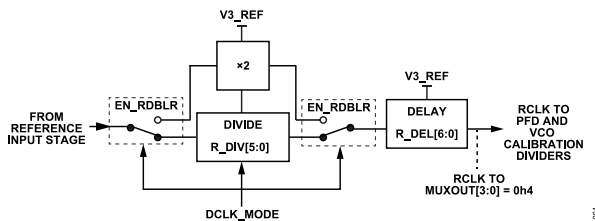
The peak detector approximates an rms detector. Therefore, sine and square wave inputs give different detection thresholds by a factor of  $4/\pi$ . For REF\_OK detection values, see Table 10.

**Table 10. *REF\_OK* Status Output vs. Reference Input**

REF_OK	Sine Wave $V_{REF}$	Square Wave $V_{REF}$
1	$\geq 200$ mV p-p	$\geq 155$ mV p-p
0	$< 160$ mV p-p	$< 125$ mV p-p

**Reference Divider (R) and Doubler (D)**

When the EN\_RDBLR bit is set to 1, a frequency multiplier is used to double the frequency seen at the PFD. When the EN\_RDBLR bit is set to 0, a 6-bit divider, R\_DIV, is used to reduce the frequency seen at the PFD. The reference divide ratio, R, may be set to any integer from 1 to 63, inclusive of all the integer divide values. Use the R\_DIV[5:0] bits found in REG0012 to directly program the R divide ratio (see Figure 67 and Table 11). For the relationship between R, D, and the  $f_{REF}$ ,  $f_{PFD}$ ,  $f_{VCO}$ , and  $f_{OUT}$  frequencies, see the Output Frequency section. The state of the DCLK\_MODE bit is determined by Table 17.



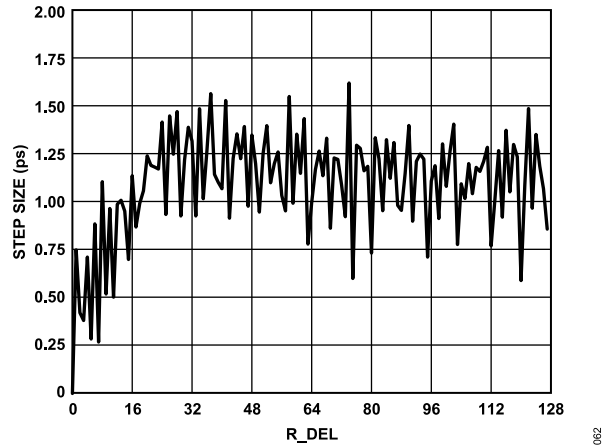
**Figure 67. Reference Divider and Doubler**

**Table 11. *EN\_RDBLR* and *R\_DIV* Programming**

EN_RDBLR	R_DIV[5:0]	R	D
1	Not applicable	Not applicable	2
0	0	1	Not applicable
0	1	1	Not applicable
0	...	...	Not applicable
0	63	63	Not applicable

**Reference Delay**

A 7-bit delay, R\_DEL, is used to increase the propagation delay from the reference input pins to the clock output pins. Use the R\_DEL[6:0] bits to directly program the reference delay ( $t_{RDEL}$ ), which typically ranges from 0 ps to 127 ps in 1 ps steps (see Figure 68).



**Figure 68. Typical Reference Delay Step Size vs. R\_DEL Register Setting**

INV\_CLKOUT, N\_DEL, and R\_DEL can be used in conjunction to align the multichip output-to-output skew to within  $\pm 0.5$  ps. Figure 45 shows that the largest R\_DEL settings may increase  $L_{NORM}$  by 1 dB. INV\_CLKOUT does not degrade performance and must be used to adjust for multichip output-to-output skews greater than a quarter of the  $1/f_{OUT}$  period, in lieu of a large N\_DEL or R\_DEL value. As a result, the maximum  $t_{RDEL}$  adjustment never needs to be more than a quarter of the  $1/f_{OUT}$  period. For the relationship between R\_DEL, N\_DEL, INV\_CLKOUT, BLEED\_I, and BLEED\_POL, see the Aligning Multiple ADF4378 Output Phases section.

**SYSREF Input Buffer**

The distributed SYSREF signal to be relocked is applied differentially to the SR\_INP and SR\_INN pins. The SYSREF input of the ADF4378 supports a range of signal types. The SR\_SEL bit in REG0042 has two settings. SR\_SEL = 0 sets the ADF4378 SYSREF input buffer for CML/LVPECL operation and the internal common mode voltage is set to 1.85 V. SR\_SEL = 1 sets the input buffer for a generic LVDS input and the internal common mode voltage is set to 1.3 V. Alternatively, it is possible to use a single-ended configuration by programming SR\_SEL = 1 and

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designing a bias network for SR\_INP and SR\_INN. For an example of SYSREF interface networks, see the [SYSREF Input Network](#) section. The ADF4378 supports continuous, burst, random, or a single pulse SYSREF signal.

**SYSREF Monitor**

A SYSREF monitor is provided at the SR\_INP and SR\_INN inputs to detect the presence of a SYSREF signal and to check the setup and hold time of the SYSREF and reference. This is reported through the SR\_OK status flag, which is available through serial-port register, REG0049. If the SYSREF monitor detects a discrepancy with the SR\_IN setup and hold time, SR\_OK shows 0 after a read back, which indicates a fault event. The SR\_OK bit also shows 0 when the SYSREF output is disabled, either by using the PD\_SYSOUT control or the ENSR pin. When SR\_OK shows 0 after a read back, it continues to read back 0 until the SYSREF monitor is reset correctly by setting RST\_SR\_MON in REG0042 to 1 and then back to 0. Then SR\_OK continues to read back 1, assuming the timing is within the limits of the SYSREF monitor.

**SYSREF Delay**

A 7-bit delay, SR\_DEL, may be used to increase delay skew from the SYSREF output and clock output. The SR\_DEL bits, Bits[6:0], in REG0043 are used to set the delay.

The ADF4378 ensures the SYSREF output edge stays within one CLKP and CLKN period over temperature. The SR\_DEL bits allow adjustment delay steps of approximately 0.8 ps.

With INV\_SR in REG0043 = 0, the SYSREF aligns with a clock rising edge. The retiming edge may be inverted, which also has the effect of adding an additional 0.5 × clock period of delay. To enable this, set INV\_SR in REG0043 = 1.

**Phase/Frequency Detector (PFD)**

The PFD, in conjunction with the charge pump, produces source and sink current pulses proportional to the phase difference between the outputs of the reference divider or reference doubler and feedback divider. This action provides the necessary feedback to phase-lock the loop, which forces a phase alignment at the inputs of the PFD. For a simplified schematic of the PFD, see [Figure 69](#).

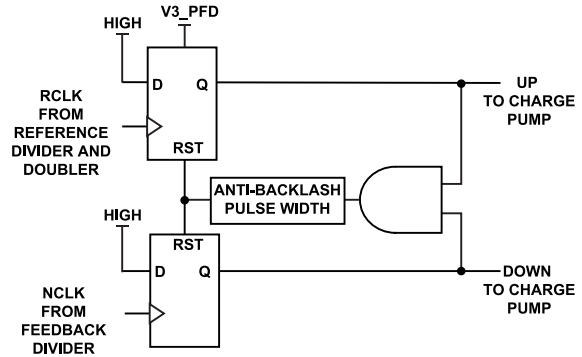


Figure 69. Simplified PFD Schematic

**Charge Pump**

The charge pump, controlled by the PFD, forces sink (down) or source (up) current pulses onto the CP pin, which must be connected to an appropriate loop filter. For a simplified schematic of the charge pump, see [Figure 70](#).

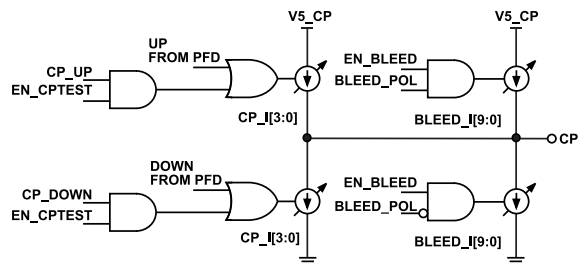


Figure 70. Simplified Charge-Pump Schematic

The output current magnitude ( $I_{CP}$ ) may be set from 0.79 mA to 11.1 mA using the CP\_I bits, Bits[3:0]. A larger  $I_{CP}$  can result in lower in-band noise ( $L_{NORM}$ ) due to the lower impedance of the loop filter components. A smaller  $I_{CP}$  can result in better spurious performance. For programming specifics, see [Table 12](#), and for information on designing a loop filter, see the [Applications Information](#) section.

Table 12. CP Programming

CP_I, Bits[3:0]	$I_{CP}$
0	0.79 mA
1	0.99 mA
2	1.19 mA
3	1.38 mA
4	1.59 mA
5	1.98 mA
6	2.39 mA
7	2.79 mA
8	3.18 mA
9	3.97 mA
10	4.77 mA
11	5.57 mA
12	6.33 mA

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Table 12. CP Programming (Continued)

CP_I, Bits[3:0]	I <sub>CP</sub>
13	7.91 mA
14	9.51 mA
15	11.1 mA

## Charge-Pump Test Mode

When the EN\_CPTTEST bit is set to 1, the CP\_UP bit and CP\_DOWN bit can be programmed to force a constant I<sub>CP</sub> source or sink current, respectively, on the CP pin. These bits are commonly used as an aid to debug PLL related issues during the hardware and software development phase of a project. For normal operation, set EN\_CPTTEST, CP\_UP, and CP\_DOWN to 0. For more information, see Figure 70 and Table 13.

Table 13. Charge-Pump Debug Functions

EN_CPTTEST	CP_UP	CP_DOWN	CP Pin State	Debug Test
1	0	0	High-Z	VCO open loop
1	1	0	~V <sub>V5_CP</sub>	Charge-pump output voltage verification
1	0	1	~GND	Charge-pump output voltage verification
0	0	0	Normal operation	Not applicable

## Charge-Pump Bleed Current

A small programmable constant charge-pump current, known as bleed current, can be used to either increase or decrease the propagation delay from the reference input pins to the clock output pins.

To enable the bleed current, set the EN\_BLEED bit to 1. When the BLEED\_POL bit is set to 1, a small constant source current is forced onto the CP pin. When the BLEED\_POL is set to 0, a small constant sink current is forced onto the CP pin (see Figure 70).

The bleed-current LSB step size is 536 nA. The bleed-current delay step size (t<sub>IDEL-STEP</sub>) is a function of the bleed-current step size (I<sub>CP</sub>) and f<sub>PFD</sub>, as shown in Equation 9. Figure 71 provides a quick reference of t<sub>IDEL-STEP</sub> vs. several common I<sub>CP</sub> and f<sub>PFD</sub> values.

$$t_{IDEL-STEP} = \frac{536 \text{ nA}}{I_{CP} \times f_{PFD}} \quad (9)$$

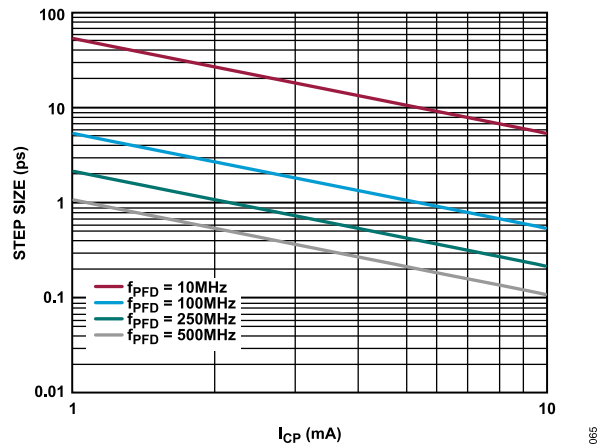


Figure 71. Bleed-Current Delay Step Size

Bleed-current delay (t<sub>IDEL</sub>) is determined by t<sub>IDEL-STEP</sub>, the BLEED\_POL bit, and BLEED\_I bit fields, Bits[9:0] (see Equation 10 and Equation 11).

If BLEED\_POL = 0, the propagation delay from the REFP and REFN input pins to the CLKP and CLKN output pins increases (see Figure 21).

$$t_{IDEL} = t_{IDEL-STEP} \times BLD\_I \quad (10)$$

where BLD\_I represents the decimal value of the BLEED\_I bit field, Bits[9:0].

If BLEED\_POL = 1, the propagation delay from the REFP and REFN input pins to the CLKP and CLKN output pins decreases (see Figure 24).

$$t_{IDEL} = -t_{IDEL-STEP} \times BLD\_I \quad (11)$$

The maximum t<sub>IDEL</sub> for proper lock detector functionality is based on the LDWIN\_PW setting, as shown in Table 16.

INV\_CLKOUT, BLEED\_I, and BLEED\_POL can be used in conjunction to align the multichip output-to-output skew to as small as ±0.05 ps (see Equation 9). The largest BLEED\_I settings may increase L<sub>NORM</sub> by 1 dB and L<sub>1/f</sub> by 4 dB, as shown in Figure 42. INV\_CLKOUT does not degrade performance and must be used to adjust for multichip output-to-output skews greater than a quarter of the 1/f<sub>OUT</sub> period, in lieu of a large BLEED\_I value. As a result, the maximum t<sub>IDEL</sub> adjustment never needs to be more than a quarter of the 1/f<sub>OUT</sub> period. For the relationship between R\_DEL, N\_DEL, INV\_CLKOUT, BLEED\_I bit fields, Bits[9:0], and BLEED\_POL, see the Applications Information section.

## Lock Detector

The lock detector uses internal signals from the PFD to measure phase coincidence between the output signal of the reference divider and doubler (RCLK) in Figure 67 and the output signal of the feedback divider (NCLK) in Figure 77. It is enabled by setting both the EN\_LOL bit and the EN\_LDWIN bit to 1 and presents the

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lock detector output on the LKDET pin and the LOCKED bit. The lock detector output can also be presented on the MUXOUT pin by programming the MUXOUT bits, Bits[4:0] (see Figure 81). The register bit field CMOS\_OV determines if the logic high level for the MUXOUT, LKDET, SDO, and SDIO output pins is 3.3 V or 1.8 V.

The PFD phase difference must be less than the phase difference lock window time ( $t_{LDWIN}$ ) for a set number of PFD cycles before the lock detector output indicates that the PLL has locked. The required number of PFD cycles varies if a designer prioritizes lock detect accuracy or speed. Five loop filter time constants can be used as an initial estimate of the desired number of PFD cycles, as shown in Equation 12. The required number of PFD cycles is set by the LD\_COUNT bits, Bits[4:0], as shown in Table 14. For more information, see Figure 72 and Table 15.

$$PFD\ Cycles = \frac{5 \times f_{PFD}}{2 \times \pi \times LPBW} \tag{12}$$

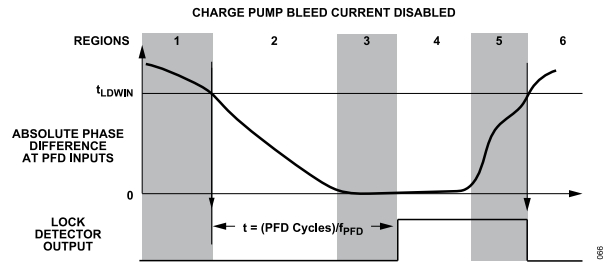
where LPBW = loop filter bandwidth.

**Table 14. LD\_COUNT Programming**

LD_COUNT Bits, Bits[4:0]	PFD Cycles
0	23
1	32
2	47
3	66
4	95
5	134
6	191
7	270
8	383
9	542
10	767
11	1085
12	1535
13	2171
14	3071
15	4343
16	6143
17	8687
18	12287
19	17376
20	24575
21	34754
22	49151
23	69510
24	98303
25	139021
26	196607
27	278044
28	393215
29	556090
30	786431

**Table 14. LD\_COUNT Programming (Continued)**

LD_COUNT Bits, Bits[4:0]	PFD Cycles
31	1112181

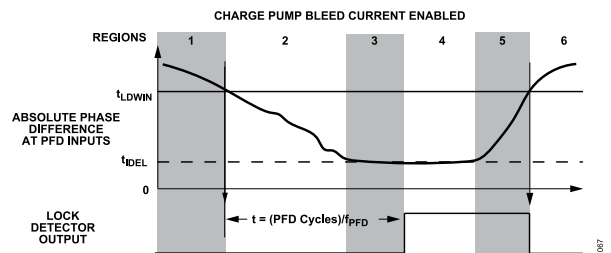


**Figure 72. Lock Detector Timing, Bleed Current Disabled**

**Table 15. Lock Detector Timing, Bleed Current Disabled**

Region	Absolute Phase Difference at PFD	Lock Detector State
1	$> t_{LDWIN}$	Low
2	$< t_{LDWIN}$	Low, counts PFD cycles
3	$\sim 0$	Low, counts PFD cycles
4	$\sim 0$	High, $\geq$ required PFD cycle count
5	$< t_{LDWIN}$	High
6	$> t_{LDWIN}$	Low (immediately)

When the charge-pump bleed current is enabled, a phase offset ( $t_{IDEL}$ ) is applied to the PFD inputs. This phase offset ( $t_{IDEL}$ ) is proportional to the amount of bleed current programmed in Equation 10 and Equation 11. Region 3 and Region 4 in Figure 72 and Figure 73 highlight the PFD phase difference that the PLL settles to when the charge-pump bleed current is disabled or enabled, respectively.



**Figure 73. Lock Detector Timing, Bleed Current Enabled**

For proper operation of the lock detector, the absolute value of  $t_{IDEL}$  must be less than  $t_{LDWIN}$ . The user sets the phase difference lock window time ( $t_{LDWIN}$ ) for a valid lock condition with the LDWIN\_PW bit. In most cases, LDWIN\_PW must be set to 0. To understand the relationship between the LDWIN\_PW bit and maximum allowable  $t_{IDEL}$ , see Table 16.

**Table 16. Maximum  $t_{IDEL}$**

LDWIN_PW	$t_{IDEL(MAX)}$
0	$\pm 150$ ps
1	$\pm 250$ ps

THEORY OF OPERATION

VCO

The VCO core consists of four separate VCOs, each of which uses 256 overlapping bands, which allows the device to cover a wide frequency range without large VCO sensitivity ( $K_{VCO}$ ). The output frequency can be further extended by utilizing the output divider (see Figure 74).

The correct register values for the VCO\_CORE, VCO\_BAND, and VCO\_BIAS settings are determined by performing a VCO calibration. For more information, see the VCO Calibration section. After a VCO calibration is performed for a specific device and frequency, the VCO\_CORE, VCO\_BAND, and VCO\_BIAS values can be recorded. These recorded values may be programmed manually on subsequent power ups when the same device and frequency are used, thereby avoiding the VCO calibration time.

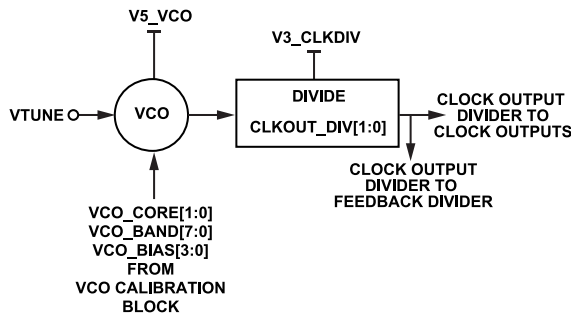


Figure 74. VCO and Clock Output Divider

VCO Calibration

A VCO calibration is required to select the correct VCO core, band, and bias settings for a specific VCO frequency. To perform a VCO calibration, several registers must be setup as described in this section. This procedure assumes that the device is powered up, the required reference frequency is present on the REFP and REFN pins, and all other registers are programmed correctly. Figure 75 and Figure 76 are provided as visual aids for this procedure.

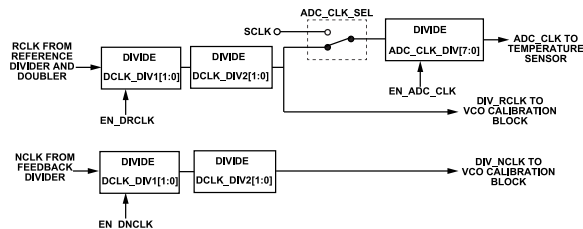


Figure 75. VCO Calibration Dividers

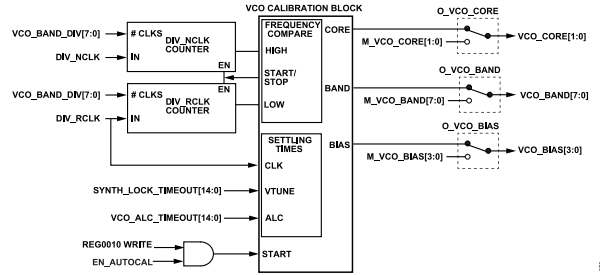


Figure 76. VCO Calibration Block

To perform a VCO calibration, set up several registers as outlined in the following procedure:

1. Set register bits based on the RCLK column in Table 22.
2. Set DCLK\_DIV1 = 1. Set CAL\_CT\_SEL, DCLK\_DIV2, and DCLK\_MODE to the values given in Table 17. Record  $f_{DIV\_RCLK}$  for later use.
3. Calculate and set the minimum values for the SYNTH\_LOCK\_TIMEOUT bit fields, Bits[14:0], the VCO\_ALC\_TIMEOUT bit fields, Bits[14:0], and the VCO\_BAND\_DIV bits. Typical automatic VCO calibration times are 3 ms to 9 ms when minimum values are chosen for these parameters. Larger values produce longer VCO calibration times.

$$SYNTH\_LOCK\_TIMEOUT \geq \text{Ceiling} (200 \mu s \times f_{DIV\_RCLK}) \tag{13}$$

$$VCO\_ALC\_TIMEOUT \geq \text{Ceiling} (50 \mu s \times f_{DIV\_RCLK}) \tag{14}$$

$$VCO\_BAND\_DIV \geq \text{Ceiling} \left( \frac{15 \mu s \times f_{DIV\_RCLK}}{16 \times 2^{DCLK\_MODE}} \right) \tag{15}$$

4. Ensure that the ADC\_CLK\_DIV bits are set so that the required analog-to-digital converter (ADC) clock frequency is <400 kHz.

$$ADC\_CLK\_DIV > \text{Ceiling} \tag{16}$$

$$\left( \frac{f_{DIV\_RCLK}}{400 \text{ kHz}} - 2 \right) / 4$$

5. Set the N\_INT bit fields, Bits[11:0], CLKOUT\_DIV bits, R\_DIV bits, and EN\_RDBLR bits by programming REG0010 last. Any write to REG0010 starts the VCO automatic calibration.
6. This is an optional step. Monitor the register bits, ADC\_BUSY, and FSM\_BUSY. The calibration is finished when ADC\_BUSY transitions from high to low, followed by FSM\_BUSY transitioning from high to low.

**THEORY OF OPERATION**

- After the VCO calibration is complete, disable calibration clocks to limit unwanted spurious content by setting  $EN\_DRCLK = EN\_DNCLK = EN\_ADC\_CLK = 0$ .
- This is an optional step. Read back the VCO\_CORE, VCO\_BAND, and VCO\_BIAS bits, and then record the read-back values. These values can be used to bypass calibration and manually program the M\_VCO\_CORE, M\_VCO\_BAND, and M\_VCO\_BIAS bits for a given device and frequency, as described in the [Fast Power-Up and Initialization, Manually Programmed VCO Calibration Settings \(Optional\)](#) section.

**Table 17. CAL\_CT\_SEL, DCLK\_DIV2, and DCLK\_MODE Setup**

f <sub>PF</sub> D (MHz)	CAL_CT_SEL	DCLK_DIV2	DCLK_MODE	f <sub>DIV_RCLK</sub> (MHz)
≤160	1	0	0	f <sub>PF</sub> D/2
>160 and ≤250	1	0	1	f <sub>PF</sub> D/2
>250 and ≤320	0	1	0	f <sub>PF</sub> D/4
>320 and ≤500	0	1	1	f <sub>PF</sub> D/4

**Clock Output Divider**

A 2-bit divider, CLKOUT\_DIV, in [Figure 74](#) is used to reduce the frequency seen at the output buffer and feedback divider. The clock output divide value (O) may be set to 1, 2, 4, or 8. Use the CLKOUT\_DIV bit to directly program the divide ratio. CLKOUT\_DIV is located inside the PLL loop. Therefore, any change to CLKOUT\_DIV requires a change to the N\_INT bit fields, Bits[11:0] to maintain the same f<sub>PF</sub>D and results in the PLL losing lock for a few loop time constants. For more information, see [Table 18](#). For the relationship between the f<sub>REF</sub>, f<sub>PF</sub>D, f<sub>VCO</sub>, and f<sub>OUT</sub> frequencies, see the [Output Frequency](#) section.

**Table 18. CLKOUT\_DIV Programming**

CLKOUT_DIV	Clock Output Divide Value (O)	Output Frequency Range (GHz)
0	1	6.4 ≥ f <sub>OUT</sub> ≤ 12.8
1	2	3.2 ≥ f <sub>OUT</sub> ≤ 6.4
2	4	1.6 ≥ f <sub>OUT</sub> ≤ 3.2
3	8	0.8 ≥ f <sub>OUT</sub> ≤ 1.6

**Output Invert (INV\_CLKOUT)**

The output invert (INV\_CLKOUT) is used to shift the output signal 180° with respect to the rising edge of the reference input signal, when f<sub>OUT</sub> is an integer multiple of f<sub>REF</sub>. For more information, see [Table 19](#). INV\_CLKOUT is located inside the PLL loop, and any change to INV\_CLKOUT results in the PLL losing lock for few a loop time constants. Use the INV\_CLKOUT bit to directly program the output phase.

**Table 19. INV\_CLKOUT Programming**

f <sub>OUT</sub> /f <sub>REF</sub> =	INV_CLKOUT	Each Reference Rising Edge Aligned to
Integer	0	CLKP rising edge
Integer	1	CLKP falling edge

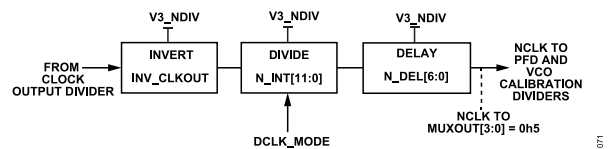
**Table 19. INV\_CLKOUT Programming (Continued)**

f <sub>OUT</sub> /f <sub>REF</sub> =	INV_CLKOUT	Each Reference Rising Edge Aligned to
Noninteger	x	Varies

INV\_CLKOUT, N\_DEL, R\_DEL, BLEED\_I, and BLEED\_POL can be used in conjunction to align the multichip output-to-output skew to sub ps levels. INV\_CLKOUT does not degrade performance and must be used to adjust for multichip output-output skews greater than a quarter of the 1/f<sub>OUT</sub> period, in lieu of a large N\_DEL, R\_DEL, or BLEED\_I value. For the relationship between R\_DEL, N\_DEL, INV\_CLKOUT, BLEED\_I, and BLEED\_POL, see the [Aligning Multiple ADF4378 Output Phases](#) section.

**Feedback Divider (N)**

A 12-bit divider, the N\_INT bit fields, Bits[11:0], in [Figure 77](#), is used to reduce the frequency seen at the output of the clock output divider. The feedback divider closes the feedback loop from the VCO and clock output divider to the PFD.



**Figure 77. Feedback Divider**

The feedback divider divide ratio (N) may be programmed to any integer from 2 to 4095. Use the N\_INT bit fields, Bits[11:0] to directly program the N divide ratio (see [Table 20](#)). For the relationship between N, O, and the f<sub>REF</sub>, f<sub>PF</sub>D, f<sub>VCO</sub>, and f<sub>OUT</sub> frequencies, see the [Output Frequency](#) section. The state of the DCLK\_MODE bit is determined by [Table 17](#).

**Table 20. N\_INT Programming**

N_INT Bit Fields, Bits[11:0]	N
0	Not applicable
1	Not applicable
2	2
3	3
...	...
4095	4095

**Feedback Delay**

A 7-bit delay, N\_DEL, is used to decrease the propagation delay from the REFP and REFN input pins to the CLKP and CLKN output pins. Use the N\_DEL bits to directly program the feedback delay (t<sub>NDEL</sub>), which typically ranges from 0 ps to 110 ps in 0.85 ps steps (see [Figure 78](#)).

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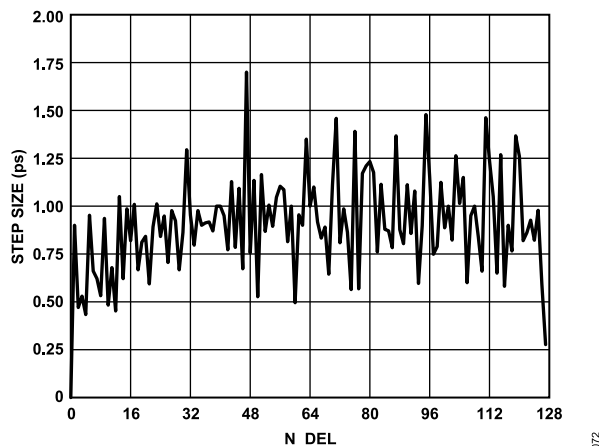


Figure 78. Step Size vs. N\_DEL, Typical Feedback Delay

INV\_CLKOUT, N\_DEL, and R\_DEL can be used in conjunction to align the multichip output-to-output skew to within  $\pm 0.5$  ps. Figure 45 shows that the largest N\_DEL settings may increase  $L_{NORM}$  by 1 dB. INV\_CLKOUT does not degrade performance and can be used to adjust for multichip output-to-output skews greater than a quarter of the  $1/f_{OUT}$  period, in lieu of a large N\_DEL or R\_DEL value. As a result, the maximum  $t_{NDEL}$  adjustment never has to be more than a quarter of the  $1/f_{OUT}$  period. For the relationship between R\_DEL, N\_DEL, INV\_CLKOUT, BLEED\_I bit fields, Bits[9:0], and BLEED\_POL, see the [Aligning Multiple ADF4378 Output Phases](#) section.

**Clock Output Buffer**

The low noise, differential output buffer in Figure 79 produces a differential output voltage. The output amplitude level and common mode voltage is settable with the CLKOUT\_OP bits according to Table 21. Each output can be either AC-coupled or DC-coupled and terminated with  $100 \Omega$ , differentially. If a single-ended output is required, then each side of the output must be individually AC-coupled and terminated with  $50 \Omega$  (see Figure 109).

Table 21. CLKOUT\_OP Programming

CLKOUT_OP	Differential Amplitude ( $V_{OD}$ )	Common-Mode Voltage
0	320 mV <sub>PEAK</sub>	$V_{CLK} - 1.2 \times V_{OD}$
1	420 mV <sub>PEAK</sub>	$V_{CLK} - 1.2 \times V_{OD}$
2	530 mV <sub>PEAK</sub>	$V_{CLK} - 1.2 \times V_{OD}$
3	640 mV <sub>PEAK</sub>	$V_{CLK} - 1.2 \times V_{OD}$

The output can be powered down by either setting the ENCLK pin and low or programming the PD\_CLKOUT and bit to 1. The EN\_CLK bit reports the state of the  $\overline{ENCLK}$  pin. When powered down, the output sources a common-mode voltage around 2 V.

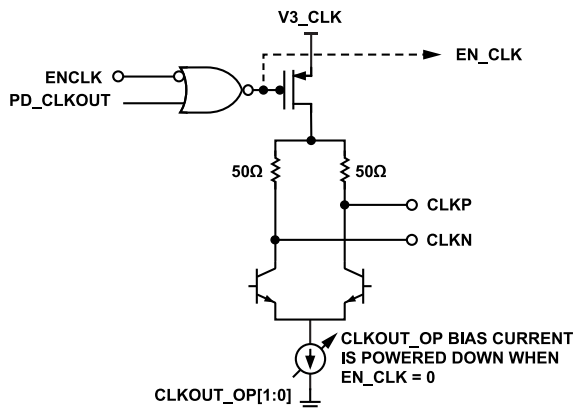


Figure 79. Simplified Clock Output

**SYSREF Output Buffer**

The retimed SYSREF output is available as an LVDS compatible signal on the SR\_OUTP and SR\_OUTN pins with a common-mode voltage of approximately 1.2 V. Figure 80 shows a simplified schematic of the SYSREF output buffer. The SYSREF output can be powered down by either setting the ENSR pin LOW or programming the PD\_SYSOUT bit to 1. The register bits EN\_SYS in REG0049 report the logic on the ENSR pin.

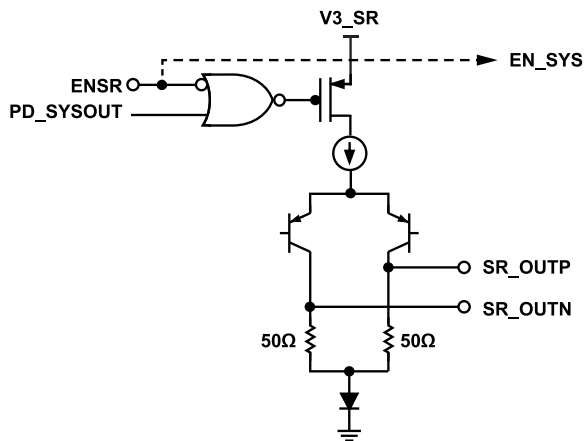


Figure 80. Simplified SYSREF Output Interface

THEORY OF OPERATION

MUXOUT

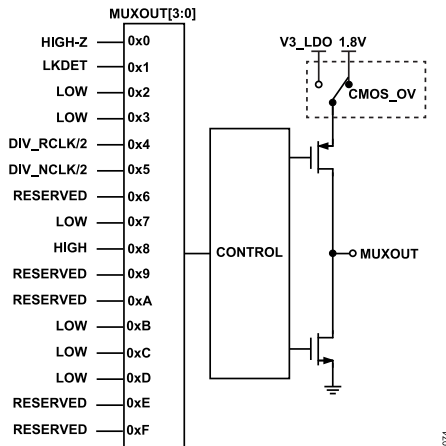


Figure 81. MUXOUT

The state of the MUXOUT pin is determined by the SPI register bit field MUXOUT, which allows the user access to various internal nodes. The MUXOUT pin and MUXOUT bits are commonly used as an additional lock status output or to debug PLL related issues during the hardware and software development phase of a project. The CMOS\_OV bit field determines if the logic high level for the MUXOUT pin, LKDET pin, SDO pin, and SDIO pin is 3.3 V or 1.8 V (see Figure 81).

Temperature Sensor

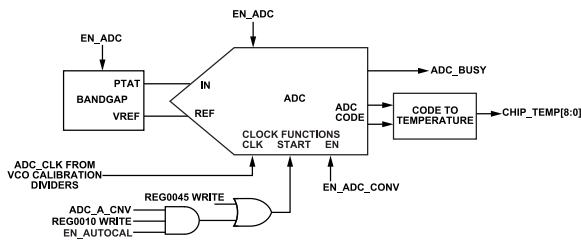


Figure 82. Temperature Sensor

The temperature sensor is composed of an 8-bit ADC, which measures the proportional to absolute temperature (PTAT) voltage with respect to the VREF voltage of a bandgap. The purpose of the temperature sensor is to measure changes in die temperature, not the absolute junction temperature.

The maximum ADC clock frequency is 400 kHz. Equation 16 calculates the correct ADC\_CLK\_DIV value. The ADC clock may be generated from either the SPI clock or the RCLK (see Figure 75). Before an ADC measurement can occur, program the registers of the ADF4378 as shown in Table 22.

Table 22. ADC Register Setup for SPI Clock and RCLK

Bits	RCLK <sup>1</sup>	SPI Clock
ADC_CLK_SEL	0	1
EN_DRCLK, EN_DNCLK	1	Not applicable

Table 22. ADC Register Setup for SPI Clock and RCLK (Continued)

Bits	RCLK <sup>1</sup>	SPI Clock
ADC_A_CONV, EN_AUTOCAL	1 <sup>1</sup>	Not applicable
EN_ADC_CNVR, EN_ADC, EN_ADC_CLK	1	
PD_ADC	0	

<sup>1</sup> Required when writing to REG0010 to start the ADC conversion and VCO calibration.

After the bits in Table 22 are programmed, start an ADC conversion with either, a register write to REG0045 or a register write to REG0010 (RCLK only). With a REG0010 write, a VCO calibration (see the VCO Calibration section) begins immediately after the ADC conversion is complete. An ADC conversion requires 17 clock cycles to complete. In serial port register REG0049, the ADC\_BUSY bit monitors the conversion status. During a conversion, ADC\_BUSY is set to 1 and on conversion completion, ADC\_BUSY is set to 0.

Measurements are recorded in the CHIP\_TEMP bit fields, Bits[8:0], in REG004C and REG004D (see Figure 82).

If an ambient temperature measurement is required, program the ADF4378 to a low power state, as shown in Table 23. For ambient temperature measurements, the SPI clock is the only available clock option.

Table 23. Ambient Temperature Full Power-Down Register Setup

Bit Fields	State
ADC_CLK_SEL	1
PD_ADC	0
PD_CLK, PD_RDDET, PD_CALDAC, PD_NDIV, PD_VCO, PD_LD, PD_PFDCCP, PD_CLKOUT, PD_SYSOUT, PD_RDIV	1

Double Buffering

Double buffering refers to a main/subordinate configuration for the bit fields shown in Table 24. Only the subordinate bit fields control the actual state of the ADF4378. When double buffering is enabled for a bit field, the serial interface only writes to the main bit field. The subordinate bit field retains its previous value until a register write is sent to REG0010. After writing to REG0010, all main bit fields are automatically loaded to their respective subordinate bit field. Writing to REG0010 also starts the autocalibration of the VCO (see the VCO Calibration section). This allows the user to update several bit fields that change the output frequency of the ADF4378 and start a new VCO calibration on the same register write. When double buffering is disabled, the serial interface writes directly to the subordinate bit field.

It is possible to read back the state of either the main or subordinate bit fields by enabling or disabling the MASTER\_READBACK\_CONTROL bit.



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**Table 24. Double Buffer Enable Bits and Bit Fields**

Double Buffer Enable Bits	Double Buffered Bit Fields
Not applicable, always enabled	N_INT bits, Bits[11:0], R_DIV, EN_RDBLR, CP_I
CLKODIV_DB	CLKOUT_DIV
DCLK_DIV_DB	DCLK_DIV1, DCLK_DIV2
O_VCO_DB	M_VCO_CORE, M_VCO_BAND, M_VCO_BIAS
DEL_CTRL_DB	INV_CLKOUT, BLEED_I bits, Bits[9:0], BLEED_POL, N_DEL, R_DEL

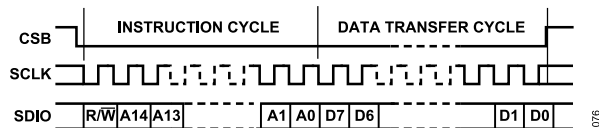
### Serial Port

The SPI-compatible serial port provides control and monitoring functionality. The CMOS\_OV bit determines if the logic high level for the SDO and SDIO SPI output pins is 3.3 V or 1.8 V. CMOS\_OV also sets the output level for MUXOUT and LKDET.

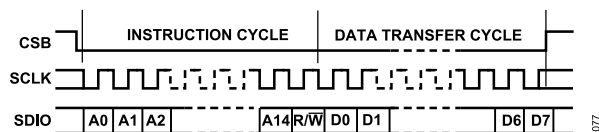
The serial port can be programmed to support several different configurations in REG0000 and REG0001.

The SDO\_ACTIVE bit determines if the serial port is configured as a 3-wire or 4-wire serial interface (see the timing diagrams [Figure 2](#), [Figure 3](#), and [Figure 4](#)).

As shown in [Figure 83](#) and [Figure 84](#), the instruction cycle is composed of 16 bits. The fifteen LSB bits determine the register address, and the MSB determines if data is written to or read from the serial interface during the data transfer cycle. The LSB\_FIRST bit determines the data orientation of the instruction cycle and data transfer cycle of the serial interface.



**Figure 83. Serial Interface, MSB First (LSB\_FIRST = 0)**



**Figure 84. Serial Interface, LSB First (LSB\_FIRST = 1)**

The SPI register map can be programmed with single instructions, as shown in [Figure 83](#) and [Figure 84](#), or in streaming mode, as shown in [Figure 85](#). Streaming mode allows for efficient data transfer read or write cycles to multiple registers. Streaming mode allows the user to program a bit stream composed of one register address in the instruction header and data for that register address, which is then followed by data in subsequent register addresses. The ADDRESS\_ASCENSION bit determines if the subsequent register addresses are incremented or decremented. It is recommended to decrement the register addresses in streaming mode (ADDRESS\_ASCENSION = 0). The reason for this recommendation is

because REG0010 triggers the VCO calibration and loading of all double buffers and, therefore, must be the last SPI register written to. The SINGLE\_INSTRUCTION bit disables streaming mode when it is set to 1. When SINGLE\_INSTRUCTION is set to 0, streaming mode is enabled.

### Block Power-Down Control

The power-down control bits of the ADF4378 reside in REG0019 and REG001A. The PD\_ALL, PD\_RDDET, PD\_CLKOUT, and PD\_SYSOOUT bits may be programmed independently.

The PD\_CLK, PD\_CALDAC, PD\_RDIV, PD\_NDIV, PD\_VCO, PD\_LD, and PD\_PFDPCP bits must be set to the same state at all times. The only time this group is allowed to be set to 1 is when a full power-down ambient temperature measurement is performed (see [Table 23](#)). In all other cases, this bit grouping must be set to 0.

THEORY OF OPERATION

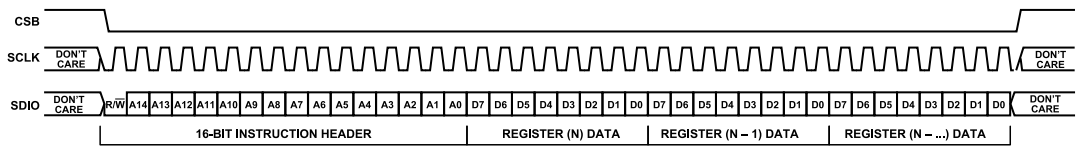


Figure 85. Serial Interface, Recommended Streaming Mode (SINGLE\_INSTRUCTION = 0) with Decrementing Registers (ADDRESS\_ASCENCION = 0)

APPLICATIONS INFORMATION

LOOP FILTER DESIGN

A stable loop filter design requires care in selecting the loop filter components of the ADF4378. It is recommended to download and install ADIsimPLL™ for loop filter design and simulation. ADIsimPLL has an integrated tutorial for first time users and a help manual for more complex topics. There are also several ADIsimPLL training videos available on [www.analog.com](http://www.analog.com). After a loop filter has been designed and simulated, it is recommended to verify the new loop filter using the ADF4378 evaluation hardware.

A full loop filter design tutorial is beyond the scope of this data sheet. However, some best practices are shown in the following list. ADIsimPLL aids in defining and simulating these parameters. Any significant change to these items requires a new loop filter design.

1. A stable loop filter must meet the following criteria:
  - a. Loop filter phase margin > 45°
  - b. Loop filter bandwidth <  $f_{PFD} \div 10$
2. The required loop filter bandwidth is determined by the following features of the ADF4378:
  - a.  $I_{CP}$
  - b.  $K_{VCO}$
  - c. PFD frequency
  - d. Reference input phase noise (for more information, see the [Reference Phase Noise](#) section).
  - e. Trade-off between minimizing jitter or settling time (for more information, see the [Output Phase Noise Characteristics](#) section and [Equation 12](#), respectively).

The VTUNE pin has an internal 30 pf capacitor to GND that must be included in the loop filter design. ADIsimPLL takes this internal capacitance into account automatically.

REFERENCE SOURCE CONSIDERATIONS

Reference Input Network

The reference input buffer of the ADF4378, shown in [Figure 66](#), provides a flexible interface to either differential or single-ended frequency sources. [Figure 86](#) to [Figure 91](#) show recommended interfaces for different reference signal types. All  $Z_0$  signal traces are 50 Ω transmission lines in [Figure 86](#), [Figure 87](#), [Figure 88](#), [Figure 89](#), [Figure 90](#), and [Figure 91](#).

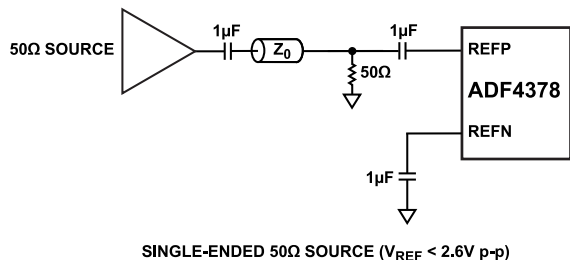


Figure 86. Single-Ended 50 Ω Source ( $V_{REF} < 2.6 V_{p-p}$ )

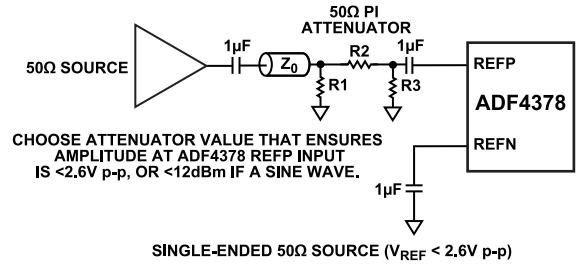


Figure 87. Single-Ended 50 Ω Source ( $V_{REF} > 2.6 V_{p-p}$ )

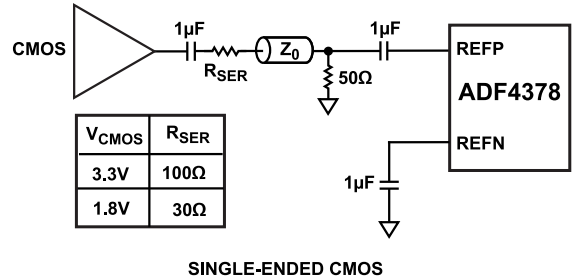


Figure 88. Single-Ended CMOS

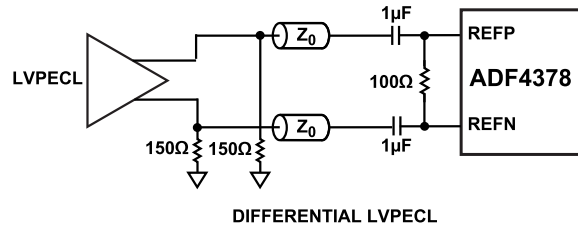


Figure 89. Differential LVPECL

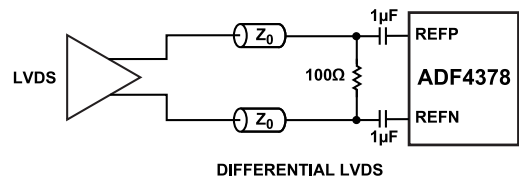


Figure 90. Differential LVDS

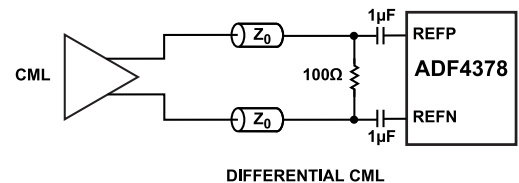


Figure 91. Differential CML

SYSREF Input Network

The ADF4378's SYSREF input may be programmed for CML/LVPECL or LVDS interfaces using the SR\_SEL bit to support a range of input SYSREF signal levels. [Figure 92](#) to [Figure 95](#) show the examples of SYSREF input interfaces.

APPLICATIONS INFORMATION

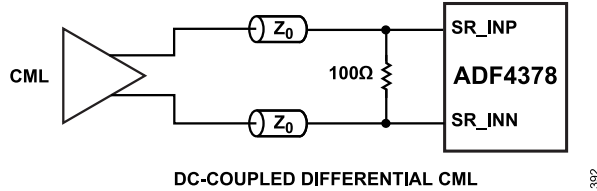


Figure 92. DC-Coupled Differential CML (Set SR\_SEL = 0)

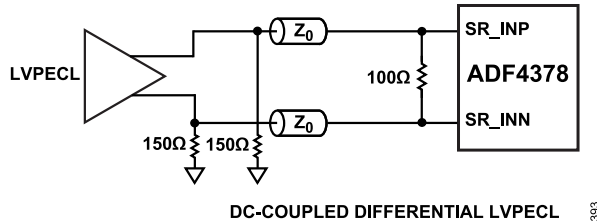


Figure 93. DC-Coupled Differential LVPECL (Set SR\_SEL = 0)

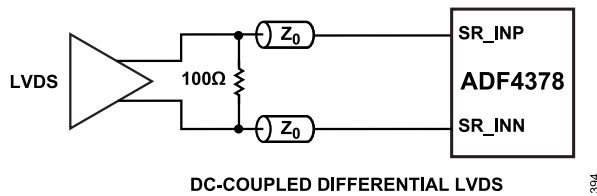


Figure 94. DC-Coupled Differential LVDS (Set SR\_SEL = 1)

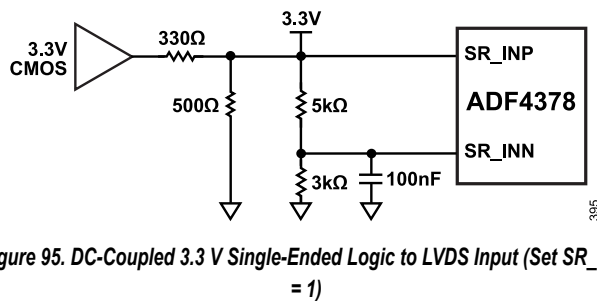


Figure 95. DC-Coupled 3.3 V Single-Ended Logic to LVDS Input (Set SR\_SEL = 1)

Reference Phase Noise

The ADF4378 achieves an in-band normalized phase noise floor of  $L_{NORM} = -239$  dBc/Hz typical. To calculate the equivalent input phase noise floor ( $L_{IN}$ ), use the following Equation 17, which is plotted in Figure 96.

$$L_{IN} = L_{NORM} + 10 \times \log_{10}(f_{REF}) \tag{17}$$

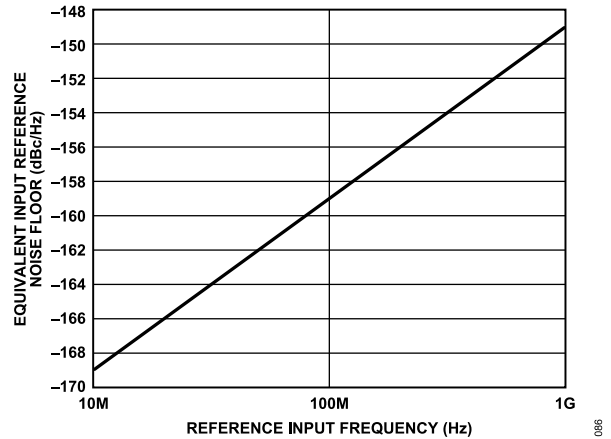


Figure 96. Equivalent Reference Input Phase Noise Floor vs.  $f_{REF}$

For example, a 100 MHz reference input frequency gives an  $L_{IN}$  of  $-159$  dBc/Hz. The phase noise of the reference frequency source must be at least 6 dB less than  $L_{IN}$  to avoid impacting and increasing the overall system phase noise.

To maintain typical  $L_{NORM}$  performance, Table 7 provides criteria for selecting the optimal REF\_SEL setting based on the input reference signal type and amplitude.

OUTPUT PHASE NOISE CHARACTERISTICS

In-Band Output Phase Noise

The in-band phase noise floor ( $L_{OUT}$ ) produced at  $f_{OUT}$  may be calculated by Equation 18 and Equation 19.

$$L_{OUT} = L_{NORM} + 10 \times \log_{10}(f_{PFD}) + 20 \times \log_{10}\left(\frac{f_{OUT}}{f_{PFD}}\right) \tag{18}$$

or

$$L_{OUT} = L_{NORM} + 10 \times \log_{10}(f_{PFD}) + 20 \times \log_{10}\left(\frac{N}{O}\right) \tag{19}$$

where  $L_{NORM} = -239$  dBc/Hz. See Figure 42 to Figure 47, which show  $L_{NORM}$  variation vs.  $I_{CP}$ ,  $N_{DEL}$ ,  $R_{DEL}$ , BLEED\_1 bit fields, Bits[9:0], and reference slew rate.

As shown in Equation 18 and Equation 19 for a given PFD frequency ( $f_{PFD}$ ), the output in-band phase noise increases at a 20 dB per decade rate with the N divider count. Therefore, for a given output frequency ( $f_{OUT}$ ),  $f_{PFD}$  must be as large as possible (or N must be as small as possible) while still satisfies the frequency step size requirements of the application.

Output Phase Noise Due to 1/f Noise

In-band phase noise at very low offset frequencies may be influenced by the 1/f noise of the ADF4378, which depends on  $f_{PFD}$ .

APPLICATIONS INFORMATION

Use the normalized in-band 1/f noise ( $L_{1/f}$ ) of  $-287$  dBc/Hz with Equation 20 to approximate the output 1/f phase noise at a given frequency offset ( $f_{OFFSET}$ ).

$$L_{OUT(1/f)} = L_{1/f} + 20 \times \log_{10}(f_{OUT}) - 10 \times \log_{10}(f_{OFFSET}) \quad (20)$$

Often  $L_{1/f}$  is normalized to a 1 GHz signal at a 10 kHz offset, as shown in Equation 21.

$$L_{1/f_{1G_{10k}}} = L_{1/f} + 20 \times \log_{10}(1\text{ GHz}) - 10 \times \log_{10}(10\text{ kHz}) = L_{1/f} + 140\text{ dB} \quad (21)$$

Unlike the in-band noise floor ( $L_{OUT}$ ), the 1/f noise ( $L_{OUT(1/f)}$ ) does not change with  $f_{PFD}$  and is not constant over offset frequency. For an example of in-band phase noise for  $f_{PFD}$  equal to 100 MHz and 500 MHz, see Figure 97. The total phase noise is the summation of  $L_{OUT}$  and  $L_{OUT(1/f)}$ , calculated by Equation 22.

$$L_{OUT(TOTAL)}(f_{OFFSET}) = 10 \times \log_{10} \left( 10^{L_{OUT}/10} + 10^{L_{OUT(1/f)}(f_{OFFSET})/10} \right) \quad (22)$$

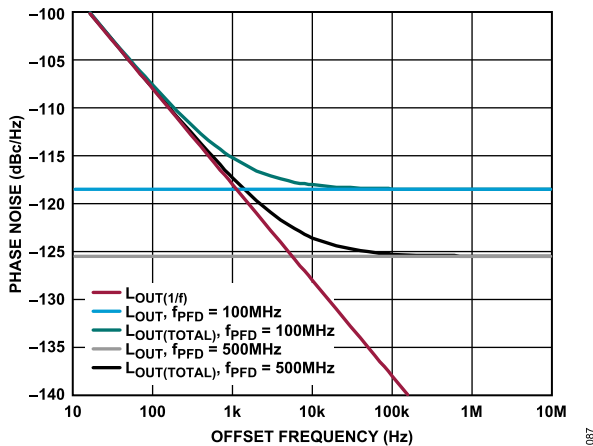


Figure 97. Theoretical In-Band Phase Noise,  $f_{OUT} = 10\text{ GHz}$

POWER-UP AND INITIALIZATION SEQUENCE

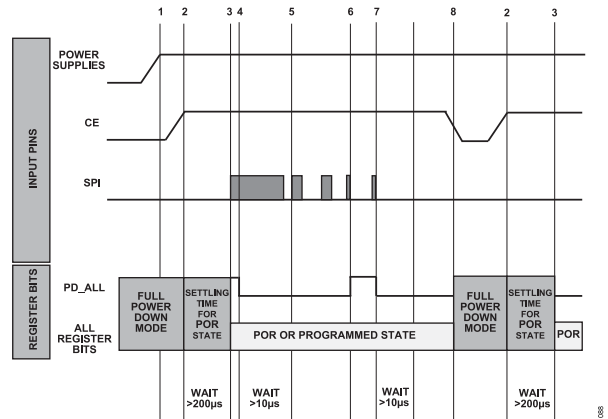


Figure 98. Power-Up and Initialization Sequence

The following steps describe the recommended power-up and initialization sequence of the ADF4378:

1. Apply specified voltages to the  $V_{5V}$ ,  $V_{3.3V_1}$ , and  $V_{3.3V_2}$  power supply groups. The ADF4378 is in full power-down mode at this point and SPI programming is not possible.
2. Set the CE pin to a logic high. It is acceptable to connect the CE pin to the  $V3\_LDO$  pin by a pull-up resistor, therefore performing Step 1 and Step 2 coincidentally.
3. After waiting  $\geq 200\ \mu\text{s}$  for all SPI register bits to settle to their power-on reset state (POR), begin programming the SPI to configure the ADF4378 to a required state. The following is the recommended SPI programming:
  - a. Set the  $SDO\_ACTIVE$  and  $CMOS\_OV$  bits to a required state for future readback operations.
  - b. Program all register addresses in descending order, REG0045 to REG0010. There are several required reserved register field settings provided in Table 44 that are required for proper device operation.
4. The ADF4378 remains in power-down mode until the PD\_ALL bit is programmed to 0. After PD\_ALL is disabled, wait at least  $10\ \mu\text{s}$  for the VCO calibration circuitry and other circuit blocks to settle before starting a VCO calibration.
5. A write to REG0010 starts a VCO autocalibration. At this point, the device is fully operational and new frequencies can be programmed as often as required.
6. Setting PD\_ALL to 1 powers down the ADF4378, which retains the latest programmed SPI settings and full SPI programming capability.
7. If only the state of PD\_ALL is modified in Step 6, setting PD\_ALL to 0 returns the ADF4378 to the frequency programmed in Step 5. After a  $10\ \mu\text{s}$  wait, all circuit blocks are completely powered up internally. This  $10\ \mu\text{s}$  wait does not include the frequency settling time associated with the loop filter bandwidth.

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8. Toggling the CE pin level causes the ADF4378 to return to full power-down mode and return the SPI registers to the POR state (see Step 2 and Step 3).

### POWER SUPPLY AND BYPASSING

The ADF4378 is a high performance and low noise device. Phase noise and spurious performance may be degraded by noisy power supplies. To achieve maximum performance and ensure that power supply noise does not degrade the performance of the ADF4378, it is recommended to use the Analog Devices low noise, high power-supply rejection ratio (PSRR) regulators. Preferred regulators include the [LT3045](#), [ADM7150](#), and the [ADM7151](#).

The ADF4378 eliminates the need for on-board supply bypass capacitors, by integrating all necessary local power supply bypass capacitors on the ADF4378 package laminate. As shown in [Figure 99](#), by removing the requirement for local power supply bypass capacitors, the ADF4378 consumes 40% less effective PCB area and reduces the number of board layout design challenges.

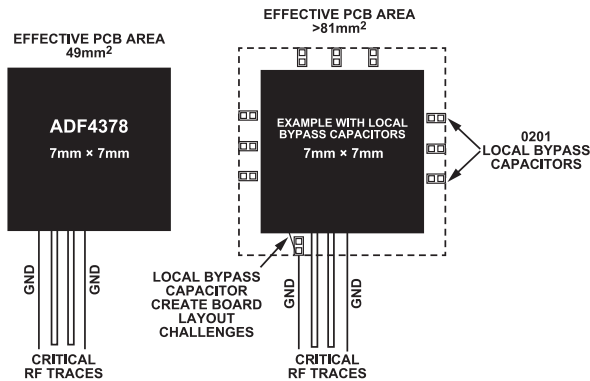


Figure 99. Layout Advantages with Integrated Power Supply Decoupling Capacitors

### DESIGN AND PROGRAMMING EXAMPLE 1: SINGLE ADF4378

A single ADF4378 clocks a single ADC. The purpose of this example is to provide a method to determine the correct inputs required to design a loop filter in [ADIsimPLL](#), provide a method to manually generate all ADF4378 register settings, and provide the method to perform a VCO autocalibration on initial power-up and bypass or override the VCO autocalibration on all future device power-ups. In practice, the ADF4378 evaluation board graphical user interface (GUI) register automates the register generation process and can replace and/or verify the manual register generation method.

For this design example, assume the following design goals:

- ▶ Reference input, 125 MHz, single-ended 7 dBm sine wave, 50 Ω environment
- ▶ Output of 12 GHz
- ▶ SPI requirements of 1.8 V, 4-wire SPI, optimize SPI write sequence

- ▶ Prioritize designing for the lowest jitter performance over other design criteria

### Design Procedure

The following design procedure aids in schematic design and SPI register generation:

1. Select the settings for reference and loop filter design (for more information, see the [Reference and Loop Filter Design](#) section).
2. Select the output, frequency, and amplitude (for more information, see the [Output Selection, Frequency and Amplitude](#) section).
3. Select the settings for the reference to output propagation delay (for more information, see the [Reference to Output Propagation Delay Settings](#) section).
4. Select the lock detector settings (for more information, see the [Lock Detector Settings](#) section).
5. Select the VCO automatic calibration settings (for more information, see the [VCO Automatic Calibration Settings](#) section).
6. Select the double buffer and manual VCO calibration settings (for more information, see the [Double Buffer and Manual VCO Calibration Settings](#) section).
7. Select the SPI protocol settings (for more information, see the [SPI Protocol Settings](#) section).
8. Select the remaining register settings (for more information, see the [Remaining Register Settings](#) section).

### Reference and Loop Filter Design

To design a loop filter in [ADIsimPLL](#), the user must determine the required reference input settings, charge pump settings, and PFD frequency. The design goals provided in the [Design and Programming Example 1: Single ADF4378](#) section state to prioritize the lowest jitter performance over other design criteria. To design the lowest jitter loop filter, determine the register settings that minimize the output phase noise characteristics as described in the [Output Phase Noise Characteristics](#) section.

The [In-Band Output Phase Noise](#) section states the maximum  $f_{PFD}$  minimizes  $L_{OUT}$ . The maximum  $f_{PFD}$  is obtained with the reference doubler enabled and the reference divider bypassed (for more information, see the [Reference Divider \(R\) and Doubler \(D\)](#) section). To enable the reference doubler, set  $EN\_RDBLR = 1$ . The reference divider is bypassed and can remain at its power on reset state ( $R\_DIV = 1$ ). Solve [Equation 7](#) for the maximum  $f_{PFD}$ .

$$f_{PFD} = D \times f_{REF} = 2 \times 125 \text{ MHz} = 250 \text{ MHz}$$

The [Charge Pump](#) section states that larger  $I_{CP}$  results in lower  $L_{NORM}$ , as shown in [Figure 46](#). Set  $CP\_I = 15$  to minimize  $L_{NORM}$ .

Selecting the optimal reference input buffer amplifier (for more information, see the [Reference Input Buffer](#) section) based on the reference input slew rate also minimizes  $L_{NORM}$  (see [Figure 43](#)). Solve [Equation 23](#) and [Equation 8](#) for the reference input slew rate.

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$$V_{PK} = \sqrt{2} \times \sqrt{10^{((P_{dBm}/10) \times 50 \Omega / 1000 mW)}} \quad (23)$$

$$V_{PK} = \sqrt{2} \times \sqrt{10^{((7 dBm/10) \times 50 \Omega / 1000 mW)}} = 0.707 V_{PK}$$

$$\text{Slew Rate} = 2 \times \pi \times f_{REF} \times V_{PK} = 2 \times \pi \times 125 \text{ MHz} \times 0.707 = 556 V/\mu s$$

Based on [Table 7](#) and [Figure 43](#), a reference input slew rate of 556 V/ $\mu$ s minimizes  $L_{NORM}$  when the LNA reference amplifier is selected by setting REF\_SEL = 1. When the LNA reference amplifier is selected, [Table 8](#) requires FILTER\_REF = 0 when  $f_{REF} = 125$  MHz, and [Table 9](#) requires BST\_REF = 1 when  $V_{REF} = 2 \times 0.707 V_{PK} = 1.414 V_{p-p}$ .

The reference peak detector (for more information, see the [Reference Peak Detector](#) section) consumes minimal power, ~10 mW, and does not degrade performance. As a result, PD\_RDDET can be set to 0 or 1 to meet the design goals. The reference and loop filter design is created with PD\_RDDET = 0 to allow for the option to monitor the reference signal with the REF\_OK bit.

**Table 25. SPI Summary, Reference and Loop Filter Design**

Bit Field	Value
EN_RDBLR	0x1
R_DIV	0x1
CP_I	0xF
REF_SEL	0x1
FILTER_REF	0x0
BST_REF	0x1
PD_RDDET	0x0

For the recommended reference input network, see [Figure 86](#), single-ended 50  $\Omega$  source ( $V_{REFIN} < 2.6 V_{p-p}$ ).

For [ADIsimPLL](#) loop filter design, note that the selected LNA reference amplifier has a higher gain than the DMA reference amplifier. As a result, the LNA generates larger reference spurious content, which requires a 5<sup>th</sup> order loop filter design to achieve the stated typical spurious performance of -100 dBc. However, the DMA has less reference spurious content and can use a simpler 4<sup>th</sup> order loop filter design for the same spurious result. For the purposes of the reference and loop filter design, assume [ADIsimPLL](#) created a loop filter with a 460 kHz loop bandwidth. The loop filter bandwidth is required later in this design to determine the LD\_COUNT setting.

### Output Selection, Frequency and Amplitude

The [Design and Programming Example 1: Single ADF4378](#) section design goals require  $f_{OUT} = 12$  GHz. [Table 18](#) sets CLKOUT\_DIV = 0 and O = 1 when  $f_{OUT} = 12$  GHz. The PLL feedback divider bit fields, N\_INT, Bits[11:0], can be determined from [Equation 4](#), [Equation 6](#), and [Table 20](#).

$$f_{OUT} = f_{VCO} / O = f_{VCO}$$

$$f_{VCO} = f_{REF} \times D \times N \times O, \text{ solving for } N \text{ produces}$$

$$N = f_{VCO} / (f_{REF} \times D \times O) = 12 \text{ GHz} / (125 \text{ MHz} \times 2 \times 1) = 48, N\_INT \text{ setting}$$

The clock output buffer amplitude (for more information, see the [Clock Output Buffer](#) section) does not have a noticeable effect on jitter performance, see [Figure 9](#). However, [Figure 52](#) indicates that lower amplitudes decrease the supply current. Therefore, choose the lowest amplitude setting the ADC clock input accepts. For the frequency and amplitude output selection, choose the clock output buffer amplitude by setting CLKOUT\_OP = 1 (see [Figure 32](#) and [Table 21](#)).

Common ADF4378 clock output networks are shown in [Figure 109](#).

**Table 26. SPI Summary, Output Selection, Frequency and Amplitude**

Bit Field	Value
CLKOUT_DIV	0x0
N_INT, Bits[11:0]	0x30
CLKOUT_OP	0x1
PD_CLKOUT	0x0

### Reference to Output Propagation Delay Settings

Reference to output propagation delay is not shown in the [Design and Programming Example 1: Single ADF4378](#) section. In the [Design and Programming Example 1: Single ADF4378](#) section, it is stated to prioritize to the lowest jitter performance. Setting the reference to output delay controls to their minimum setting achieves the lowest jitter by minimizing  $L_{NORM}$  and  $L_{1f}$  (see [Figure 12](#), [Figure 15](#), [Figure 42](#), and [Figure 45](#)). As shown in [Figure 14](#), the INV\_CLKOUT setting does not affect jitter performance and can remain at its power on reset state of 0.

**Table 27. SPI Summary, Propagation Delay**

Bit Field	Value
EN_BLEED	0x0
BLEED_I	0x0
BLEED_POL	0x0
R_DEL	0x0
N_DEL	0x0
INV_CLKOUT	0x0

### Lock Detector Settings

To enable the lock detector (for more information, see the [Lock Detector](#) section), set the EN\_LOL and EN\_LDWIN bits to 1. The LD\_COUNT bit field is determined by [Equation 12](#). As shown in the [Reference and Loop Filter Design](#) section, a 460 kHz loop bandwidth (LPBW) is assumed.

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$$\text{PFD Cycles} = f_{\text{PFD}} \times 5 / (2 \times \pi \times \text{LPBW}) = 250 \text{ MHz} \times 5 / (2 \times \pi \times 460 \text{ kHz}) = 432$$

The calculated minimum PFD cycle count of 432 is then compared to the PFD cycle column in [Table 14](#), which results in 542 PFD cycles and LD\_COUNT = 9.

To determine the LDWIN\_PW setting from [Table 16](#), calculate  $t_{\text{DEL}}$  from [Equation 10](#) or [Equation 11](#). Because the BLEED\_I bit fields, Bits[9:0], is set to 0 in the [Reference to Output Propagation Delay Settings](#) section,  $t_{\text{DEL}} = 0$ . Based on [Table 16](#), when  $t_{\text{DEL}} = 0$ , LDWIN\_PW is set to 0. The RST\_LD bit is related to the lock detector and is set to 0 in normal use cases.

**Table 28. SPI Summary, Lock Detector**

Bit Field	Value
EN_LOL	0x1
EN_LDWIN	0x1
LD_COUNT	0x9
LDWIN_PW	0x0
RST_LD	0x0

### VCO Automatic Calibration Settings

The procedure to determine the SPI registers for an automatic VCO calibration is outlined in the [VCO Calibration](#) section.

The VCO calibration Step 1 enables the automatic calibration bit, EN\_AUTOCAL, along with enabling several VCO calibration dividers, clocks, and the temperature sensor.

**Table 29. SPI Summary, VCO Automatic Calibration, Step 1**

Bit Field	Value
EN_DNCLK	0x1
EN_DRCLK	0x1
ADC_CLK_SEL	0x0
ADC_A_CONV	0x1
EN_AUTOCAL	0x1
EN_ADC_CNV	0x1
EN_ADC	0x1
EN_ADC_CLK	0x1
PD_ADC	0x0

In VCO calibration Step 2, [Table 17](#) determines the state of CAL\_CT\_SEL, DCLK\_DIV2, and DCLK\_MODE based off the 250 MHz PFD frequency. DCLK\_DIV1 must always be set to 1 regardless of PFD frequency. [Table 17](#) provides an equation to calculate  $f_{\text{DIV\_RCLK}}$ :

$$f_{\text{DIV\_RCLK}} = f_{\text{PFD}} / 2 = 250 \text{ MHz} / 2 = 125 \text{ MHz}$$

**Table 30. SPI Summary, VCO Automatic Calibration, Step 2**

Bit Field	Value
CAL_CT_SEL	0x1

**Table 30. SPI Summary, VCO Automatic Calibration, Step 2 (Continued)**

Bit Field	Value
DCLK_DIV2	0x0
DCLK_MODE	0x1
DCLK_DIV1	0x1

In the VCO calibration Step 3 and Step 4, [Equation 13](#), [Equation 14](#), [Equation 15](#), and [Equation 16](#) are provided to calculate the SYNTH\_LOCK\_TIMEOUT bit fields, Bits[14:0], VCO\_ALC\_TIMEOUT bit fields, Bits[14:0], VCO\_BAND\_DIV bits, and ADC\_CLK\_DIV bits from  $f_{\text{DIV\_RCLK}}$ .

$$\text{SYNTH\_LOCK\_TIMEOUT} \geq \text{Ceiling} (200 \mu\text{s} \times 125 \text{ MHz}) = 25000$$

$$\text{VCO\_ALC\_TIMEOUT} \geq \text{Ceiling} (50 \mu\text{s} \times 125 \text{ MHz}) = 6250$$

$$\text{VCO\_BAND\_DIV} \geq \text{Ceiling} \left( \frac{15 \mu\text{s} \times 125 \text{ MHz}}{16 \times 2^1} \right) = \text{Ceiling} (58.59375) = 59$$

$$\text{ADC\_CLK\_DIV} > \text{Ceiling} \left( \frac{125 \text{ MHz}}{400 \text{ kHz}} - 2 \right) = \text{Ceiling} (77.625) = 78$$

**Table 31. SPI Summary, VCO Automatic Calibration, Step 3 and Step 4**

Bit Field	Value
SYNTH_LOCK_TIMEOUT	0x61A8
VCO_ALC_TIMEOUT	0x186A
VCO_BAND_DIV	0x3B
ADC_CLK_DIV	0x4E

### SYSREF Input Settings

To use SYSREF retimer path, R\_DIV value must be equal to 1. EN\_RDBLR may be enabled. Maximum input reference frequency is 500 MHz while EN\_RDBLR bit is 0. If EN\_RDBLR bit is set to 1, maximum reference frequency is limited to 250 MHz.

The SYSREF input buffer type can be selected by SR\_SEL bit in REG0042. SR\_SEL = 0, which sets the ADF4378 SYSREF input buffer for CML/LVPECL operation. Internal common mode voltage is set to 1.85 V. SR\_SEL = 1, which sets the input buffer for a generic LVDS input. Internal common mode voltage is set to 1.3 V.

**Table 32. SPI Summary, SYSREF Input Settings**

Bit Field	Value
R_DIV	0x01
EN_RDBLR	0x01 for input reference frequency <250 or 0x00
SR_SEL	0x00 for CML/LVPECL operation, 0x01 for LVDS operation



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### SYSREF Output Settings

The retimed SYSREF output is available as LVDS compatible signal on the SR\_OUTP and SR\_OUTN pins. SYSREF output can be powered down by either setting the ENSR pin LOW or programming PD\_SYSOUT bit in Register 0x001A to 1.

A 7-bit delay, SR\_DEL, may be used to increase time delay between rising edge of CLK and SYSREF signal. SR\_DEL[6:0] in REG0043 is used to set the delay. With INV\_SR in REG0043 = 0, the SYSREF aligns with a clock rising edge. The retiming edge may be inverted, which also has the effect of adding an additional  $0.5 \times t_{CLK}$  of delay. To enable this, set INV\_SR in REG0043 = 1.

**Table 33. SPI Summary, SYSREF OUTPUT Settings**

Bit Field	Value
PD_SYSOUT	0x00
SR_DEL[0:6]	0x00 to 0x7F
INV_SR	0x00 (default), 0x01 for additional $0.5 \times t_{CLK}$ delay

### Double Buffer and Manual VCO Calibration Settings

If multiple frequency settings are required, double buffering (for more information, see the [Double Buffering](#) section) and manual programming of the VCO settings can improve frequency switching times. In a single fixed frequency application, such as this design procedure, these modes are rarely required. Therefore, related bits can remain in their power-up default state.

**Table 34. SPI Summary, Double Buffer and Manual VCO Calibration Settings**

Bit Field	Value
M_VCO_CORE	0x0
M_VCO_BAND	0x0
M_VCO_BIAS	0x0
O_VCO_CORE	0x0
O_VCO_BAND	0x0
O_VCO_BIAS	0x0
CLKO_DIV_DB	0x0
DCLK_DIV_DB	0x0
O_VCO_DB	0x0
DEL_CTRL_DB	0x0

### SPI Protocol Settings

The design goals stated for the SPI protocol (for more information, see the [Serial Port](#) section) are 1.8 V logic, 4-wire SPI, and optimize SPI write sequence. REG0000, REG0001, and REG0018 have the SPI related register bits, which are shown in [Table 35](#) with the required state based on the design goals. The power-on default state is assumed if the bit function is not listed as a design goal.

**Table 35. SPI Summary - SPI Protocol**

Bit Field	Value
CMOS_OV	0x0
SDO_ACTIVE, SDO_ACTIVE_R	0x1
ADDRESS_ASCENSION, ADDRESS_ASCENSION_R	0x0
SINGLE_INSTRUCTION	0x0
LSB_FIRST, LSB_FIRST_R	0x0
MASTER_READBACK_CONTROL	0x0

### Remaining Register Settings

The [Charge-Pump Test Mode](#), [MUXOUT](#), and [Block Power-Down Control](#) sections list several bit fields that are recommended for special purposes, such as debug or ambient die temperature measurements. For this normal use case, these bit fields must be set to their POR state (see [Table 36](#)). SOFT\_RESET, SOFT\_RESET\_R, RST\_SYS, and ADC\_ST\_CNV are the only remaining RW bit fields not shown yet, and must also be set to their POR state (see [Table 36](#)).

The bit columns in [Table 44](#) have several cells without a name. These unnamed, reserved cells must be programmed to the state provided in [Table 44](#) for proper operation.

**Table 36. SPI Summary, Remaining Registers**

Bit Field	Value
EN_CPTTEST	0x0
CP_UP	0x0
CP_DOWN	0x0
MUXOUT	0x0
PD_CLK	0x0
PD_CALDAC	0x0
PD_ALL	0x0
PD_RDIV	0x0
PD_NDIV	0x0
PD_VCO	0x0
PD_LD	0x0
PD_PFDPCP	0x0
SOFT_RESET, SOFT_RESET_R	0x0
RESET_SYS	0x0
ADC_ST_CNV	0x0

### Programming Procedure

There are two different methods to power up the ADF4378. The most commonly used method provided in the [Standard Power-Up and Initialization Sequence, Automatic VCO Calibration](#) section is mandatory on the initial device power-up.

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The method provided in the [Fast Power-Up and Initialization, Manually Programmed VCO Calibration Settings \(Optional\)](#) section is an optional power-up procedure after the initial power-up.

### Standard Power-Up and Initialization Sequence, Automatic VCO Calibration

The following standard power-up and initialization sequence is the recommended procedure to power up and program the ADF4378:

1. Follow Step 1 through Step 5 in the [Power-Up and Initialization Sequence](#) section, using the register settings provided in the [Design Procedure](#) section.
2. It is optional to monitor the status of the VCO calibration bit fields, ADC\_BUSY, and FSM\_BUSY. A VCO calibration is completed when ADC\_BUSY transitions from high to low, followed by FSM\_BUSY transitioning from high to low. Typical automatic VCO calibration times range from 3 ms to 9 ms.
3. After the VCO calibration completes, disable the VCO calibration clocks by setting EN\_DRCLK = EN\_DNCLK = EN\_ADC\_CLK = 0. Disabling the VCO calibration clocks reduces the  $V_{3.3V_1}$  current by roughly 15 mA and reduces unwanted spurious content.
4. PLL is locked when the lock detector sets the LKDET pin and the LOCKED bit high.

### Fast Power-Up and Initialization, Manually Programmed VCO Calibration Settings (Optional)

The purpose of the fast power-up and initialization method is to avoid the automatic VCO calibration time, which is typically 3 ms to 9 ms. For fixed clock frequency converter applications, such as this design and programming Example 1, automatic VCO calibration times are typically acceptable. The following list provides the steps to record the VCO calibration results on the initial power-up and manually program VCO Calibration settings on subsequent power ups:

- ▶ On initial power, follow the procedure shown in the [Standard Power-Up and Initialization Sequence, Automatic VCO Calibration](#) section.
- ▶ Record calibration results from the VCO\_CORE, VCO\_BAND, and VCO\_BIAS bit fields and store the recorded results in memory. Note that each unique device and frequency combination generates different VCO\_CORE, VCO\_BAND, and VCO\_BIAS values.
- ▶ Subsequent power-up and initialization sequences (for more information, see the [Power-Up and Initialization Sequence](#) section) can bypass the automatic VCO calibration procedure by programming the override (O\_VCO\_CORE, O\_VCO\_BAND, and O\_VCO\_BIAS) and manual (M\_VCO\_CORE, M\_VCO\_BAND, and M\_VCO\_BIAS) VCO register bits with the register settings provided in [Table 37](#). All other bit fields from the [Design Procedure](#) section remain the same.

**Table 37. Manually Programmed VCO Calibration Settings**

Bit Fields	Value
EN_AUTOCAL	0x0
EN_DRCLK	0x0
EN_DNCLK	0x0
EN_ADC_CLK	0x0
O_VCO_CORE	0x1
O_VCO_BAND	0x1
O_VCO_BIAS	0x1
M_VCO_CORE	Program M_VCO_CORE, M_VCO_BAND, and M_VCO_BIAS with recorded VCO_CORE, VCO_BAND, and VCO_BIAS values, respectively, from the <a href="#">Standard Power-Up and Initialization Sequence, Automatic VCO Calibration</a> section
M_VCO_BAND	
M_VCO_BIAS	

## ALIGNING MULTIPLE ADF4378 OUTPUT PHASES

Aligning multiple ADF4378 output phases break into two steps. The first step ensures that the reference dividers, reference doubler, and clock output divider of the multiple devices are setup correctly to ensure phase alignment. The second step minimizes output-to-output skew between multiple ADF4378 devices.

### Step 1: Phase Alignment

The ADF4378 architecture includes the clock output divider and the output invert inside the integer PLL feedback loop (see [Functional Block Diagram](#)), which allows the locked PLL to align the clock output divider phase to the reference input phase. Therefore, to align multiple ADF4378 output phases, ensure that the reference phases are aligned at all the reference input pins of the ADF4378.

Because the reference divider and reference doubler are outside of the PLL loop, see [Table 38](#) to ensure that phase alignment between multiple ADF4378 devices is guaranteed.

**Table 38. Reference Settings to Align Multiple ADF4378 Devices**

Reference Divider and Doubler State	Guaranteed Reference to Output Phase Alignment
EN_RDBLR = 1	Yes
R_DIV = 1	Yes
R_DIV > 1	When $f_{OUT}/f_{REF}$ = integer, and $f_{REF} \leq f_{OUT}$

### Step 2: Output-to-Output Skew Adjustment

Any variation in reference input to output propagation delay ( $t_{PD}$ ) between multiple ADF4378 devices presents itself as output skew between multiple ADF4378 devices.

To minimize  $t_{PD}$  across process and temperature, select the DMA of the reference input buffer by setting REF\_SEL = 0. When the DMA is selected, the typical  $t_{PD}$  standard deviation due to process variation is 3 ps with a temperature coefficient ( $t_{PD-TC}$ ) of 0.03 ps/°C, as shown in [Figure 26](#) and [Figure 22](#), respectively.

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Due to the controlled  $t_{PD}$  of the ADF4378 devices, it is reasonable to expect that a significant portion of the total system skew ( $t_{SKEW\_SYSTEM}$ ) is due to propagation delay mismatches in traces or cables ( $t_{SKEW\_B}$ ,  $t_{SKEW\_D}$ ), and skew in other components ( $t_{SKEW\_A}$ ) or instruments ( $t_{MEAS\_ERROR}$ ). Figure 100 and Equation 24 provide several sources of possible output skew error in a typical system. The [Clock Skew in Large Multi-GHz Clock Trees](#) article outlines the skew trade-offs in component selection, board design, and end-user cost requirements in large clock trees.

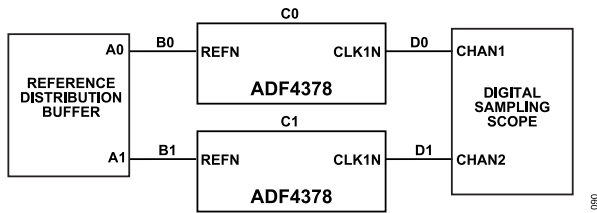


Figure 100. Total System Skew

$$t_{SKEW\_SYSTEM} = t_{SKEW\_A} + t_{SKEW\_B} + t_{SKEW\_C} + t_{SKEW\_D} + t_{MEAS\_ERROR} \quad (24)$$

where:

$$t_{SKEW\_A} = t_{A1} - t_{A0}$$

$$t_{SKEW\_B} = t_{PD\_B1} - t_{PD\_B0}$$

$$t_{SKEW\_C} = t_{PD\_C1} - t_{PD\_C0}$$

$$t_{SKEW\_D} = t_{PD\_D1} - t_{PD\_D0}$$

$$t_{MEAS\_ERROR} = t_{CHAN1} - t_{CHAN2}$$

To further minimize clock skew between multiple clocks, the ADF4378 devices provide SPI programmable adjustments to increase or decrease the  $t_{PD}$  in sub-ps steps. Table 39 and Table 40 provide a comparison of the multiple reference to output delay controls. In large clock trees, these  $t_{PD}$  adjustments can alleviate output-to-output skew trade-offs in component selection, board design, and end-user cost requirements.

Table 39. ADF4378 Reference to Output Delay Control Comparison

Parameters	Reference Delay	Feedback Delay	Charge-Pump Bleed Current	Output Invert
Register Bits	R_DEL	N_DEL	EN_BLEED, BLEED_I bit fields, Bits[9:0], BLEED_POL	INV_CLKOUT
$t_{PD}$	Increases	Decreases	BLEED_POL = 0, increases BLEED_POL = 1, decreases	Inverts output, see Table 19
Number of Steps	127	127	1023	1023
Step Size	~1 ps	~1 ps	~0.01 ps to 65 ps, varies with CP_I and $f_{PFD}$ Equation 9	$1/(2 \times f_{OUT})$

Table 40. ADF4378 Reference to Output Typical Performance Impact

Parameters	Reference and Feedback Delay	Charge-Pump Bleed Current	Output Invert
Temperature Coefficient	Minimal, Figure 18 and Figure 23	None, Figure 21 and Figure 24	None
$L_{NORM}$	<1 dB, Figure 45	<1 dB, Figure 42	None
$L_{1/f}$	<1 dB, Figure 45	<4 dB, Figure 42	None
Spurious	Minimal	$f_{PFD} \geq 50$ MHz: minimal, $f_{PFD} < 50$ MHz, contact ADI	Minimal
Lock Detector	None	For more information, see the Lock Detector section	None

Figure 45 and Figure 43 show a general trend that an increasing magnitude of R\_DEL, N\_DEL, or BLEED\_I bit fields, Bits[9:0] causes a small increase in  $L_{NORM}$  and  $L_{1/f}$ . Increases in  $L_{NORM}$  and  $L_{1/f}$  result in clock jitter (see Figure 12 and Figure 15). Therefore, in the most performance sensitive applications, identifying ways to minimize the magnitude of the R\_DEL, N\_DEL, or BLEED\_I bit fields, Bits[9:0] values is required. As an example, Figure 101 provides two skew adjustment methods to minimize the skew in Figure 100. Method 1 only adjusts one of the reference to output delay adjustments provided in Table 39. Method 1 results in an R\_DEL, N\_DEL, or BLEED\_I bit fields, Bits[9:0] maximum adjustment equal to half an output cycle, or  $1/(2 \times f_{OUT})$ . Method 2 minimizes the magnitude of R\_DEL, N\_DEL, or BLEED\_I bit fields, Bits[9:0] by utilizing the output invert along with either R\_DEL, N\_DEL, or BLEED\_I bit fields, Bits[9:0] adjustments. When compared to Method 1, Method 2 results in a lower R\_DEL, N\_DEL, or BLEED\_I bit fields, Bits[9:0] maximum adjustment of a quarter cycle output cycle, or  $1/(4 \times f_{OUT})$ . Method 2 is further described in Table 41.

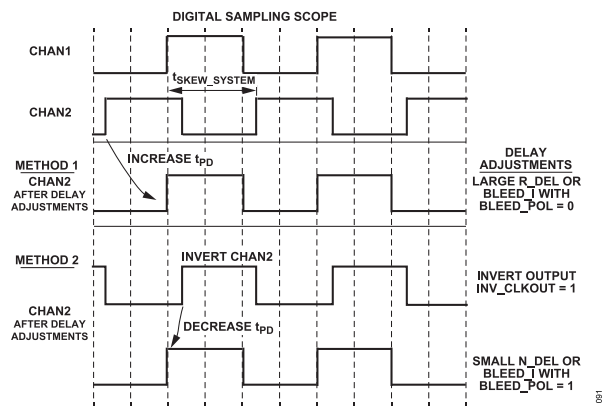


Figure 101. Skew Adjustment Methods

APPLICATIONS INFORMATION

Table 41. Method 2: Skew Adjustment

$t_{SKEW\_SYSTEM}$	Procedure
$0 < t_{SKEW\_SYSTEM} \leq \frac{1}{4} \times f_{OUT}$	INV_CLKOUT = 0 and decrease $t_{PD}$
$\frac{1}{4} \times f_{OUT} < t_{SKEW\_SYSTEM} \leq \frac{2}{4} \times f_{OUT}$	INV_CLKOUT = 1 and increase $t_{PD}$
$\frac{2}{4} \times f_{OUT} < t_{SKEW\_SYSTEM} \leq \frac{3}{4} \times f_{OUT}$	INV_CLKOUT = 1 and decrease $t_{PD}$
$\frac{3}{4} \times f_{OUT} < t_{SKEW\_SYSTEM} \leq \frac{1}{f_{OUT}}$	INV_CLKOUT = 0 and increase $t_{PD}$

DESIGN EXAMPLE 2: JESD204B/C MULTICHIP CLOCK AND SYSREF ALIGNMENT

This design Example 2 focuses on the system level approach of ADI to minimize clock skew between converters. For detailed ADF4378 loop filter and register map design, follow the procedure outlined in the [Design and Programming Example 1: Single ADF4378](#) section. Device specific programming and programming details of Converters and Stage 1 distribution IC are beyond the scope of this example.

For this design example, assume the following goals:

- ▶ Clock two converter devices with two separate ADF4378 devices.
- ▶ Minimize clock skew at time zero.
- ▶ Provide procedure to measure and reduce clock skew errors.

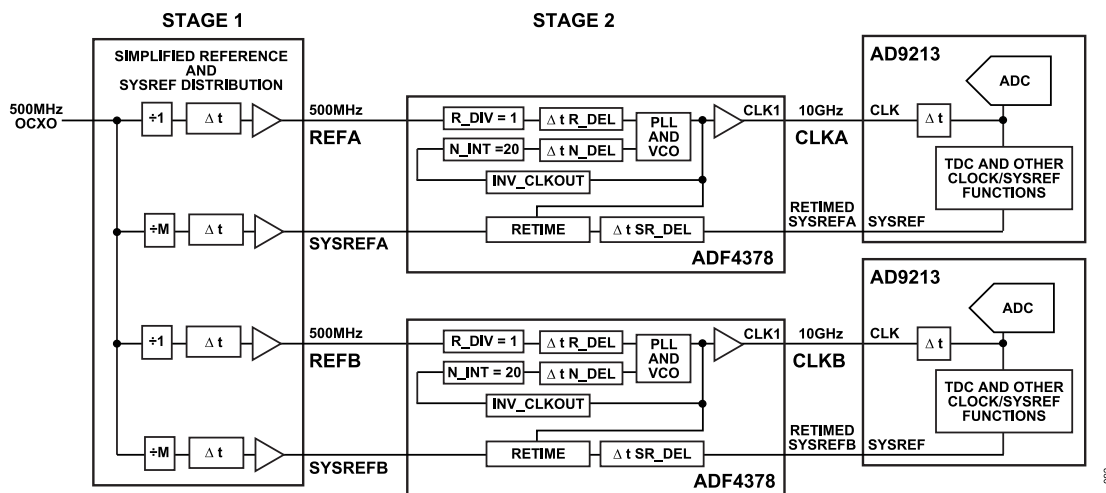


Figure 102. Design Example 2: JESD204B/C Multichip Clock and SYSREF Alignment

## APPLICATIONS INFORMATION

### Design Considerations

The [Reference and SYSREF Distribution Selection](#), [Board Layout Considerations](#), [Skew Adjustment Options](#), [Skew Adjustments and System Error](#), and [Power-Up, Programming, and Measurement Sequence](#) sections provide an overview of several design considerations when designing a low clock skew system with multiple ADF4378 devices and multiple JESD204B/C converters.

### Reference and SYSREF Distribution Selection

In high performance applications that require minimum clock skew and drift, it is recommended to choose a reference distribution device whose additive noise floor meets the requirements described in the [Reference Source Considerations](#) section, and whose output slew rate allows for the DMA option of the ADF4378 reference input buffer (see [Table 7](#)). The DMA option minimizes  $t_{PD-TC}$ , as shown in [Figure 22](#). Most reference distribution ICs output a square wave. The slew rate of a square wave is determined by [Equation 25](#).

$$\text{Slew Rate} = V_{p-p} \times \frac{(\%Upper\ t_{RISE}\ Threshold - \%Lower\ t_{RISE}\ Threshold)}{t_{RISE}} \quad (25)$$

The [HMC7043](#), [HMC7044](#), [LTC6952](#), or [LTC6953](#) are adequate reference distribution ICs for the noise floor and rise time requirements.

By using multiple outputs from a single reference and SYSREF distribution IC, the reference and SYSREF temperature delay drift match. The [LTC6952](#) and [LTC6953](#) data sheets provide output skew variation over process per output to aid in SYSREF output selection. Choosing the outputs with the least skew for SYSREF outputs improves the skew adjustment errors, as described in the [Skew Adjustments and System Error](#) section.

Selecting a JESD204B/C reference and SYSREF distribution IC requires knowledge of the JESD204B serial lane rates and the clock and SYSREF requirements of the field programmable gate array (FPGA). Both these topics are beyond the scope of this data sheet. However, ADI has created several JESD204B/C development platforms that provide hardware and software examples that can aid further in the reference and SYSREF distribution IC selection. Several of these platforms are available on the [ADI website](#).

### Board Layout Considerations

During hardware design, it is best to match the electrical lengths ( $\ell$ ) for the reference, clock, and SYSREF traces in [Figure 102](#), as shown in [Table 42](#).

**Table 42. Trace Length Matching for Skew Optimization**

If Skew Adjustments Performed	Skew Optimization	Skew Temperature Coefficient Optimization
No	$\ell_{REFA} = \ell_{REFB}$ , $\ell_{CLKA} = \ell_{CLKB}$ , $\ell_{SYSREFA} = \ell_{SYSREFB}$	$\ell_{SYSREFx} = \ell_{REFx}$ and $\ell_{RE-TIMED\_SYSREFx} = \ell_{CLKx}$

**Table 42. Trace Length Matching for Skew Optimization (Continued)**

If Skew Adjustments Performed	Skew Optimization	Skew Temperature Coefficient Optimization
	and $\ell_{RETIMED\_SYSREFA} = \ell_{RE-TIMED\_SYSREFB}$	
Yes	$\ell_{SYSREFA} = \ell_{SYSREFB}$	$\ell_{SYSREFx} = \ell_{REFx}$

For more information on PCB material selection, transmission line selection, cable selection, and several other concerns related to clock skew, refer to the [Clock Skew in Large Multi-GHz Clock Trees](#) article.

Signal attenuation is proportional to the length of the trace and signal frequency. Converter clock traces must be treated as RF traces because any unwanted spurious or noise that couples onto the clock signals can affect the performance of the converters. Therefore, it is recommended to minimize the  $\ell_{CLKA}$  and  $\ell_{CLKB}$  trace lengths to optimize performance and limit attenuation. For an additional information on clock performance concerns, routing, and recommended schematics, see the [ADC Clock and Jitter Considerations](#) section.

In most cases, trace matching board layout errors can be corrected with the  $\Delta t$  functions in the reference and SYSREF distribution IC or the ADF4378 shown in [Figure 102](#).

### Skew Adjustment Options

[Figure 102](#) has skew adjustment ( $\Delta t$ ) blocks in the Stage 1 IC and the ADF4378. In most cases, the ADF4378 is the preferred skew adjustment option in terms of maximizing performance.

The ADF4378  $\Delta t$  blocks are discussed in [Table 39](#). For this design example, SR\_DEL, R\_DEL and N\_DEL or BLEED\_I bit fields, Bits[9:0] are valid options. However, in [Figure 102](#), only SR\_DEL, R\_DEL, and N\_DEL are shown.

Like any  $\Delta t$  block, there is an opportunity for increased phase noise. The ADF4378  $\Delta t$  blocks affect phase noise at different frequency offsets, as shown in [Table 43](#).

**Table 43. Clock Phase Noise Region Affected by ADF4378  $\Delta t$  Blocks**

$\Delta t$ Block	In-Band Phase Noise	Wideband Phase Noise
	<ADF4378 Loop Filter Bandwidth	~10 MHz to $f_{CLK}$
R_DEL $\Delta t$	Minimal additive noise, see <a href="#">Table 40</a>	None
N_DEL $\Delta t$	Minimal additive noise, see <a href="#">Table 40</a>	None
SR_DEL $\Delta t$	None	None

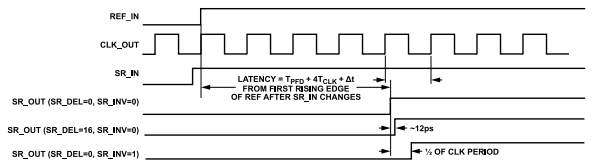
The reference and SYSREF distribution IC in [Figure 102](#) has a  $\Delta t$  block for each output. The typical Stage 1 IC skew adjustment step size is in the 11 ps ([LTC6952](#), [LTC6953](#)) to 25 ps ([HMC7043](#), [HMC7044](#)) range. These  $\Delta t$  blocks typically increase the phase

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noise floor of the output, which then impacts the in-band performance of the ADF4378. As a result, the Stage 1 reference and SYSREF distribution IC  $\Delta t$  blocks are recommended for SYSREF signals only.

### Skew Adjustments and System Error

In [Figure 102](#), SR\_DEL  $\Delta t$ , shown in ADF4378, has an ability to control the time delta between the rising edge of the SYSREF output ( $t_{\text{SYSREF}}$ ) and the rising edge of the CLK output ( $t_{\text{CLK}}$ ). Timing relationship between CLK\_OUT and SR\_OUT pins are given in [Figure 103](#).



**Figure 103. Timing Relationships of REF\_IN, CLK\_OUT, SR\_IN, and SR\_OUT**

By following design constraint that  $l_{\text{RETIMED\_SYSREF}}$  and  $l_{\text{CLK}}$  lanes are designed to have minimum mismatch, SYSREF retimer feature in ADF4378 allows SYSREF output rising edge to fall in one output CLK period and stay there over temperature. It does not have to be a specific CLK period, as long as SYSREF rising edge does not move near or past a CLK rising edge vs. temperature. Latency from first rising edge of reference signal after SYSREF IN changes to SYSREF OUT rising edge is stable over temperature and can be calculated by [Equation 26](#).

$$\text{Latency} = T_{\text{PFD}} + 4 \times T_{\text{CLK}} + \Delta t \quad (26)$$

If there is a mismatch in propagation delay between  $l_{\text{RETIMED\_SYSREF}}$  and  $l_{\text{CLK}}$ , SR\_DEL  $\Delta t$  block can delay SYSREF output up to 120 ps in  $\sim 0.8$  ps steps or half of a CLK period by setting SR\_INV = 1. SYSREF retimer feature of the ADF4378 simplifies the design of high frequency CLK path and retimed SYSREF path. Therefore, designers can focus on reference and SYSREF distribution side of the system.

Usually,  $l_{\text{SYSREF}}$  and  $l_{\text{REF}}$  are longest paths in the design. However, it is easier to design length-matched paths for reference and SYSREF distribution due to low frequency nature of those signals compared to  $l_{\text{CLK}}$ . The retimer simplifies the system design by allowing the widely distributed SYSREF to only meet the slower reference frequency timing instead of the much more stringent output clock timing. If there is mismatch between  $l_{\text{REFA}}$  and  $l_{\text{REFB}}$ , N\_DEL, and R\_DEL block on ADF4378 can modify skew between reference signals. Delay blocks on reference distribution can also be used for reference alignment between two ADF4378s, however, Delay blocks on reference distribution can increase in-band noise of the ADF4378. Delay blocks for SYSREF distribution can be used to align SYSREF signals as delay on SYSREF has no effect on in-band noise of the ADF4378.

### Power-Up, Programming, and Measurement Sequence

The following list provides the recommended system level power-up, device programming, and skew measurement sequence:

1. Power up system.
2. Program Stage 1 IC and ADF4378 devices to their expected frequency plan.
3. Allow temperature of the components to settle.
4. Perform clock skew adjustments for first ADF4378.
5. Program skew adjustments per Method 2 for other ADF4378, as shown in [Figure 101](#).
6. Perform JESD204B/C initialization.

## ADC CLOCK AND JITTER CONSIDERATIONS

### Estimating ADC SNR and Clock Jitter Requirements

Adding noise directly to a clean signal reduces its signal-to-noise ratio (SNR). In data acquisition applications, digitizing a clean signal with a noisy clock signal also degrades the SNR. This issue is best explained in the time domain by using jitter instead of phase noise. For this discussion, assume that the jitter is white (flat with frequency) and of Gaussian distribution.

[Figure 104](#) shows a sine wave signal entering a typical data acquisition circuit composed of an ADC, an input signal amplifier, and a sampling clock. [Figure 104](#) also shows the three signal sampling scenarios for sampling the sine wave at its zero crossing.

In the first scenario, a perfect sine wave input is buffered by a noiseless amplifier to drive the ADC. Sampling is performed by a perfect, zero jitter clock. Without any added noise or sampling clock jitter, the digitized output value of the ADC is very clearly determined and perfectly repeatable from cycle-to-cycle.

In the second scenario, a perfect sine wave input is buffered by a noisy amplifier to drive the ADC. Sampling is performed by a perfect, zero jitter clock. The added noise results in an uncertainty in the digitized value, which causes an error term that degrades the SNR. The degraded SNR in this scenario, from adding noise to the signal, is expected.

In the third scenario, a perfect sine wave input is buffered by a noiseless amplifier to drive the ADC. Sampling is performed by a clock signal with added jitter. Note that as the signal is slewing, the jitter of the clock signal leads to an uncertainty in the digitized value and an error term, like in the second scenario. Again, this error term degrades the SNR.

A real-world system has both additive amplifier noise and sample clock jitter. After the signal is digitized, determining the root cause of any SNR degradation, amplifier noise, or sampling clock jitter, is essentially impossible.

APPLICATIONS INFORMATION

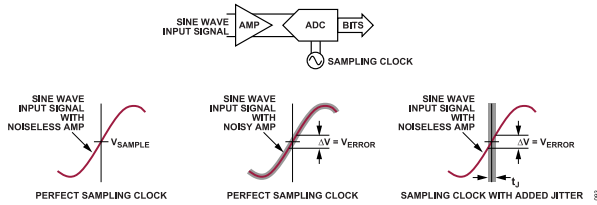


Figure 104. A Typical Data Acquisition Circuit Showing the Sampling Error Effects of a Noisy Amplifier and a Jittery Clock

Degradation of the SNR due to sample clock jitter only occurs if the analog input signal is slewing. If the analog input signal is stationary (DC), it does not matter when in time the sampling occurs. Additionally, a faster slewing input signal yields a greater error (more noise) than a slower slewing input signal.

Figure 105 demonstrates this effect. Note how much larger the error term is with the fast slewing signal than with the slow slewing signal. To maintain the SNR performance of the data converter, digitization of high input frequency signals requires a clock with much less jitter than applications with lower frequency input signals.

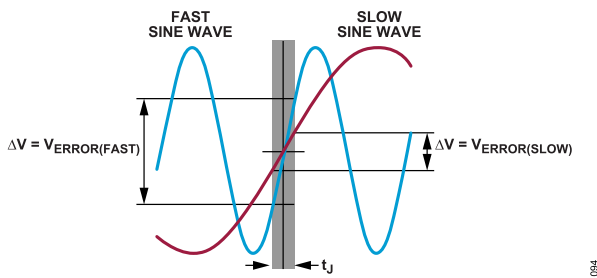


Figure 105. Fast and Slow Sine Wave Signals Sampled with a Jittery Clock

It is important to note that the frequency of the analog input signal determines the jitter requirement of the sample clock. The actual sample clock frequency does not matter. Many ADC applications that under sample high frequency signals have especially challenging sample clock jitter requirements.

This information is useful for gaining an intuitive feel for the SNR degradation due to sampling clock jitter. Quantitatively, the actual sample clock jitter requirement for a given application is calculated as follows:

$$t_{J(TOTAL)} = \frac{10^{-SNR_{dB}/20}}{2 \times \pi \times f_{SIG}} \tag{27}$$

where:

$t_{J(TOTAL)}$  is the total RMS jitter in seconds.

$SNR_{dB}$  is the SNR requirement in decibels.

$f_{SIG}$  is the highest frequency signal to be digitized, expressed in Hz.

The total jitter is the rms sum of the aperture jitter of the ADC and the sample clock jitter, calculated as follows:

$$t_{J(TOTAL)} = \sqrt{t_{J(CLK)}^2 + t_{J(ADC)}^2} \tag{28}$$

Alternatively, for a given total jitter, the attainable SNR is calculated as follows:

$$SNR_{dB} = -20 \times \log(2 \times \pi \times f_{SIG} \times t_{J(TOTAL)}) \tag{29}$$

These calculations assume a full-scale sine wave input signal. If the input signal is a complex, modulated signal with a moderate crest factor, the peak slew rate of the signal may be lower and the sample clock jitter requirement may be relaxed.

These calculations are also theoretical. They assume a noiseless ADC with infinite resolution. All realistic ADCs have both added noise and a resolution limit. The limitations of the ADC must be accounted for to prevent overspecifying the sampling clock.

Figure 106 plots the previous equations and provides a way to estimate the sampling clock jitter requirement for a given input signal or the expected SNR performance for a given sample clock jitter.

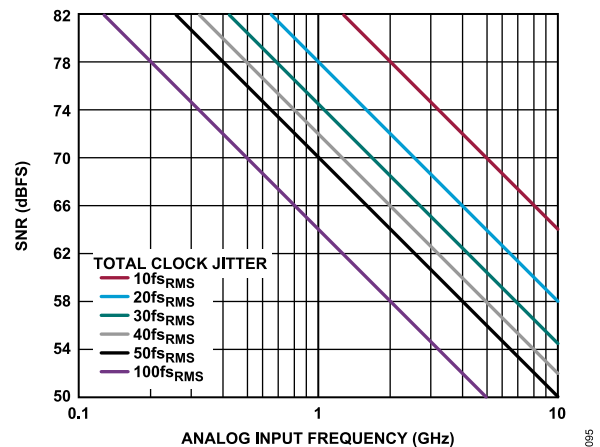


Figure 106. SNR vs. Input Signal Frequency vs. Sample Clock Jitter

Measuring Clock Jitter Indirectly Using ADC SNR

For some applications, which integrate the phase noise of a clock generator within a defined offset frequency range (for example, 12 kHz to 20 MHz) is sufficient to calculate the impact of the clock on the overall system performance. In these situations, the rms jitter can be calculated from a phase noise measurement.

However, other applications require knowledge of the phase noise of the clock at frequency offsets that exceed the capabilities of phase noise analyzers. This limitation makes it difficult to calculate jitter from a phase noise measurement.

The rms jitter of an ADC clock source can be indirectly measured by comparing a jitter dominated SNR measurement to a non-jitter dominated SNR measurement. A jitter dominated SNR measurement ( $SNR_{JITTER}$ ) is created by applying a low jitter, high frequency full-scale sine wave to the ADC analog input. A non-jitter dominated

APPLICATIONS INFORMATION

SNR measurement ( $SNR_{BASE}$ ) is created by applying a very low amplitude (or low frequency) sine wave to the ADC analog input. The total clock jitter ( $t_{J(TOTAL)}$ ) can be calculated using Equation 30.

$$t_{J(TOTAL)} = \frac{10^{1/2} \times \log_{10} \left( 10^{-SNR_{JITTER}/10} - 10^{-SNR_{BASE}/10} \right)}{2 \times \pi \times f_{SIG}} \quad (30)$$

Assuming the inherent aperture jitter of the ADC ( $t_{J(ADC)}$ ) is known, the jitter of the clock generator ( $t_{J(CLK)}$ ) is obtained using Equation 28.

ADC Sample Clock Input Drive Requirements

Modern high speed, high resolution ADCs are sensitive components able to match or exceed laboratory instrument performance in many regards. Noise or interfering signals on the analog signal input, the voltage reference, or the sampling clock input can easily appear in the digitized data. To deliver the full performance of any ADC, the sampling clock input must be driven with a clean, low jitter signal.

Figure 107 shows a simplified version of a typical ADC sample clock input. In Figure 107, the input pins may be labeled  $ENC_{\pm}$  for encode or  $CLK_{\pm}$  for clock in different ADCs. The input is composed of a differential limiting amplifier stage followed by a buffer that directly controls the track and hold stage of the ADC.

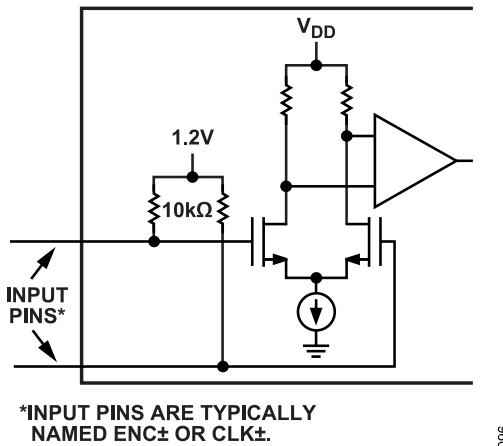


Figure 107. Simplified Sample Clock Input Circuit

The sample clock input amplifier also benefits from a fast slewing input signal because the amplifier has noise of its own. By slewing through the crossover region quickly, the amplifier noise creates less jitter than if the transition is slow. As shown in Figure 107, the sample clock input of the ADC is typically differential, with a differential sampling clock delivering the best performance. Figure 107 also shows the sample clock input with a different common-mode input voltage than the outputs of the ADF4378. Most ADC applications require AC coupling to convert between the two common-mode voltages.

Transmission Lines and Termination

Interconnection of high speed signaling with fast rise and fall times requires the use of transmission lines with properly matched termination. The transmission lines may be stripline, microstrip, or any other design topology. A detailed discussion of transmission line design is beyond the scope of this data sheet. Any mismatch between the characteristic impedance of the transmission line and the terminating impedance results in a portion of the signal reflecting back toward the other end of the transmission line. In the extreme case of an open or short-circuit termination, all of the signal is reflected back. This signal reflection leads to overshoot and ringing on the waveform. Figure 108 shows the preferred method of far-end termination of the transmission line.

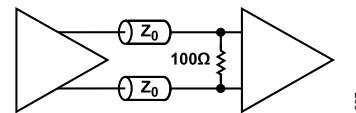


Figure 108. Far-End Transmission Line Termination ( $Z_0 = 50 \Omega$ )

ADF4378 Output Networks

The differential outputs of the ADF4378 are designed to interface with most differential signal devices while driving transmission lines with far-end termination. Figure 109, Figure 110, and Figure 111 shows AC-coupled output configurations. Note that some receiver devices have the 100 Ω termination resistor internal to the device, in which case the external 100 Ω resistor is unnecessary. The ADF4378 also interfaces with single-ended 50 Ω end terminations. In this case, the unused output requires an AC-coupled 50 Ω termination. For the single-ended example in Figure 111, the  $CLK_N$  and  $CLK_P$  pins may be swapped.

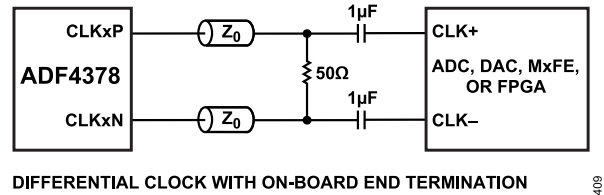


Figure 109. Common Clock Interface: Differential Clock with On-Board End Termination ( $Z_0 = 50 \Omega$ )

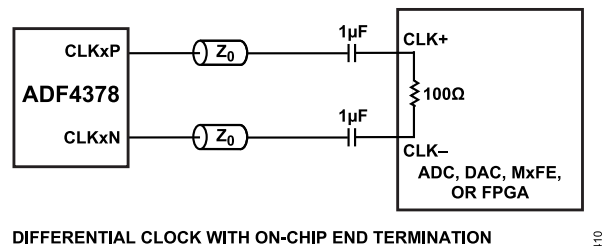
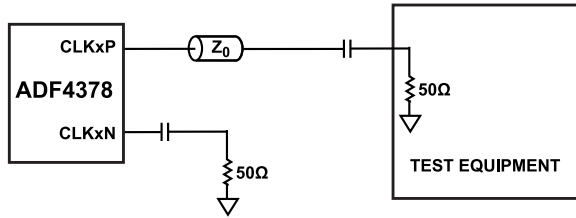


Figure 110. Common Clock Interface: Differential Clock with On-Chip End Termination ( $Z_0 = 50 \Omega$ )



APPLICATIONS INFORMATION



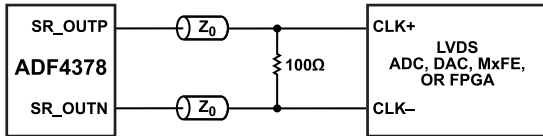
SINGLE-ENDED CLOCK WITH END TERMINATION

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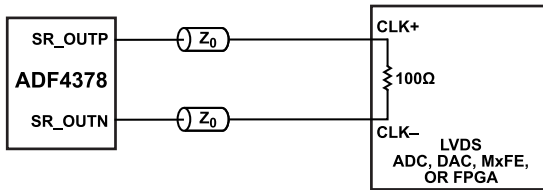
Figure 111. Common Clock Interface: Single-Ended Clock with End Termination ( $Z_0 = 50 \Omega$ )

SYSREF Output Networks

The ADF4378's differential output is designed to interface with most LVDS compatible interfaces while driving transmission lines with far-end termination. Figure 112 shows DC-coupled output configurations. Note that some receiver devices have the 100 Ω termination resistor internal to the part, in which case the external 100 Ω resistor is unnecessary.



DIFFERENTIAL SYSREF WITH ON-BOARD END TERMININATION



DIFFERENTIAL SYSREF WITH ON-CHIP END TERMININATION

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Figure 112. Common SYSREF Connections

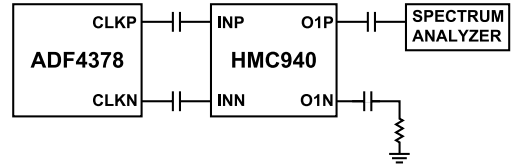
MEASURING DIFFERENTIAL SPURS WITH A SINGLE-ENDED TEST INSTRUMENT

Using a spectrum analyzer to measure spurious signals on the single-ended output of a clock generation chip gives pessimistic results, particularly for outputs that approximate square waves. There are two reasons for this.

First, because the spurious energy is often an AC signal superimposed on the power supply, a differential output rejects the spurs to within the matching of the positive and negative outputs. Observing only one side of the differential output provides no rejection.

Second, and most importantly, the spectrum analyzer displays all of the energy at its input, which includes amplitude modulation that occurs at the top and bottom pedestal voltage of the square wave. However, only amplitude modulation near a zero crossing affects the clock.

The best way to remove this measurement error is to drive the clock generator output differentially into a limiting buffer on a separate clean power supply. One of the differential outputs of the limiting buffer can then connect to a spectrum analyzer to correctly measure the spurious energy. An example of this technique using the ADF4378 as the clock generator and an HMC940 as the limiter is shown in Figure 113.



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Figure 113. Example of Spurious Measurement Techniques

APPLICATION CIRCUITS

PARALLEL ADF4378 DEVICES, 13 fs<sub>RMS</sub> JITTER

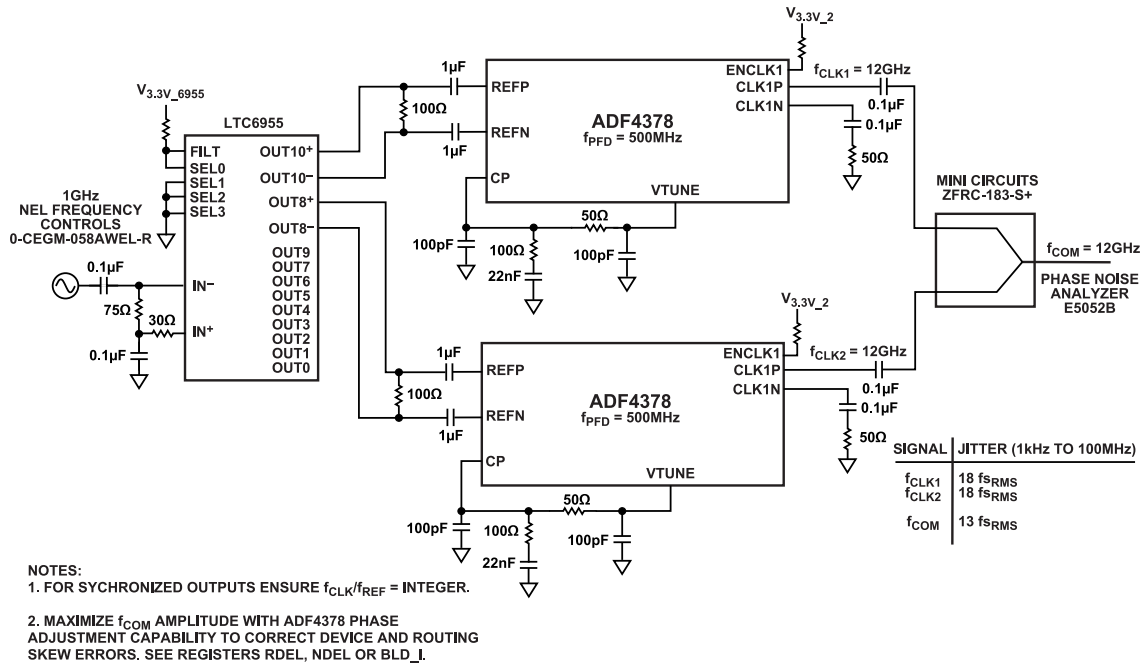


Figure 114. Block Diagram of Parallel ADF4378 Devices

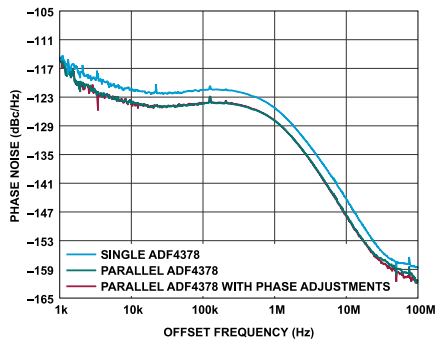


Figure 115. 12 GHz Parallel ADF4378s, 13 fs<sub>RMS</sub> Jitter

APPLICATION CIRCUITS

AD9082 ERROR VECTOR MAGNITUDE (EVM) WITH ADF4378 AS CLOCK

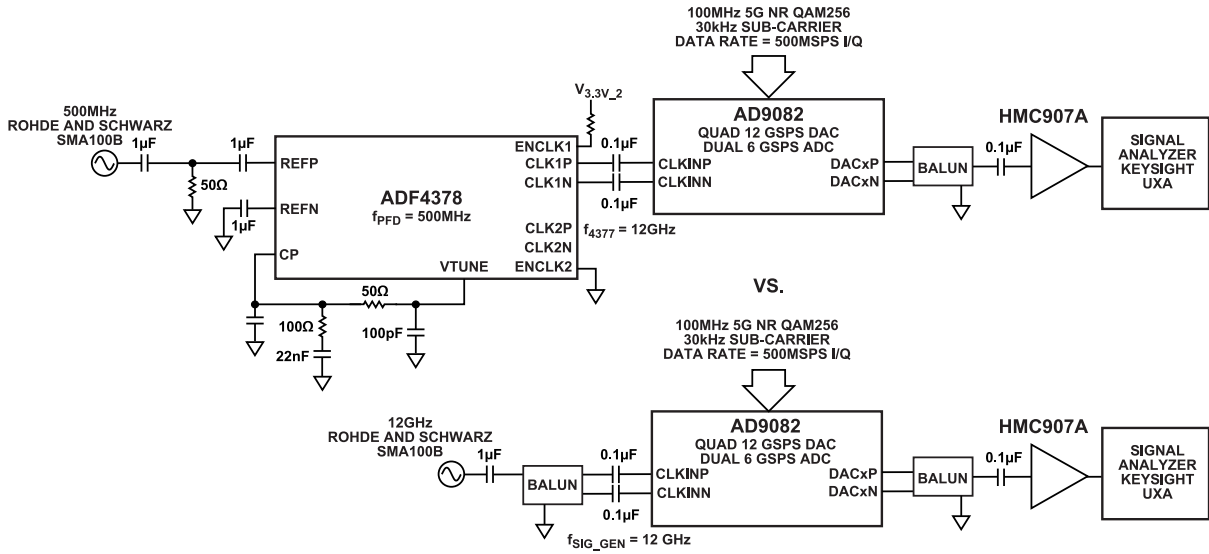


Figure 116. AD9082 and ADF4378 Measurement Schematic

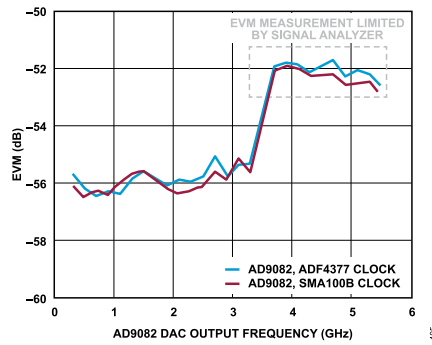


Figure 117. AD9082 EVM with ADF4378 as 12 GHz Clock

## REGISTER SUMMARY

Table 44. ADF4378 Register Summary

Reg	Name	Bits	Bit 7	Bit 6	Bit 5	Bit 4	Bit 3	Bit 2	Bit 1	Bit 0	Reset	RW	
0x00	REG0000	[7:0]	SOFT_RES ET_R	LSB_FIRST _R	ADDRESS_ ASCENSIO N_R	SDO_ACTIV E_R	SDO_ACTIV E	ADDRESS_ ASCENSIO N	LSB_FIRST	SOFT_RES ET	0x00	R/W	
0x01	REG0001	[7:0]	SINGLE_IN STRUCTIO N	R001_RSV6	MAIN_REA DBACK_CO NTROL	R001_RSV4	RESERVED	R001_RSV2	R001_RSV1	RESERVED	0x00	R/W	
0x02	REG0002	[7:0]	RESERVED				R002_RSV1				0x00	R	
0x03	REG0003	[7:0]	RESERVED				CHIP_TYPE				0x00	R	
0x04	REG0004	[7:0]	PRODUCT_ID[7:0]								0x00	R	
0x05	REG0005	[7:0]	PRODUCT_ID[15:8]								0x00	R	
0x06	REG0006	[7:0]	R006_RSV2				R006_RSV1				0x00	R	
0x0A	REG000A	[7:0]	SCRATCHPAD								0x00	R/W	
0x0B	REG000B	[7:0]	SPI_REVISION								0x00	R	
0x0C	REG000C	[7:0]	VENDOR_ID[7:0]								0x56	R	
0x0D	REG000D	[7:0]	VENDOR_ID[15:8]								0x04	R	
0x0F	REG000F	[7:0]	RESERVED							R00F_RSV1	0x00	R/W	
0x10	REG0010	[7:0]	N_INT[7:0]								0x80	R/W	
0x11	REG0011	[7:0]	EN_AUTOC AL	EN_RDBLR	DCLK_DIV2		N_INT[11:8]				0x00	R/W	
0x12	REG0012	[7:0]	CLKOUT_DIV		R_DIV						0x01	R/W	
0x13	REG0013	[7:0]	R013_RSV1		M_VCO_CORE		M_VCO_BIAS				0x00	R/W	
0x14	REG0014	[7:0]	M_VCO_BAND								0x00	R/W	
0x15	REG0015	[7:0]	BLEED_I[1:0]		BLEED_PO L	EN_BLEED	CP_I				0x00	R/W	
0x16	REG0016	[7:0]	BLEED_I[9:2]								0x00	R/W	
0x17	REG0017	[7:0]	INV_CLKOU T	N_DEL							0x00	R/W	
0x18	REG0018	[7:0]	CMOS_OV	R_DEL							0x00	R/W	
0x19	REG0019	[7:0]	R019_RSV1		CLKOUT_OP		PD_CLK	PD_RDET	PD_ADC	PD_CALDA C	0x04	R/W	
0x1A	REG001A	[7:0]	PD_ALL	PD_RDIV	PD_NDIV	PD_VCO	PD_LD	PD_PFD DCP	PD_CLKOU T1	PD_SYSSO UT	0x83	R/W	
0x1B	REG001B	[7:0]	EN_LOL	LDWIN_PW	EN_LDWIN	LD_COUNT					0x00	R/W	
0x1C	REG001C	[7:0]	EN_DNCLK	EN_DRCLK	R01C_RSV4	R01C_RSV3	R01C_RSV2	RST_LD	R01C_RSV1		0x00	R/W	
0x1D	REG001D	[7:0]	MUXOUT				R01D_RSV1	EN_CPTES T	CP_DOWN	CP_UP		0x00	R/W
0x1E	REG001E	[7:0]	R01E_RSV6	R01E_RSV5	R01E_RSV4		R01E_RSV3	R01E_RSV2	R01E_RSV1		0x00	R/W	
0x1F	REG001F	[7:0]	BST_REF	FILT_REF	REF_SEL	R01F_RSV2	R01F_RSV1				0x00	R/W	
0x20	REG0020	[7:0]	R020_RSV5		R020_RSV4	RST_SYS	EN_ADC_C LK	R020_RSV3	R020_RSV2	R020_RSV1		0x00	R/W
0x21	REG0021	[7:0]	R021_RSV7				R021_RSV3				0x00	R/W	
0x22	REG0022	[7:0]	R022_RSV0[7:0]								0x00	R/W	
0x23	REG0023	[7:0]	CAL_CT_SE L	R023_RSV6						R022_RSV 0[8]	0x00	R/W	
0x24	REG0024	[7:0]	R024_RSV4	R024_RSV3				DCLK_MOD E	R024_RSV2	R024_RSV1		0x00	R/W
0x25	REG0025	[7:0]	CLKODIV_D B	DCLK_DIV DB	R025_RSV3	R025_RSV2	R025_RSV1				0x00	R/W	
0x26	REG0026	[7:0]	VCO_BAND_DIV								0x00	R/W	

## REGISTER SUMMARY

Table 44. ADF4378 Register Summary (Continued)

Reg	Name	Bits	Bit 7	Bit 6	Bit 5	Bit 4	Bit 3	Bit 2	Bit 1	Bit 0	Reset	RW	
0x27	REG0027	[7:0]	SYNTH_LOCK_TIMEOUT[7:0]								0x00	R/W	
0x28	REG0028	[7:0]	O_VCO_DB	SYNTH_LOCK_TIMEOUT[14:8]								0x00	R/W
0x29	REG0029	[7:0]	VCO_ALC_TIMEOUT[7:0]								0x00	R/W	
0x2A	REG002A	[7:0]	DEL_CTRL_DB	VCO_ALC_TIMEOUT[14:8]								0x00	R/W
0x2B	REG002B	[7:0]	R02B_RSV1[7:0]								0x00	R/W	
0x2C	REG002C	[7:0]	R02C_RSV3			R02C_RSV2	R02B_RSV1[11:8]					0x00	R/W
0x2D	REG002D	[7:0]	ADC_CLK_DIV								0x00	R/W	
0x2E	REG002E	[7:0]	EN_ADC_CNV	R02E_RSV5	R02E_RSV4	R02E_RSV3	R02E_RSV2	R02E_RSV1	EN_ADC	ADC_A_CNV	0x00	R/W	
0x2F	REG002F	[7:0]	R02F_RSV5	R02F_RSV4	R02F_RSV3	R02F_RSV2	R02F_RSV1		DCLK_DIV1		0x00	R/W	
0x30	REG0030	[7:0]	R030_RSV4		R030_RSV3		R030_RSV2		R030_RSV1		0x00	R/W	
0x31	REG0031	[7:0]	R031_RSV6	R031_RSV5	R031_RSV4	R031_RSV3	R031_RSV2	R031_RSV1			0x00	R/W	
0x32	REG0032	[7:0]	R032_RSV5	ADC_CLK_SEL	R032_RSV4	R032_RSV3	R032_RSV2	R032_RSV1			0x00	R/W	
0x33	REG0033	[7:0]	R033_RSV6	R033_RSV5	R033_RSV4	R033_RSV3	R033_RSV2	R033_RSV1			0x00	R/W	
0x34	REG0034	[7:0]	R034_RSV5		R034_RSV4	R034_RSV3	R034_RSV2	R034_RSV1			0x00	R/W	
0x35	REG0035	[7:0]	R035_RSV1								0x00	R/W	
0x36	REG0036	[7:0]	R036_RSV3	R036_RSV2				R036_RSV1			0x00	R/W	
0x37	REG0037	[7:0]	R037_RSV7	R037_RSV6	R037_RSV5	R037_RSV4	R037_RSV3	R037_RSV2	R037_RSV1		0x00	R/W	
0x38	REG0038	[7:0]	R038_RSV1								0x00	R	
0x39	REG0039	[7:0]	R039_RSV1								0x00	R/W	
0x3A	REG003A	[7:0]	R03A_RSV1								0x00	R/W	
0x3B	REG003B	[7:0]	R03B_RSV2			R03B_RSV1					0x00	R/W	
0x3C	REG003C	[7:0]	R03C_RSV2				R03C_RSV1				0x00	R/W	
0x3D	REG003D	[7:0]	R03D_RSV2				O_VCO_BAND	O_VCO_CO RE	O_VCO_BIA S	R03D_RSV1		0x00	R/W
0x3E	REG003E	[7:0]	R03E_RSV8	R03E_RSV7	R03E_RSV6	R03E_RSV5	R03E_RSV4	R03E_RSV3	R03E_RSV2	R03E_RSV1	0x00	R/W	
0x3F	REG003F	[7:0]	R03F_RSV1								0x00	R/W	
0x40	REG0040	[7:0]	R040_RSV1								0x00	R/W	
0x41	REG0041	[7:0]	R041_RSV2				R041_RSV1				0x00	R/W	
0x42	REG0042	[7:0]	R042_RSV5	PD_SR_MON	SR_SEL	RST_SR_MON	R042_RSV1				0x00	R/W	
0x43	REG0043	[7:0]	INV_SR	SR_DEL							0x00	R/W	
0x44	REG0044	[7:0]	R044_RSV5	R044_RSV4			R044_RSV3	R044_RSV2	R044_RSV1		0x00	R/W	
0x45	REG0045	[7:0]	RESERVED								ADC_ST_CNV	0x00	R/W
0x46	REG0046	[7:0]	R046_RSV1[7:0]								0x00	R	
0x47	REG0047	[7:0]	R046_RSV1[15:8]								0x00	R	
0x48	REG0048	[7:0]	R046_RSV1[23:16]								0x00	R	
0x49	REG0049	[7:0]	EN_SYS	EN_CLK	SR_OK	R049_RSV1	REF_OK	ADC_BUSY	FSM_BUSY	LOCKED	0x00	R	
0x4A	REG004A	[7:0]	R04A_RSV1								0x00	R	
0x4B	REG004B	[7:0]	RESERVED						VCO_CORE			0x00	R
0x4C	REG004C	[7:0]	CHIP_TEMP[7:0]								0x00	R	
0x4D	REG004D	[7:0]	RESERVED								CHIP_TEMP[8]	0x00	R
0x4E	REG004E	[7:0]	R04E_RSV1								0x00	R	
0x4F	REG004F	[7:0]	VCO_BAND								0x00	R	

## REGISTER SUMMARY

Table 44. ADF4378 Register Summary (Continued)

Reg	Name	Bits	Bit 7	Bit 6	Bit 5	Bit 4	Bit 3	Bit 2	Bit 1	Bit 0	Reset	RW
0x50	REG0050	[7:0]					R050_RSV1				0x00	R
0x51	REG0051	[7:0]			RESERVED			VCO_BIAS			0x00	R
0x52	REG0052	[7:0]			RESERVED			R052_RSV1			0x00	R
0x53	REG0053	[7:0]			RESERVED				R053_RSV2	R053_RSV1	0x00	R
0x54	REG0054	[7:0]			VERSION						0x00	R

## REGISTER DETAILS

Address: 0x00, Reset: 0x00, Name: REG0000

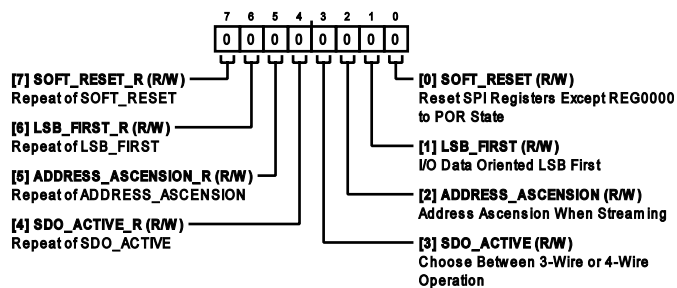


Figure 118.

Table 45. Bit Descriptions for REG0000

Bits	Bit Name	Description	Reset	Access
7	SOFT_RESET_R	Repeat of SOFT_RESET.	0x0	R/W
6	LSB_FIRST_R	Repeat of LSB_FIRST.	0x0	R/W
5	ADDRESS_ASCENSION_R	Repeat of ADDRESS_ASCENSION.	0x0	R/W
4	SDO_ACTIVE_R	Repeat of SDO_ACTIVE.	0x0	R/W
3	SDO_ACTIVE	Choose Between 3-Wire or 4-Wire Operation. 0: 3-wire. 1: 4-wire SPI (enables SDO and SDIO becomes an input only).	0x0	R/W
2	ADDRESS_ASCENSION	Address Ascension When Streaming. 0: address auto-decrements when streaming. 1: address auto-increments when streaming.	0x0	R/W
1	LSB_FIRST	I/O Data Oriented LSB First. 0: MSB first. 1: LSB first.	0x0	R/W
0	SOFT_RESET	Reset SPI Registers Except REG0000 to POR State. Self-clearing reset. 0: Normal operation. 1: Soft reset.	0x0	R/W

Address: 0x01, Reset: 0x00, Name: REG0001

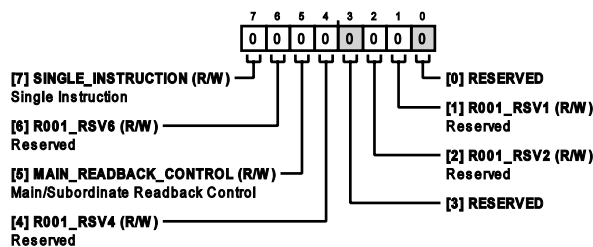


Figure 119.

Table 46. Bit Descriptions for REG0001

Bits	Bit Name	Description	Reset	Access
7	SINGLE_INSTRUCTION	Single Instruction. 0: SPI streaming enabled. 1: SPI streaming disabled.	0x0	R/W
6	R001_RSV6	Reserved.	0x0	R/W

REGISTER DETAILS

Table 46. Bit Descriptions for REG0001 (Continued)

Bits	Bit Name	Description	Reset	Access
5	MAIN_READBACK_CONTROL	Main/Subordinate Readback Control. 0: double buffering, readback subordinate register. 1: double buffering, readback main register.	0x0	R/W
4	R001_RSV4	Reserved.	0x0	R/W
3	RESERVED	Reserved.	0x0	R
2	R001_RSV2	Reserved.	0x0	R/W
1	R001_RSV1	Reserved.	0x0	R/W
0	RESERVED	Reserved.	0x0	R

Address: 0x02, Reset: 0x00, Name: REG0002

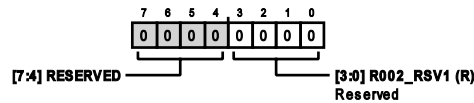


Figure 120.

Table 47. Bit Descriptions for REG0002

Bits	Bit Name	Description	Reset	Access
[7:4]	RESERVED	Reserved.	0x0	R
[3:0]	R002_RSV1	Reserved.	0x0	R

Address: 0x03, Reset: 0x00, Name: REG0003

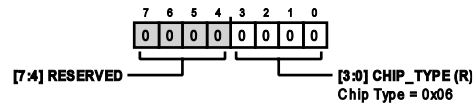


Figure 121.

Table 48. Bit Descriptions for REG0003

Bits	Bit Name	Description	Reset	Access
[7:4]	RESERVED	Reserved.	0x0	R
[3:0]	CHIP_TYPE	Chip Type = 0x06.	0x0	R

Address: 0x04, Reset: 0x00, Name: REG0004

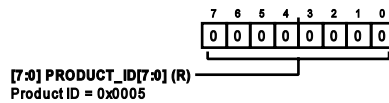


Figure 122.

Table 49. Bit Descriptions for REG0004

Bits	Bit Name	Description	Reset	Access
[7:0]	PRODUCT_ID[7:0]	Product ID = 0x0005.	0x0	R



## REGISTER DETAILS

Address: 0x05, Reset: 0x00, Name: REG0005

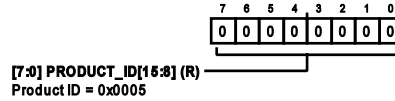


Figure 123.

Table 50. Bit Descriptions for REG0005

Bits	Bit Name	Description	Reset	Access
[7:0]	PRODUCT_ID[15:8]	Product ID = 0x0005.	0x0	R

Address: 0x06, Reset: 0x00, Name: REG0006

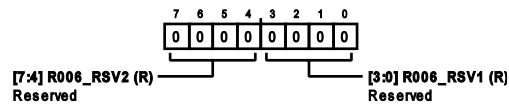


Figure 124.

Table 51. Bit Descriptions for REG0006

Bits	Bit Name	Description	Reset	Access
[7:4]	R006_RSV2	Reserved.	0x0	R
[3:0]	R006_RSV1	Reserved.	0x0	R

Address: 0x0A, Reset: 0x00, Name: REG000A

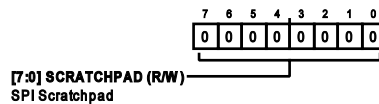


Figure 125.

Table 52. Bit Descriptions for REG000A

Bits	Bit Name	Description	Reset	Access
[7:0]	SCRATCHPAD	SPI Scratchpad.	0x0	R/W

Address: 0x0B, Reset: 0x00, Name: REG000B

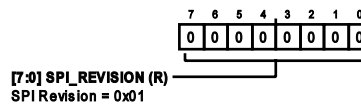


Figure 126.

Table 53. Bit Descriptions for REG000B

Bits	Bit Name	Description	Reset	Access
[7:0]	SPI_REVISION	SPI Revision = 0x01.	0x0	R

## REGISTER DETAILS

Address: 0x0C, Reset: 0x56, Name: REG000C

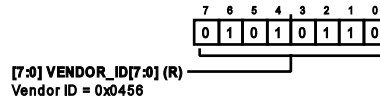


Figure 127.

Table 54. Bit Descriptions for REG000C

Bits	Bit Name	Description	Reset	Access
[7:0]	VENDOR_ID[7:0]	Vendor ID = 0x0456.	0x56	R

Address: 0x0D, Reset: 0x04, Name: REG000D

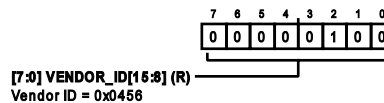


Figure 128.

Table 55. Bit Descriptions for REG000D

Bits	Bit Name	Description	Reset	Access
[7:0]	VENDOR_ID[15:8]	Vendor ID = 0x0456.	0x4	R

Address: 0x0F, Reset: 0x00, Name: REG000F

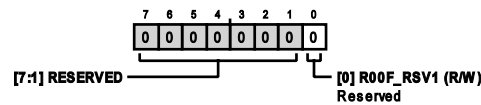


Figure 129.

Table 56. Bit Descriptions for REG000F

Bits	Bit Name	Description	Reset	Access
[7:1]	RESERVED	Reserved.	0x0	R
0	R00F_RSV1	Reserved.	0x0	R/W

Address: 0x10, Reset: 0x80, Name: REG0010

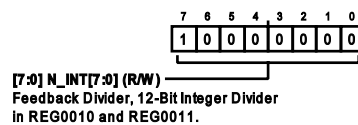


Figure 130.

Table 57. Bit Descriptions for REG0010

Bits	Bit Name	Description	Reset	Access
[7:0]	N_INT[7:0]	Feedback Divider, 12-Bit Integer Divider in REG0010 and REG0011. Set to any divide value from 2 to 4095, inclusive. Double buffering always enabled.	0x80	R/W

REGISTER DETAILS

Address: 0x11, Reset: 0x00, Name: REG0011

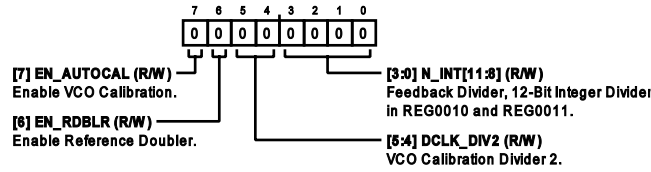


Figure 131.

Table 58. Bit Descriptions for REG0011

Bits	Bit Name	Description	Reset	Access
7	EN_AUTOCAL	Enable VCO Calibration. 0: disabled. 1: enabled.	0x0	R/W
6	EN_RDBLR	Enable Reference Doubler. 0: reference divider path selected. 1: reference doubler path selected.	0x0	R/W
[5:4]	DCLK_DIV2	VCO Calibration Divider 2. 00: divide by 1. 01: divide by 2. 10: divide by 4. 11: divide by 8.	0x0	R/W
[3:0]	N_INT[11:8]	Feedback Divider, 12-Bit Integer Divider in REG0010 and REG0011. Set to any divide value from 2 to 4095, inclusive. Double buffering always enabled.	0x0	R/W

Address: 0x12, Reset: 0x01, Name: REG0012

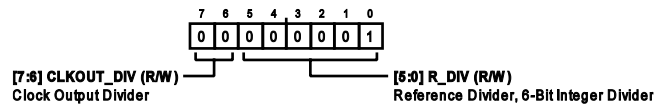


Figure 132.

Table 59. Bit Descriptions for REG0012

Bits	Bit Name	Description	Reset	Access
[7:6]	CLKOUT_DIV	Clock Output Divider. 00: divide by 1. 01: divide by 2. 10: divide by 4. 11: divide by 8.	0x0	R/W
[5:0]	R_DIV	Reference Divider, 6-Bit Integer Divider.	0x1	R/W

Address: 0x13, Reset: 0x00, Name: REG0013

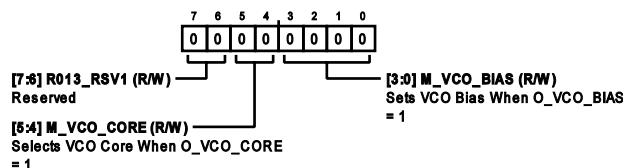


Figure 133.

REGISTER DETAILS

Table 60. Bit Descriptions for REG0013

Bits	Bit Name	Description	Reset	Access
[7:6]	R013_RSV1	Reserved.	0x0	R/W
[5:4]	M_VCO_CORE	Selects VCO Core When O_VCO_CORE = 1. 00: VCO 0 lowest frequency. 01: VCO 1. 10: VCO 2. 11: VCO 3 highest frequency.	0x0	R/W
[3:0]	M_VCO_BIAS	Sets VCO Bias When O_VCO_BIAS = 1. 0000: bias = 0. 0001: bias = 1. 0010: bias = 2. 0011: bias = 3. 0100: bias = 4. 0101: bias = 5. 0110: bias = 6. 0111: bias = 7. 1000: bias = 8. 1001: bias = 9. 1010: bias = 10. 1011: bias = 11. 1100: bias = 12. 1101: bias = 13. 1110: bias = 14. 1111: bias = 15.	0x0	R/W

Address: 0x14, Reset: 0x00, Name: REG0014

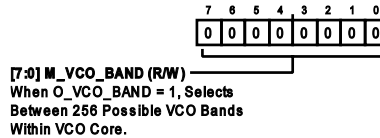


Figure 134.

Table 61. Bit Descriptions for REG0014

Bits	Bit Name	Description	Reset	Access
[7:0]	M_VCO_BAND	When O_VCO_BAND = 1, Selects Between 256 Possible VCO Bands Within VCO Core. 0: highest frequency VCO band. 255: lowest frequency VCO band.	0x0	R/W

Address: 0x15, Reset: 0x00, Name: REG0015

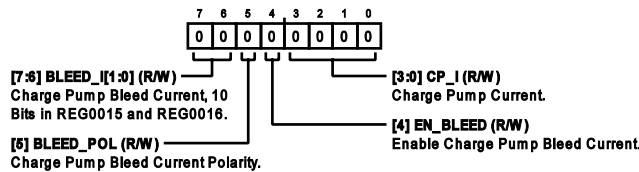


Figure 135.

REGISTER DETAILS

Table 62. Bit Descriptions for REG0015

Bits	Bit Name	Description	Reset	Access
[7:6]	BLEED_I[1:0]	Charge-Pump Bleed Current, 10 Bits in REG0015 and REG0016. For more information, see the <a href="#">Charge-Pump Bleed Current</a> section. Double buffering option.	0x0	R/W
5	BLEED_POL	Charge-Pump Bleed Current Polarity. 0: sink current. Increases reference input to clock output propagation delay. 1: source current. Decreases reference input to clock output propagation delay.	0x0	R/W
4	EN_BLEED	Enable Charge-Pump Bleed Current. 0: disabled. 1: enabled.	0x0	R/W
[3:0]	CP_I	Charge-Pump Current. 0000: 0.79 mA. 0001: 0.99 mA. 0010: 1.19 mA. 0011: 1.38 mA. 0100: 1.59 mA. 0101: 1.98 mA. 0110: 2.39 mA. 0111: 2.79 mA. 1000: 3.18 mA. 1001: 3.97 mA. 1010: 4.77 mA. 1011: 5.57 mA. 1100: 6.33 mA. 1101: 7.91 mA. 1110: 9.51 mA. 1111: 11.1 mA.	0x0	R/W

Address: 0x16, Reset: 0x00, Name: REG0016

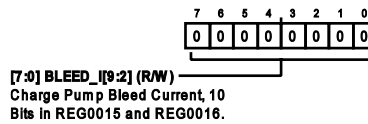


Figure 136.

Table 63. Bit Descriptions for REG0016

Bits	Bit Name	Description	Reset	Access
[7:0]	BLEED_I[9:2]	Charge-Pump Bleed Current, 10 Bits in REG0015 and REG0016. For more information, see the <a href="#">Charge-Pump Bleed Current</a> section. Double buffering option.	0x0	R/W

Address: 0x17, Reset: 0x00, Name: REG0017

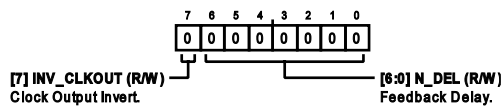


Figure 137.

## REGISTER DETAILS

Table 64. Bit Descriptions for REG0017

Bits	Bit Name	Description	Reset	Access
7	INV_CLKOUT	Clock Output Invert. Double buffering option. 0: not inverted. 1: inverted.	0x0	R/W
[6:0]	N_DEL	Feedback Delay. Decreases reference input to clock output propagation delay. Double buffering option.	0x0	R/W

Address: 0x18, Reset: 0x00, Name: REG0018

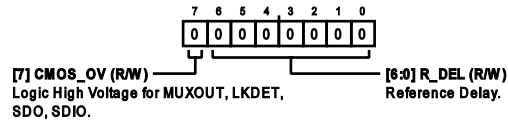


Figure 138.

Table 65. Bit Descriptions for REG0018

Bits	Bit Name	Description	Reset	Access
7	CMOS_OV	Logic High Voltage for MUXOUT, LKDET, SDO, SDIO. 0: 1.8 V logic. 1: 3.3 V logic.	0x0	R/W
[6:0]	R_DEL	Reference Delay. Increases reference input to clock output propagation delay. Double buffering option.	0x0	R/W

Address: 0x19, Reset: 0x04, Name: REG0019

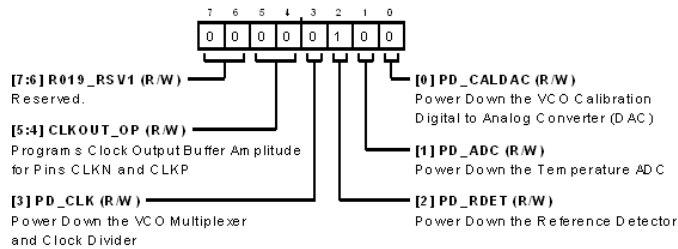


Figure 139.

Table 66. Bit Descriptions for REG0019

Bits	Bit Name	Description	Reset	Access
[7:6]	R019_RS1	Reserved. ADF4378 Register Map <a href="#">Register Summary</a> provides required reserved register settings.	0x0	R/W
[5:4]	CLKOUT_OP	Programs Clock Output Buffer Amplitude for CLK1N Pin and CLK1P Pin. 00: minimum amplitude, for more information, see the <a href="#">Specifications</a> section. 01: for more information, see the <a href="#">Specifications</a> section. 10: for more information, see the <a href="#">Specifications</a> section. 11: maximum amplitude, for more information, see the <a href="#">Specifications</a> section.	0x0	R/W
3	PD_CLK	Power-Down the VCO Multiplexer and Clock Divider. 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W
2	PD_RDET	Power-Down the Reference Detector. 0: active. Normal operation. 1: power-down.	0x1	R/W
1	PD_ADC	Power-Down the Temperature ADC. 0: active. Normal operation.	0x0	R/W

## REGISTER DETAILS

Table 66. Bit Descriptions for REG0019 (Continued)

Bits	Bit Name	Description	Reset	Access
0	PD_CALDAC	1: power-down. Power-Down the VCO Calibration Digital-to-Analog Converter (DAC). 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W

Address: 0x1A, Reset: 0x83, Name: REG001A

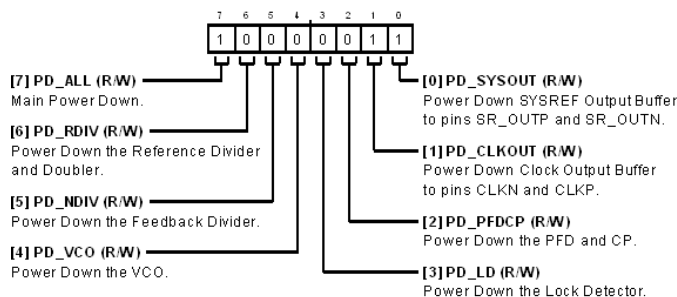


Figure 140.

Table 67. Bit Descriptions for REG001A

Bits	Bit Name	Description	Reset	Access
7	PD_ALL	Main Power-Down. 0: active. 1: power-down. Does not reset SPI registers to POR state. For more information, see the example in the <a href="#">Power-Up and Initialization Sequence</a> section.	0x1	R/W
6	PD_RDIV	Power-Down the Reference Divider and Doubler. 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W
5	PD_NDIV	Power-Down the Feedback Divider. 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W
4	PD_VCO	Power-Down the VCO. 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W
3	PD_LD	Power-Down the Lock Detector. 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W
2	PD_PFDPCP	Power-Down the PFD and CP. 0: active. Normal operation. 1: power-down. For more information, see the <a href="#">Block Power-Down Control</a> section.	0x0	R/W
1	PD_CLKOUT	Power-Down Clock Output Buffer to the CLKN Pin and CLKP Pin. 0: active. Normal operation. 1: power-down.	0x1	R/W
0	PD_SYSOUT	Power-Down SYSREF Output Buffer to pins SR_OUTP and SR_OUTN. 0: active. Normal operation. 1: power-down.	0x1	R/W

## REGISTER DETAILS

Address: 0x1B, Reset: 0x00, Name: REG001B

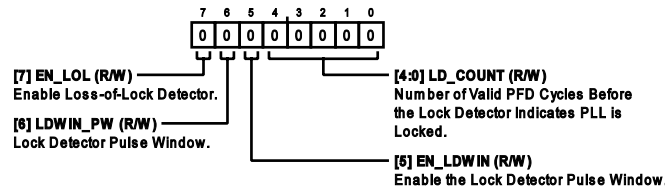


Figure 141.

Table 68. Bit Descriptions for REG001B

Bits	Bit Name	Description	Reset	Access
7	EN_LOL	Enable Loss-of-Lock Detector. 0: disabled. 1: enabled. Normal operation.	0x0	R/W
6	LDWIN_PW	Lock Detector Pulse Window. 0: narrow window. Normal operation. 1: wide window. For more information, see the <a href="#">Lock Detector</a> section.	0x0	R/W
5	EN_LDWIN	Enable the Lock Detector Pulse Window. 0: disabled. 1: enabled. Normal operation.	0x0	R/W
[4:0]	LD_COUNT	Number of Valid PFD Cycles Before the Lock Detector Indicates PLL is Locked. For more information, see the <a href="#">Lock Detector</a> section.	0x0	R/W

Address: 0x1C, Reset: 0x00, Name: REG001C

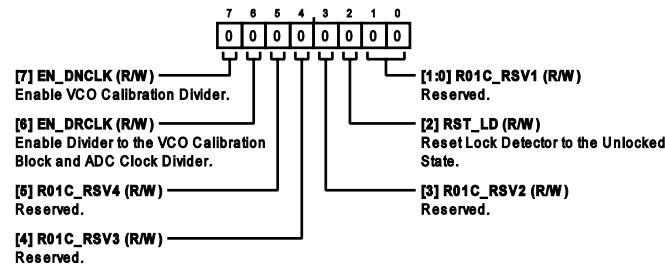


Figure 142.

Table 69. Bit Descriptions for REG001C

Bits	Bit Name	Description	Reset	Access
7	EN_DNCLK	Enable VCO Calibration Divider. For more information, see <a href="#">Figure 75</a> . 0: disabled. Disable when not in use to reduce spurious content. 1: enabled. Enable before a VCO calibration begins.	0x0	R/W
6	EN_DRCLK	Enable Divider to the VCO Calibration Block and ADC Clock Divider. For more information, see <a href="#">Figure 75</a> . 0: disabled. Disable when not in use to reduce spurious content. 1: enabled. Enable before a VCO calibration or temperature sensor measurement begins.	0x0	R/W
5	R01C_RSV4	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
4	R01C_RSV3	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
3	R01C_RSV2	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
2	RST_LD	Reset Lock Detector to the Unlocked State. This bit is not self-clearing. 0: reset inactive. Normal operation. 1: reset active.	0x0	R/W



## REGISTER DETAILS

Table 69. Bit Descriptions for REG001C (Continued)

Bits	Bit Name	Description	Reset	Access
[1:0]	R01C_RSV1	Reserved. Table 44 provides required reserved register settings.	0x0	R/W

Address: 0x1D, Reset: 0x00, Name: REG001D

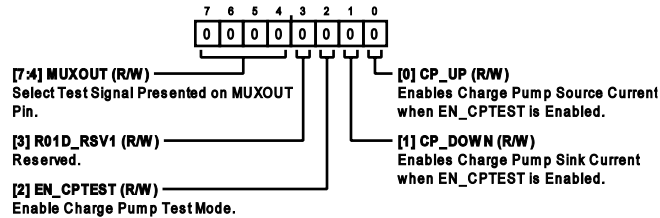


Figure 143.

Table 70. Bit Descriptions for REG001D

Bits	Bit Name	Description	Reset	Access
[7:4]	MUXOUT	Select Test Signal Presented on MUXOUT Pin. 0000: high-Z. 0001: LKDET. Lock detector output. 0010: low. 0011: low. 0100: $f_{DIV\_RCLK}/2$ . 0101: $f_{DIV\_NCLK}/2$ . 0110: reserved. 0111: low. 1000: high. 1001: reserved. 1010: reserved. 1011: low. 1100: low. 1101: low. 1110: reserved. 1111: reserved.	0x0	R/W
3	R01D_RSV1	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
2	EN_CPTTEST	Enable Charge-Pump Test Mode. 0: disabled. Normal operation. 1: enabled.	0x0	R/W
1	CP_DOWN	Enables Charge-Pump Sink Current when EN_CPTTEST is Enabled. 0: disabled. 1: enabled.	0x0	R/W
0	CP_UP	Enables Charge-Pump Source Current when EN_CPTTEST is Enabled. 0: disabled. 1: enabled.	0x0	R/W

## REGISTER DETAILS

Address: 0x1E, Reset: 0x00, Name: REG001E

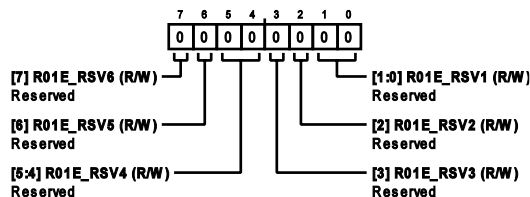


Figure 144.

Table 71. Bit Descriptions for REG001E

Bits	Bit Name	Description	Reset	Access
7	R01E_RSV6	Reserved.	0x0	R/W
6	R01E_RSV5	Reserved.	0x0	R/W
[5:4]	R01E_RSV4	Reserved.	0x0	R/W
3	R01E_RSV3	Reserved.	0x0	R/W
2	R01E_RSV2	Reserved.	0x0	R/W
[1:0]	R01E_RSV1	Reserved.	0x0	R/W

Address: 0x1F, Reset: 0x00, Name: REG001F

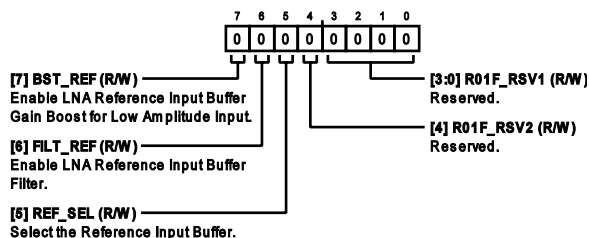


Figure 145.

Table 72. Bit Descriptions for REG001F

Bits	Bit Name	Description	Reset	Access
7	BST_REF	Enable LNA Reference Input Buffer Gain Boost for Low Amplitude Input. For more information, see <a href="#">Table 9</a> . 0: disabled. 1: enabled.	0x0	R/W
6	FILT_REF	Enable LNA Reference Input Buffer Filter. For more information, see <a href="#">Table 8</a> . 0: disabled. 1: enabled.	0x0	R/W
5	REF_SEL	Select the Reference Input Buffer. For more information, see <a href="#">Table 7</a> . 0: DMA for an improved reference input to clock output propagation delay temperature coefficient. 1: LNA for improved PLL in-band noise when a low slew rate signal is applied to the reference input.	0x0	R/W
4	R01F_RSV2	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
[3:0]	R01F_RSV1	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W

REGISTER DETAILS

Address: 0x20, Reset: 0x00, Name: REG0020

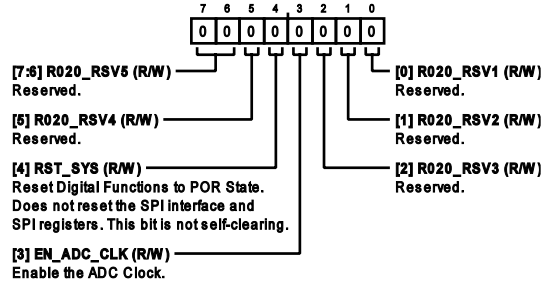


Figure 146.

Table 73. Bit Descriptions for REG0020

Bits	Bit Name	Description	Reset	Access
[7:6]	R020_RSV5	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
5	R020_RSV4	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
4	RST_SYS	Reset Digital Functions to POR State. Does not reset the SPI interface and SPI registers. This bit is not self-clearing. 0: reset inactive. Normal operation. 1: reset active.	0x0	R/W
3	EN_ADC_CLK	Enable the ADC Clock. For more information, see Figure 75. 0: disabled. 1: enabled. Normal operation.	0x0	R/W
2	R020_RSV3	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
1	R020_RSV2	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
0	R020_RSV1	Reserved. Table 44 provides required reserved register settings.	0x0	R/W

Address: 0x21, Reset: 0x00, Name: REG0021

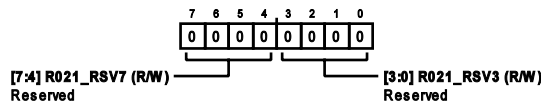


Figure 147.

Table 74. Bit Descriptions for REG0021

Bits	Bit Name	Description	Reset	Access
[7:4]	R021_RSV7	Reserved.	0x0	R/W
[3:0]	R021_RSV3	Reserved.	0x0	R/W

Address: 0x22, Reset: 0x00, Name: REG0022

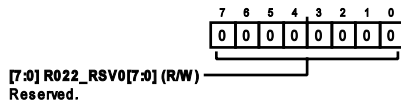


Figure 148.

Table 75. Bit Descriptions for REG0022

Bits	Bit Name	Description	Reset	Access
[7:0]	R022_RSV0[7:0]	Reserved. Table 44 provides required reserved register settings.	0x0	R/W

## REGISTER DETAILS

Address: 0x23, Reset: 0x00, Name: REG0023

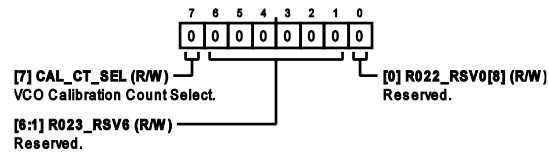


Figure 149.

Table 76. Bit Descriptions for REG0023

Bits	Bit Name	Description	Reset	Access
7	CAL_CT_SEL	VCO Calibration Count Select. For more information, see <a href="#">Table 17</a> .	0x0	R/W
[6:1]	R023_RSV6	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
0	R022_RSV0[8]	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W

Address: 0x24, Reset: 0x00, Name: REG0024

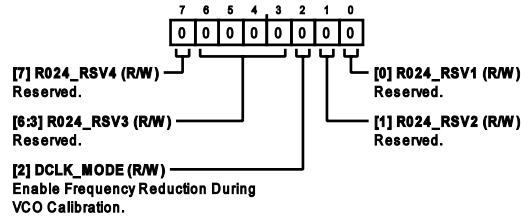


Figure 150.

Table 77. Bit Descriptions for REG0024

Bits	Bit Name	Description	Reset	Access
7	R024_RSV4	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
[6:3]	R024_RSV3	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
2	DCLK_MODE	Enable Frequency Reduction During VCO Calibration. Divides $f_{DIV\_RCLK}$ and $f_{DIV\_NCLK}$ by 2 when enabled. For more information, see <a href="#">Table 17</a> . 0: disabled. 1: enabled.	0x0	R/W
1	R024_RSV2	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
0	R024_RSV1	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W

Address: 0x25, Reset: 0x00, Name: REG0025

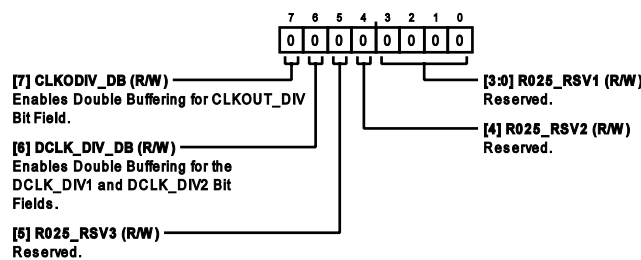


Figure 151.

REGISTER DETAILS

Table 78. Bit Descriptions for REG0025

Bits	Bit Name	Description	Reset	Access
7	CLKODIV_DB	Enables Double Buffering for CLKOUT_DIV Bit Field. 0: disabled. 1: enabled.	0x0	R/W
6	DCLK_DIV_DB	Enables Double Buffering for the DCLK_DIV1 and DCLK_DIV2 Bit Fields. 0: disabled. 1: enabled.	0x0	R/W
5	R025_RSV3	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
4	R025_RSV2	Reserved. Table 44 provides required reserved register settings.	0x0	R/W
[3:0]	R025_RSV1	Reserved. Table 44 provides required reserved register settings.	0x0	R/W

Address: 0x26, Reset: 0x00, Name: REG0026

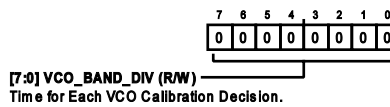


Figure 152.

Table 79. Bit Descriptions for REG0026

Bits	Bit Name	Description	Reset	Access
[7:0]	VCO_BAND_DIV	Time for Each VCO Calibration Decision. Determined by the equation shown in the VCO Calibration section.	0x0	R/W

Address: 0x27, Reset: 0x00, Name: REG0027

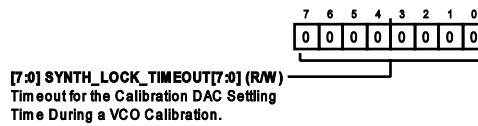


Figure 153.

Table 80. Bit Descriptions for REG0027

Bits	Bit Name	Description	Reset	Access
[7:0]	SYNTH_LOCK_TIMEOUT[7:0]	Timeout for the Calibration DAC Settling Time During a VCO Calibration. Determined by the equation shown in the VCO Calibration section.	0x0	R/W

Address: 0x28, Reset: 0x00, Name: REG0028

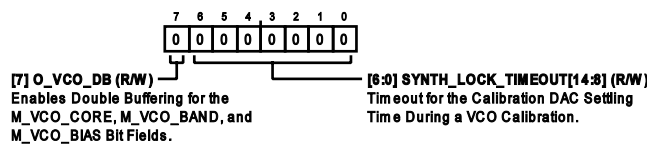


Figure 154.

Table 81. Bit Descriptions for REG0028

Bits	Bit Name	Description	Reset	Access
7	O_VCO_DB	Enables Double Buffering for the M_VCO_CORE, M_VCO_BAND, and M_VCO_BIAS Bit Fields. 0: disabled.	0x0	R/W

## REGISTER DETAILS

Table 81. Bit Descriptions for REG0028 (Continued)

Bits	Bit Name	Description	Reset	Access
[6:0]	SYNTH_LOCK_TIMEOUT[14:8]	1: enabled. Timeout for the Calibration DAC Settling Time During a VCO Calibration. Determined by the equation shown in the <a href="#">VCO Calibration</a> section.	0x0	R/W

Address: 0x29, Reset: 0x00, Name: REG0029

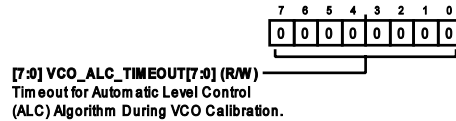


Figure 155.

Table 82. Bit Descriptions for REG0029

Bits	Bit Name	Description	Reset	Access
[7:0]	VCO_ALC_TIMEOUT[7:0]	Timeout for Automatic Level Control (ALC) Algorithm During VCO Calibration. Determined by the equation shown in the <a href="#">VCO Calibration</a> section.	0x0	R/W

Address: 0x2A, Reset: 0x00, Name: REG002A

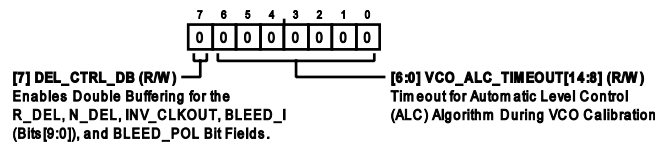


Figure 156.

Table 83. Bit Descriptions for REG002A

Bits	Bit Name	Description	Reset	Access
7	DEL_CTRL_DB	Enables Double Buffering for the R_DEL, N_DEL, INV_CLKOUT, BLEED_I (Bits[9:0]), and BLEED_POL Bit Fields. 0: disabled. 1: enabled.	0x0	R/W
[6:0]	VCO_ALC_TIMEOUT[14:8]	Timeout for Automatic Level Control (ALC) Algorithm During VCO Calibration. Determined by the equation shown in the <a href="#">VCO Calibration</a> section.	0x0	R/W

Address: 0x2B, Reset: 0x00, Name: REG002B

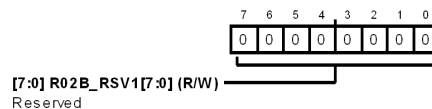


Figure 157.

Table 84. Bit Descriptions for REG002B

Bits	Bit Name	Description	Reset	Access
[7:0]	R02B_RSV1[7:0]	Reserved.	0x0	R/W

## REGISTER DETAILS

Address: 0x2C, Reset: 0x00, Name: REG002C

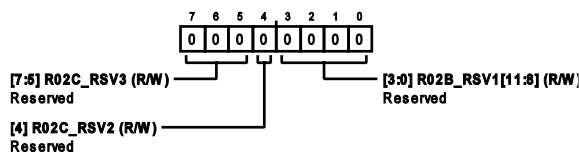


Figure 158.

Table 85. Bit Descriptions for REG002C

Bits	Bit Name	Description	Reset	Access
[7:5]	R02C_RSV3	Reserved.	0x0	R/W
4	R02C_RSV2	Reserved.	0x0	R/W
[3:0]	R02B_RSV1[11:8]	Reserved.	0x0	R/W

Address: 0x2D, Reset: 0x00, Name: REG002D

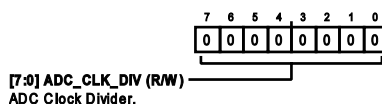


Figure 159.

Table 86. Bit Descriptions for REG002D

Bits	Bit Name	Description	Reset	Access
[7:0]	ADC_CLK_DIV	ADC Clock Divider. Determined by the equation shown in the <a href="#">VCO Calibration</a> section.	0x0	R/W

Address: 0x2E, Reset: 0x00, Name: REG002E

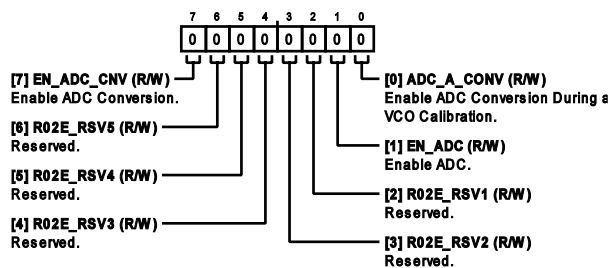


Figure 160.

Table 87. Bit Descriptions for REG002E

Bits	Bit Name	Description	Reset	Access
7	EN_ADC_CNV	Enable ADC Conversion. For more information, see the <a href="#">Temperature Sensor</a> section. 0: disabled. 1: enabled. Normal operation.	0x0	R/W
6	R02E_RSV5	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
5	R02E_RSV4	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
4	R02E_RSV3	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
3	R02E_RSV2	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
2	R02E_RSV1	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
1	EN_ADC	Enable ADC. For more information, see the <a href="#">Temperature Sensor</a> section.	0x0	R/W

REGISTER DETAILS

Table 87. Bit Descriptions for REG002E (Continued)

Bits	Bit Name	Description	Reset	Access
0	ADC_A_CONV	0: ADC conversion only possible with a write to the ADC_ST_CNVR bit field. 1: enabled. Normal operation.  Enable ADC Conversion During a VCO Calibration. 0: ADC conversion only possible with write to ADC_ST_CNVR bit. 1: enabled. Normal operation. Automatically begins ADC conversion at the start of a VCO calibration or with a write to the ADC_ST_CNVR bit.	0x0	R/W

Address: 0x2F, Reset: 0x00, Name: REG002F

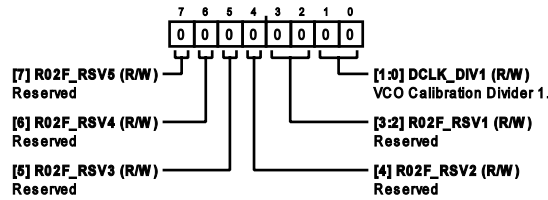


Figure 161.

Table 88. Bit Descriptions for REG002F

Bits	Bit Name	Description	Reset	Access
7	R02F_RSV5	Reserved.	0x0	R/W
6	R02F_RSV4	Reserved.	0x0	R/W
5	R02F_RSV3	Reserved.	0x0	R/W
4	R02F_RSV2	Reserved.	0x0	R/W
[3:2]	R02F_RSV1	Reserved.	0x0	R/W
[1:0]	DCLK_DIV1	VCO Calibration Divider 1. 0: divide by 1. 1: divide by 2. 10: divide by 8. 11: divide by 32.	0x0	R/W

Address: 0x30, Reset: 0x00, Name: REG0030

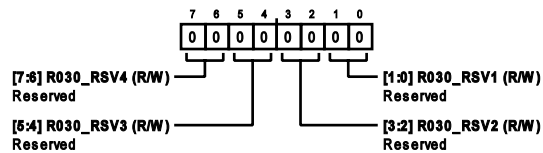


Figure 162.

Table 89. Bit Descriptions for REG0030

Bits	Bit Name	Description	Reset	Access
[7:6]	R030_RSV4	Reserved.	0x0	R/W
[5:4]	R030_RSV3	Reserved.	0x0	R/W
[3:2]	R030_RSV2	Reserved.	0x0	R/W
[1:0]	R030_RSV1	Reserved.	0x0	R/W



REGISTER DETAILS

Address: 0x31, Reset: 0x00, Name: REG0031

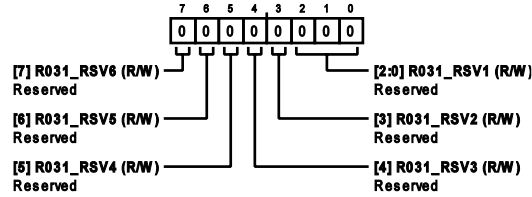


Figure 163.

Table 90. Bit Descriptions for REG0031

Bits	Bit Name	Description	Reset	Access
7	R031_RSV6	Reserved.	0x0	R/W
6	R031_RSV5	Reserved.	0x0	R/W
5	R031_RSV4	Reserved.	0x0	R/W
4	R031_RSV3	Reserved.	0x0	R/W
3	R031_RSV2	Reserved.	0x0	R/W
[2:0]	R031_RSV1	Reserved.	0x0	R/W

Address: 0x32, Reset: 0x00, Name: REG0032

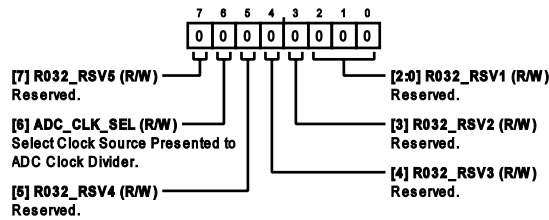


Figure 164.

Table 91. Bit Descriptions for REG0032

Bits	Bit Name	Description	Reset	Access
7	R032_RSV5	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
6	ADC_CLK_SEL	Select Clock Source Presented to ADC Clock Divider. For more information, see <a href="#">Figure 75</a> . 0: select internal clock. Normal operation. Used during VCO calibrations and full power die temperature measurement. 1: select SCLK pin. Ambient die temperature measurements with the temperature sensor. For more information, see the <a href="#">Temperature Sensor</a> section.	0x0	R/W
5	R032_RSV4	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
4	R032_RSV3	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
3	R032_RSV2	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
[2:0]	R032_RSV1	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W

REGISTER DETAILS

Address: 0x33, Reset: 0x00, Name: REG0033

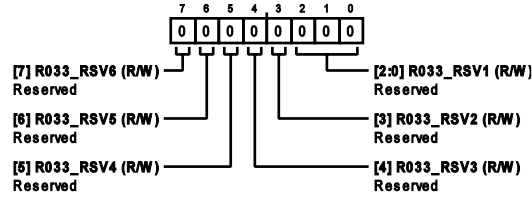


Figure 165.

Table 92. Bit Descriptions for REG0033

Bits	Bit Name	Description	Reset	Access
7	R033_RSV6	Reserved.	0x0	R/W
6	R033_RSV5	Reserved.	0x0	R/W
5	R033_RSV4	Reserved.	0x0	R/W
4	R033_RSV3	Reserved.	0x0	R/W
3	R033_RSV2	Reserved.	0x0	R/W
[2:0]	R033_RSV1	Reserved.	0x0	R/W

Address: 0x34, Reset: 0x00, Name: REG0034

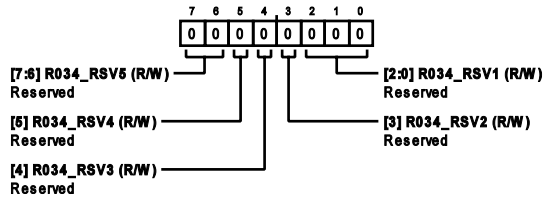


Figure 166.

Table 93. Bit Descriptions for REG0034

Bits	Bit Name	Description	Reset	Access
[7:6]	R034_RSV5	Reserved.	0x0	R/W
5	R034_RSV4	Reserved.	0x0	R/W
4	R034_RSV3	Reserved.	0x0	R/W
3	R034_RSV2	Reserved.	0x0	R/W
[2:0]	R034_RSV1	Reserved.	0x0	R/W

Address: 0x35, Reset: 0x00, Name: REG0035

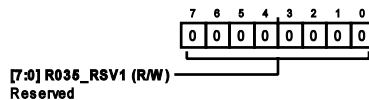


Figure 167.

Table 94. Bit Descriptions for REG0035

Bits	Bit Name	Description	Reset	Access
[7:0]	R035_RSV1	Reserved.	0x0	R/W

## REGISTER DETAILS

Address: 0x36, Reset: 0x00, Name: REG0036

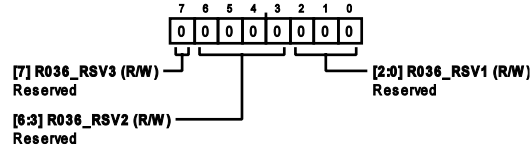


Figure 168.

Table 95. Bit Descriptions for REG0036

Bits	Bit Name	Description	Reset	Access
7	R036_RSV3	Reserved.	0x0	R/W
[6:3]	R036_RSV2	Reserved.	0x0	R/W
[2:0]	R036_RSV1	Reserved.	0x0	R/W

Address: 0x37, Reset: 0x00, Name: REG0037

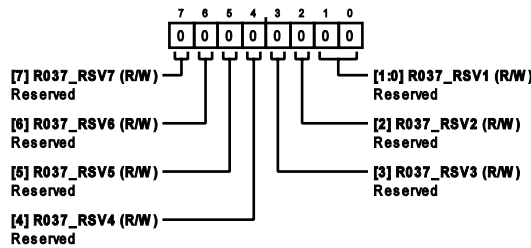


Figure 169.

Table 96. Bit Descriptions for REG0037

Bits	Bit Name	Description	Reset	Access
7	R037_RSV7	Reserved.	0x0	R/W
6	R037_RSV6	Reserved.	0x0	R/W
5	R037_RSV5	Reserved.	0x0	R/W
4	R037_RSV4	Reserved.	0x0	R/W
3	R037_RSV3	Reserved.	0x0	R/W
2	R037_RSV2	Reserved.	0x0	R/W
[1:0]	R037_RSV1	Reserved.	0x0	R/W

Address: 0x38, Reset: 0x00, Name: REG0038

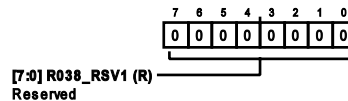


Figure 170.

Table 97. Bit Descriptions for REG0038

Bits	Bit Name	Description	Reset	Access
[7:0]	R038_RSV1	Reserved.	0x0	R

## REGISTER DETAILS

Address: 0x39, Reset: 0x00, Name: REG0039

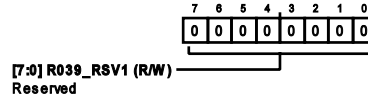


Figure 171.

Table 98. Bit Descriptions for REG0039

Bits	Bit Name	Description	Reset	Access
[7:0]	R039_RSV1	Reserved.	0x0	R/W

Address: 0x3A, Reset: 0x00, Name: REG003A

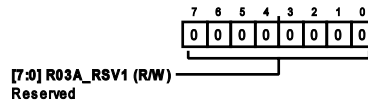


Figure 172.

Table 99. Bit Descriptions for REG003A

Bits	Bit Name	Description	Reset	Access
[7:0]	R03A_RSV1	Reserved.	0x0	R/W

Address: 0x3B, Reset: 0x00, Name: REG003B

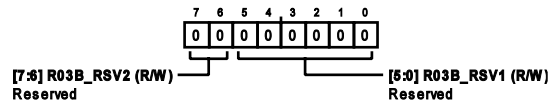


Figure 173.

Table 100. Bit Descriptions for REG003B

Bits	Bit Name	Description	Reset	Access
[7:6]	R03B_RSV2	Reserved.	0x0	R/W
[5:0]	R03B_RSV1	Reserved.	0x0	R/W

Address: 0x3C, Reset: 0x00, Name: REG003C

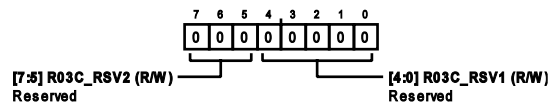


Figure 174.

Table 101. Bit Descriptions for REG003C

Bits	Bit Name	Description	Reset	Access
[7:5]	R03C_RSV2	Reserved.	0x0	R/W
[4:0]	R03C_RSV1	Reserved.	0x0	R/W

## REGISTER DETAILS

Address: 0x3D, Reset: 0x00, Name: REG003D

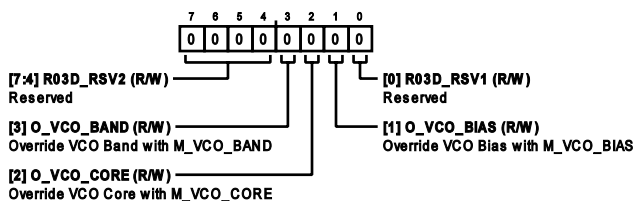


Figure 175.

Table 102. Bit Descriptions for REG003D

Bits	Bit Name	Description	Reset	Access
[7:4]	R03D_RSV2	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W
3	O_VCO_BAND	Override VCO Band with M_VCO_BAND. 0: VCO band code from VCO calibration state machine. 1: VCO band code from M_VCO_BAND.	0x0	R/W
2	O_VCO_CORE	Override VCO Core with M_VCO_CORE. For more information, see the <a href="#">VCO Calibration</a> section. 0: VCO core set by the VCO calibration state machine. 1: VCO core set by M_VCO_CORE.	0x0	R/W
1	O_VCO_BIAS	Override VCO Bias with M_VCO_BIAS. For more information, see the <a href="#">VCO Calibration</a> section. 0: VCO bias set by the VCO calibration state machine. 1: VCO bias set by M_VCO_BIAS.	0x0	R/W
0	R03D_RSV1	Reserved. <a href="#">Table 44</a> provides required reserved register settings.	0x0	R/W

Address: 0x3E, Reset: 0x00, Name: REG003E

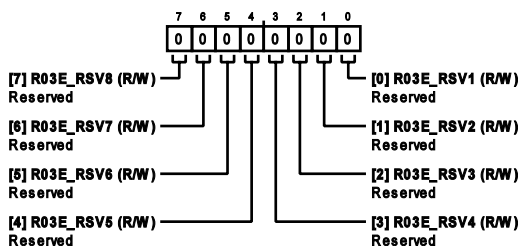


Figure 176.

Table 103. Bit Descriptions for REG003E

Bits	Bit Name	Description	Reset	Access
7	R03E_RSV8	Reserved.	0x0	R/W
6	R03E_RSV7	Reserved.	0x0	R/W
5	R03E_RSV6	Reserved.	0x0	R/W
4	R03E_RSV5	Reserved.	0x0	R/W
3	R03E_RSV4	Reserved.	0x0	R/W
2	R03E_RSV3	Reserved.	0x0	R/W
1	R03E_RSV2	Reserved.	0x0	R/W
0	R03E_RSV1	Reserved.	0x0	R/W

REGISTER DETAILS

Address: 0x3F, Reset: 0x00, Name: REG003F

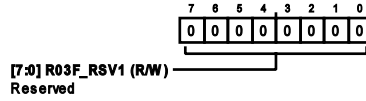


Figure 177.

Table 104. Bit Descriptions for REG003F

Bits	Bit Name	Description	Reset	Access
[7:0]	R03F_RSV1	Reserved.	0x0	R/W

Address: 0x40, Reset: 0x00, Name: REG0040

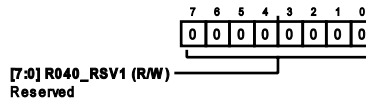


Figure 178.

Table 105. Bit Descriptions for REG0040

Bits	Bit Name	Description	Reset	Access
[7:0]	R040_RSV1	Reserved.	0x0	R/W

Address: 0x41, Reset: 0x00, Name: REG0041

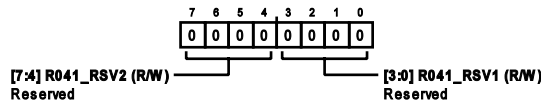


Figure 179.

Table 106. Bit Descriptions for REG0041

Bits	Bit Name	Description	Reset	Access
[7:4]	R041_RSV2	Reserved.	0x0	R/W
[3:0]	R041_RSV1	Reserved.	0x0	R/W

Address: 0x42, Reset: 0x00, Name: REG0042

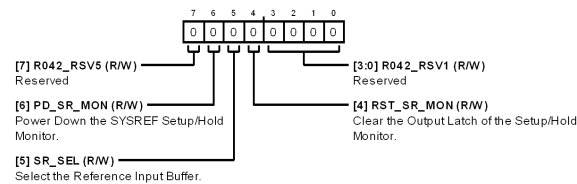


Figure 180.

Table 107. Bit Descriptions for REG0042

Bits	Bit Name	Description	Reset	Access
7	R042_RSV5	Reserved.	0x0	R/W
6	PD_SR_MON	Power-Down the SYSREF Setup/Hold Monitor. 0: active. Normal Operation. 1: Power-down Mode.	0x0	R/W

## REGISTER DETAILS

Table 107. Bit Descriptions for REG0042 (Continued)

Bits	Bit Name	Description	Reset	Access
5	SR_SEL	Select the Reference Input Buffer. 0: CML/LVPECL input buffer. 1: LVDS input buffer.	0x0	R/W
4	RST_SR_MON	Clear the Output Latch of the Setup/Hold Monitor. This bit is not self-clearing. 0: Reset Inactive. Normal Operation. 1: Reset Active.	0x0	R/W
[3:0]	R042_RSV1	Reserved.	0x0	R/W

Address: 0x43, Reset: 0x00, Name: REG0043

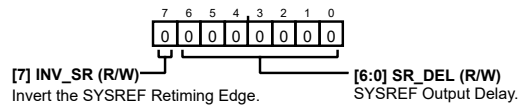


Figure 181.

Table 108. Bit Descriptions for REG0043

Bits	Bit Name	Description	Reset	Access
7	INV_SR	Invert the SYSREF Retiming Edge. Delays SYSREF output by 1/2 clock output period. 1: Not Inverted. 0: Inverted.	0x0	R/W
[6:0]	SR_DEL	SYSREF Output Delay. Puts delay to SYSREF output.	0x0	R/W

Address: 0x44, Reset: 0x00, Name: REG0044

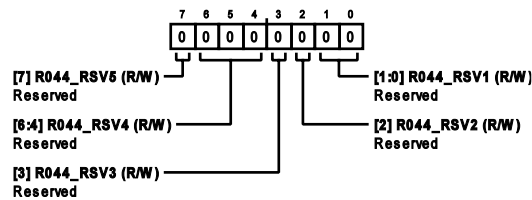


Figure 182.

Table 109. Bit Descriptions for REG0044

Bits	Bit Name	Description	Reset	Access
7	R044_RSV5	Reserved.	0x0	R/W
[6:4]	R044_RSV4	Reserved.	0x0	R/W
3	R044_RSV3	Reserved.	0x0	R/W
2	R044_RSV2	Reserved.	0x0	R/W
[1:0]	R044_RSV1	Reserved.	0x0	R/W

Address: 0x45, Reset: 0x00, Name: REG0045

For more information, see the [Temperature Sensor](#) section.

REGISTER DETAILS

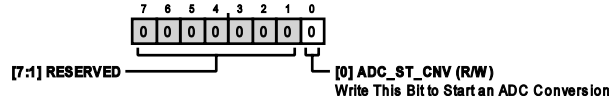


Figure 183.

Table 110. Bit Descriptions for REG0045

Bits	Bit Name	Description	Reset	Access
[7:1]	RESERVED	Reserved.	0x0	R
0	ADC_ST_CNV	Write This Bit to Start an ADC Conversion.	0x0	R/W

Address: 0x46, Reset: 0x00, Name: REG0046

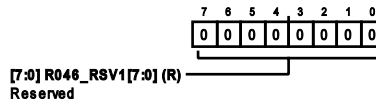


Figure 184.

Table 111. Bit Descriptions for REG0046

Bits	Bit Name	Description	Reset	Access
[7:0]	R046_RSV1[7:0]	Reserved.	0x0	R

Address: 0x47, Reset: 0x00, Name: REG0047

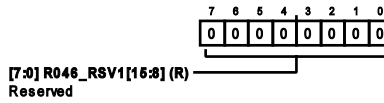


Figure 185.

Table 112. Bit Descriptions for REG0047

Bits	Bit Name	Description	Reset	Access
[7:0]	R046_RSV1[15:8]	Reserved.	0x0	R

Address: 0x48, Reset: 0x00, Name: REG0048

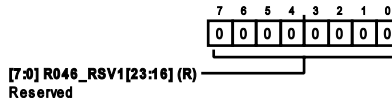


Figure 186.

Table 113. Bit Descriptions for REG0048

Bits	Bit Name	Description	Reset	Access
[7:0]	R046_RSV1[23:16]	Reserved.	0x0	R



REGISTER DETAILS

Address: 0x49, Reset: 0x00, Name: REG0049

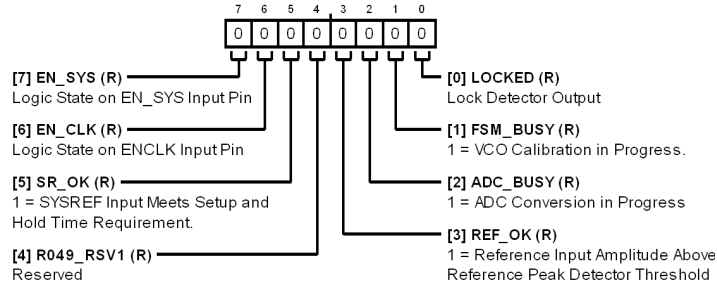


Figure 187.

Table 114. Bit Descriptions for REG0049

Bits	Bit Name	Description	Reset	Access
7	EN_SYS	Logic State on ENSR Input Pin. For more information, see <a href="#">Figure 80</a> .	0x0	R
6	EN_CLK1	Logic State on ENCLK Input Pin. For more information, see <a href="#">Figure 79</a> .	0x0	R
5	SR_OK	1 = SYSREF Input Meets Setup and Hold Time Requirement.	0x0	R
4	R049_RSV1	Reserved.	0x0	R
3	REF_OK	1 = Reference Input Amplitude Above Reference Peak Detector Threshold.	0x0	R
2	ADC_BUSY	1 = ADC Conversion in Progress. For more information, see the <a href="#">VCO Calibration</a> and the <a href="#">Temperature Sensor</a> sections.	0x0	R
1	FSM_BUSY	1 = VCO Calibration in Progress.	0x0	R
0	LOCKED	Lock Detector Output.	0x0	R

Address: 0x4A, Reset: 0x00, Name: REG004A

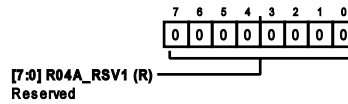


Figure 188.

Table 115. Bit Descriptions for REG004A

Bits	Bit Name	Description	Reset	Access
[7:0]	R04A_RSV1	Reserved.	0x0	R

Address: 0x4B, Reset: 0x00, Name: REG004B

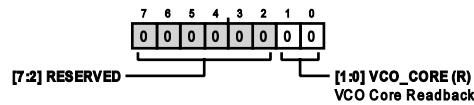


Figure 189.

Table 116. Bit Descriptions for REG004B

Bits	Bit Name	Description	Reset	Access
[7:2]	RESERVED	Reserved.	0x0	R
[1:0]	VCO_CORE	VCO Core Readback. For more information, see the <a href="#">VCO Calibration</a> section.	0x0	R

## REGISTER DETAILS

Address: 0x4C, Reset: 0x00, Name: REG004C

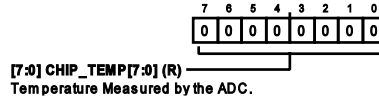


Figure 190.

Table 117. Bit Descriptions for REG004C

Bits	Bit Name	Description	Reset	Access
[7:0]	CHIP_TEMP[7:0]	Temperature Measured by the ADC. CHIP_TEMP[8] is the sign bit, where 0 = positive and 1 = negative. CHIP_TEMP[7:0] = magnitude.	0x0	R

Address: 0x4D, Reset: 0x00, Name: REG004D

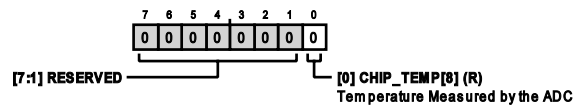


Figure 191.

Table 118. Bit Descriptions for REG004D

Bits	Bit Name	Description	Reset	Access
[7:1]	RESERVED	Reserved.	0x0	R
0	CHIP_TEMP[8]	Temperature Measured by the ADC. CHIP_TEMP[8] is the sign bit, where 0 = positive and 1 = negative. CHIP_TEMP[7:0] = magnitude.	0x0	R

Address: 0x4E, Reset: 0x00, Name: REG004E

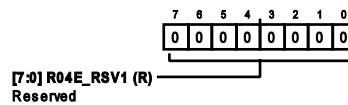


Figure 192.

Table 119. Bit Descriptions for REG004E

Bits	Bit Name	Description	Reset	Access
[7:0]	R04E_RSV1	Reserved.	0x0	R

Address: 0x4F, Reset: 0x00, Name: REG004F

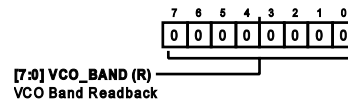


Figure 193.

Table 120. Bit Descriptions for REG004F

Bits	Bit Name	Description	Reset	Access
[7:0]	VCO_BAND	VCO Band Readback. For more information, see the <a href="#">VCO Calibration</a> section.	0x0	R

REGISTER DETAILS

Address: 0x50, Reset: 0x00, Name: REG0050

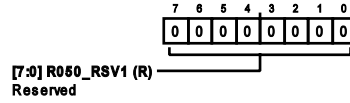


Figure 194.

Table 121. Bit Descriptions for REG0050

Bits	Bit Name	Description	Reset	Access
[7:0]	R050_RSV1	Reserved.	0x0	R

Address: 0x51, Reset: 0x00, Name: REG0051

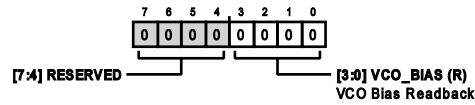


Figure 195.

Table 122. Bit Descriptions for REG0051

Bits	Bit Name	Description	Reset	Access
[7:4]	RESERVED	Reserved.	0x0	R
[3:0]	VCO_BIAS	VCO Bias Readback. For more information, see the <a href="#">VCO Calibration</a> section.	0x0	R

Address: 0x52, Reset: 0x00, Name: REG0052

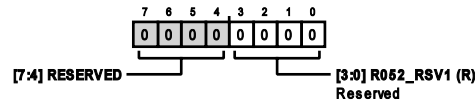


Figure 196.

Table 123. Bit Descriptions for REG0052

Bits	Bit Name	Description	Reset	Access
[7:4]	RESERVED	Reserved.	0x0	R
[3:0]	R052_RSV1	Reserved.	0x0	R

Address: 0x53, Reset: 0x00, Name: REG0053

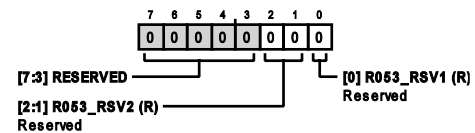


Figure 197.

Table 124. Bit Descriptions for REG0053

Bits	Bit Name	Description	Reset	Access
[7:3]	RESERVED	Reserved.	0x0	R
[2:1]	R053_RSV2	Reserved.	0x0	R
0	R053_RSV1	Reserved.	0x0	R

## REGISTER DETAILS

Address: 0x54, Reset: 0x00, Name: REG0054

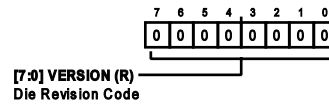


Figure 198.

Table 125. Bit Descriptions for REG0054

Bits	Bit Name	Description	Reset	Access
[7:0]	VERSION	Die Revision Code.	0x0	R

OUTLINE DIMENSIONS

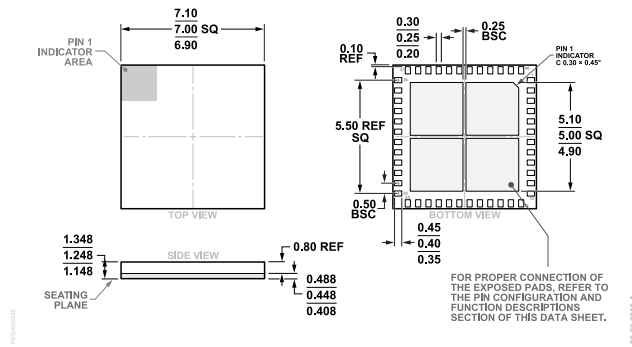


Figure 199. 48-Terminal Land Grid Array [LGA]  
CC-48-6  
Dimensions Shown in millimeters

Updated: November 20, 2023

ORDERING GUIDE

Model <sup>1</sup>	Temperature Range	Package Description	Packing Quantity	Package Option
ADF4378BCCZ	-40°C to +105°C	LGA/CASON/CH ARRAY SO NO LD	Tray, 260	CC-48-6
ADF4378BCCZ-RL7	-40°C to +105°C	LGA/CASON/CH ARRAY SO NO LD	Reel, 500	CC-48-6

<sup>1</sup> Z = RoHS-Compliant Part.

EVALUATION BOARDS

Model <sup>1</sup>	Description
EV-ADF4378SD1Z	Evaluation Board

<sup>1</sup> Z = RoHS-Compliant Part.